

## FEATURES

- Dual Synchronous Step-Up DC/DC Converters
- Delivers 3.3V at 200mA/100mA from one Alkaline/NiMH Cell, or 3.3V at 400mA/200mA from Two Cells
- $V_{IN}$  Start-Up Voltage: 700mV
- 0.5V to 5V  $V_{IN}$  Range after Start-Up
- 1.6V to 5.25V  $V_{OUT}$  Range
- Output Disconnect in Shutdown
- $V_{IN} > V_{OUT}$  Operation
- 1.2MHz or 2.2MHz Operation
- Up to 94% Efficiency
- 12 $\mu$ A Quiescent Current in Burst Mode<sup>®</sup> Operation
- Inrush Current Limiting and Soft-Start
- Internal Synchronous Rectifiers
- Logic-Controlled Shutdown ( $< 2\mu$ A)
- Quick  $V_{OUT}$  Discharge (LTC3527-1)
- 16-Lead, 0.75mm  $\times$  3mm  $\times$  3mm QFN Package

## APPLICATIONS

- MP3/Personal Media Players
- Noise Canceling/Bluetooth Headsets
- Wireless Mice
- Portable Medical Instruments

## DESCRIPTION

The LTC<sup>®</sup>3527/LTC3527-1 are dual high efficiency, step-up DC/DC converters in a space saving 16-lead 3mm  $\times$  3mm QFN package. Battery life is maximized with a 700mV start-up voltage and operation down to 500mV once started. The  $\overline{SHDN}$  and PGOOD pins enable the converters to be sequenced or started together.

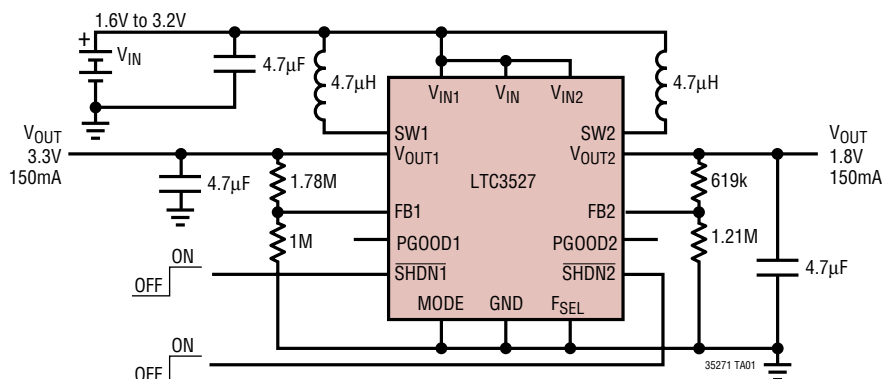
The LTC3527/LTC3527-1 limit inrush current during start-up. Selectable 1.2MHz or 2.2MHz operation provides a choice between the highest efficiency or smallest solution footprint. The current mode PWM design is internally compensated reducing external parts count. Burst Mode operation or fixed frequency operation is selectable via the MODE pin. Anti-ringing circuitry reduces EMI in discontinuous mode. This device also features thermal shutdown.

True output disconnect allows the output to be completely open in shutdown. The LTC3527-1 actively discharges  $V_{OUT1}$  or  $V_{OUT2}$  when its respective  $\overline{SHDN}$  goes low. Quiescent current in shutdown is less than 2 $\mu$ A.

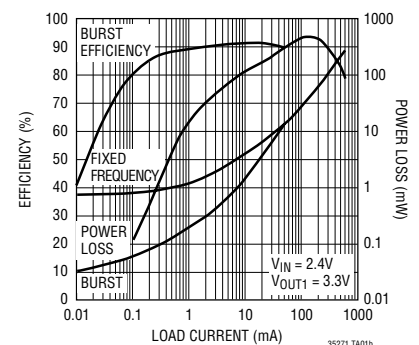
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## TYPICAL APPLICATION

Two-Cell Alkaline to 3.3V/1.8V Synchronous Boost Converters



1.2MHz Efficiency and Power Loss



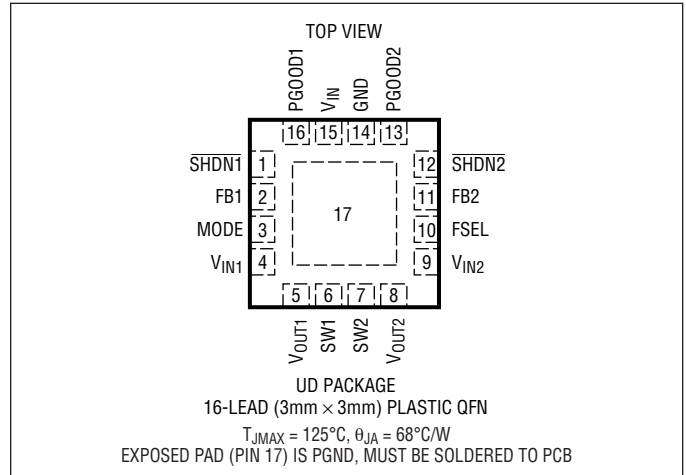
# LTC3527/LTC3527-1

## ABSOLUTE MAXIMUM RATINGS

(Note 1)

$V_{IN}$ , $V_{IN1}$ , $V_{IN2}$ Voltage .....	-0.3V to 6V
SW1, SW2 Voltage (DC) .....	-0.3V to 6V
(Pulsed < 100ns) .....	-0.3V to 7V
SHDN1, SHDN2, FB1, FB2 Voltage.....	-0.3V to 6V
$V_{OUT1}$ , $V_{OUT2}$ .....	-0.3V to 6V
MODE, FSEL, PGOOD1, PGOOD2.....	-0.3V to 6V
Operating Temperature (Notes 2, 5).....	-40°C to 85°C
Junction Temperature .....	125°C
Storage Temperature Range.....	-65°C to 125°C

## PIN CONFIGURATION



## ORDER INFORMATION

LEAD FREE FINISH	TAPE AND REEL	PART MARKING	PACKAGE DESCRIPTION	TEMPERATURE RANGE
LTC3527EUD#PBF	LTC3527EUD#TRPBF	LDDK	16-Lead (3mm x 3mm) Plastic QFN	-40°C to 85°C
LTC3527EUD-1#PBF	LTC3527EUD-1#TRPBF	LCXP	16-Lead (3mm x 3mm) Plastic QFN	-40°C to 85°C
LEAD BASED FINISH	TAPE AND REEL	PART MARKING	PACKAGE DESCRIPTION	TEMPERATURE RANGE
LTC3527EUD	LTC3527EUD#TR	LDDK	16-Lead (3mm x 3mm) Plastic QFN	-40°C to 85°C
LTC3527EUD-1	LTC3527EUD-1#TR	LCXP	16-Lead (3mm x 3mm) Plastic QFN	-40°C to 85°C

Consult LTC Marketing for parts specified with wider operating temperature ranges.

For more information on lead free part marking, go to: <http://www.linear.com/leadfree/>

For more information on tape and reel specifications, go to: <http://www.linear.com/tapeandreel/>

## ELECTRICAL CHARACTERISTICS

The ● denotes the specifications which apply over the full operating temperature range, -40°C to 85°C.  $V_{IN} = 1.2V$ ,  $V_{OUT1} = V_{OUT2} = 3.3V$ ,  $T_A = 25^\circ C$ , unless otherwise noted.

PARAMETER	CONDITIONS	MIN	TYP	MAX	UNITS
Minimum Start-Up Voltage	$I_{LOAD} = 1mA$		0.7	0.88	V
Output Voltage Adjust Range	$V_{OUT1}$	● 1.7		5.25	V
	$V_{OUT1}$ , 0°C to 85°C		1.6	5.25	V
	$V_{OUT2}$	● 1.7		5.25	V
	$V_{OUT2}$ , 0°C to 85°C		1.6	5.25	V
Feedback Voltage FB1, FB2		● 1.176	1.20	1.224	V
Feedback Input Current FB1, FB2	$V_{FB1,2} = 1.20V$		1	50	nA
Quiescent Current: Shutdown	$V_{SHDN1} = V_{SHDN2} = 0V$ , Not Including Switch Leakage, $V_{OUT1} = V_{OUT2} = 0V$		0.1	2	μA
Quiescent Current: Burst Mode Operation	Measured on $V_{OUT}$ , $V_{FB1} = V_{FB2} = 1.5V$		12		μA
Quiescent Current: Active	$V_{FB1} = V_{FB2} > 1.2V$ (Note 3)		500	900	μA
NMOS Switch Leakage Current	$V_{SW1,2} = 5V$ , $SHDN1,2 = 0V$		0.1	10	μA
PMOS Switch Leakage Current	$V_{SW1,2} = 5V$ , $V_{OUT1,2} = 0V$ , $SHDN1,2 = 0V$		0.1	10	μA

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## ELECTRICAL CHARACTERISTICS

The ● denotes the specifications which apply over the full operating temperature range,  $-40^{\circ}\text{C}$  to  $85^{\circ}\text{C}$ .  $V_{\text{IN}} = 1.2\text{V}$ ,  $V_{\text{OUT1}} = V_{\text{OUT2}} = 3.3\text{V}$ ,  $T_{\text{A}} = 25^{\circ}\text{C}$ , unless otherwise noted.

PARAMETER	CONDITIONS	MIN	TYP	MAX	UNITS
NMOS Switch On-Resistance, SW1			0.30		$\Omega$
NMOS Switch On-Resistance, SW2			0.50		$\Omega$
PMOS Switch On-Resistance, SW1			0.40		$\Omega$
PMOS Switch On-Resistance, SW2			0.60		$\Omega$
NMOS Current Limit, SW1		● 800			mA
NMOS Current Limit, SW2		● 400			mA
Current Limit Delay to Output Time	(Note 4)		60		ns
Maximum Duty Cycle	$V_{\text{FB1,2}} = 1\text{V}$	● 85	90		%
Minimum Duty Cycle	$V_{\text{FB1,2}} = 1.3\text{V}$	●		0	%
Switching Frequency	$V_{\text{FSEL}} = 0\text{V}$	● 0.9	1.2	1.5	MHz
Switching Frequency	$V_{\text{FSEL}} = 3.3\text{V}$	● 1.9	2.2	2.8	MHz
SHDN1,2 Input High Voltage		0.88			V
SHDN1,2 Input Low Voltage				0.35	V
SHDN1,2 Input Current	$V_{\text{SHDN1,2}} = 3.3\text{V}$		1	2	$\mu\text{A}$
PGOOD1, PGOOD2 Threshold	Referenced to the Feedback Voltage	-6	-9	-14	%
PGOOD1, PGOOD2 Low Voltage	$I_{\text{PGOOD1,2}} = 1\text{mA}$		0.1	0.2	V
PGOOD1, PGOOD2 Leakage Current	$V_{\text{PGOOD1,2}} = 5.25\text{V}$		0.01	1	$\mu\text{A}$
MODE Input High Voltage		1			V
MODE Input Low Voltage				0.35	V
MODE Input Current	$V_{\text{MODE}} = 3.3\text{V}$		1	2	$\mu\text{A}$
FSEL Input High Voltage		0.88			V
FSEL Input Low Voltage				0.35	V
FSEL Input Current	$V_{\text{FSEL}} = 3.3\text{V}$		1	2	$\mu\text{A}$
Soft-Start Time			0.5		ms

**Note 1:** Stresses beyond those listed under Absolute Maximum Ratings may cause permanent damage to the device. Exposure to any Absolute Maximum Rating condition for extended periods may affect device reliability and lifetime.

**Note 2:** The LTC3527E/LTC3527E-1 are guaranteed to meet performance specifications from  $0^{\circ}\text{C}$  to  $85^{\circ}\text{C}$ . Specifications over the  $-40^{\circ}\text{C}$  to  $85^{\circ}\text{C}$  operating temperature range are assured by design, characterization and correlation with statistical process controls.

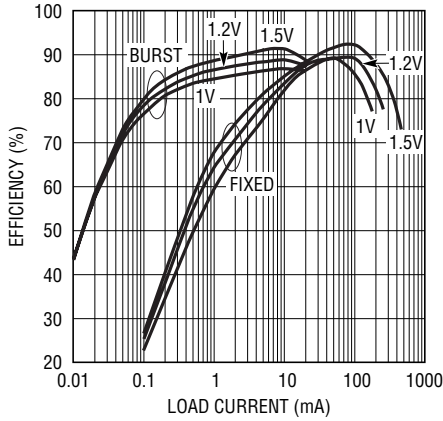
**Note 3:** Current is measured into the  $V_{\text{OUT}}$  pin since the supply current is bootstrapped to the output. The current will reflect to the input supply by:  $(V_{\text{OUT}}/V_{\text{IN}}) \cdot (1/\text{Efficiency})$ . All switches are off.

**Note 4:** Specification is guaranteed by design and not 100% tested in production.

**Note 5:** The LTC3527/LTC3527-1 includes an overtemperature shutdown that is intended to protect the device during momentary overload conditions. Junction temperature will exceed  $125^{\circ}\text{C}$  when the overtemperature shutdown is active. Continuous operation above the specified maximum junction temperature may impair device reliability.

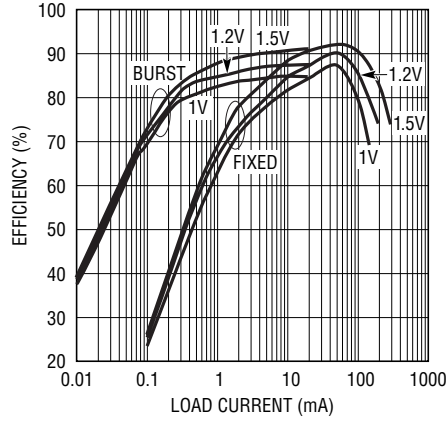
## TYPICAL PERFORMANCE CHARACTERISTICS ( $T_A = 25^\circ\text{C}$ , unless otherwise noted)

**Efficiency vs Load Current and  $V_{IN}$  for  $V_{OUT1} = 1.8\text{V}$  at 1.2MHz**



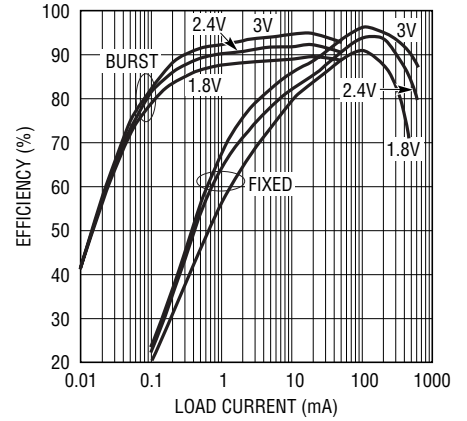
35271 G01

**Efficiency vs Load Current and  $V_{IN}$  for  $V_{OUT2} = 1.8\text{V}$  at 1.2MHz**



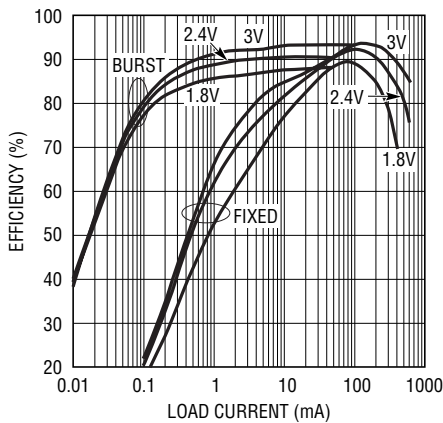
35271 G02

**Efficiency vs Load Current and  $V_{IN}$  for  $V_{OUT1} = 3.3\text{V}$  at 1.2MHz**



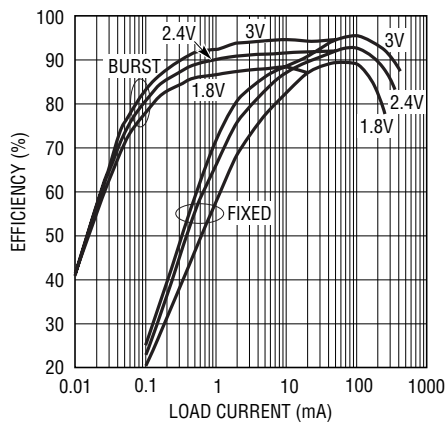
35271 G03

**Efficiency vs Load Current and  $V_{IN}$  for  $V_{OUT1} = 3.3\text{V}$  at 2.2MHz**



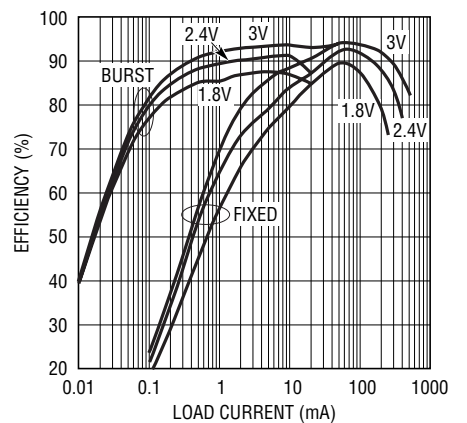
35271 G04

**Efficiency vs Load Current and  $V_{IN}$  for  $V_{OUT2} = 3.3\text{V}$  at 1.2MHz**



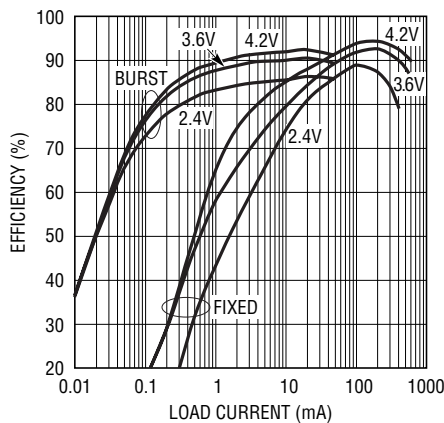
35271 G05

**Efficiency vs Load Current and  $V_{IN}$  for  $V_{OUT2} = 3.3\text{V}$  at 2.2MHz**



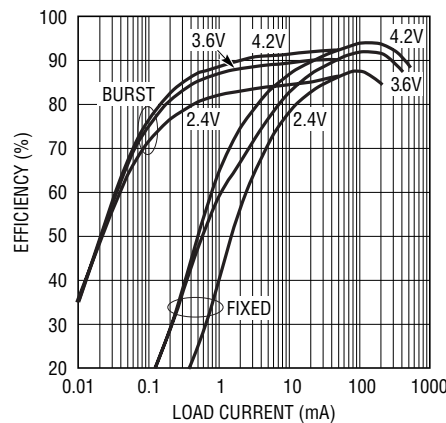
35271 G06

**Efficiency vs Load Current and  $V_{IN}$  for  $V_{OUT1} = 5\text{V}$  at 1.2MHz**



35271 G07

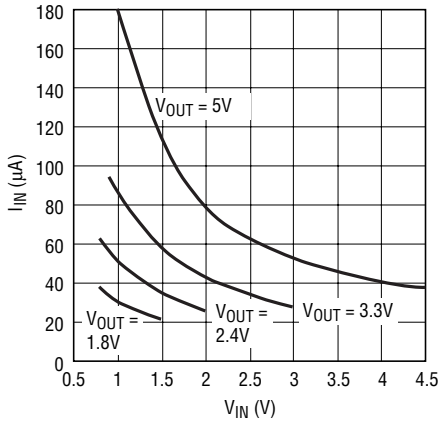
**Efficiency vs Load Current and  $V_{IN}$  for  $V_{OUT2} = 5\text{V}$  at 1.2MHz**



35271 G08

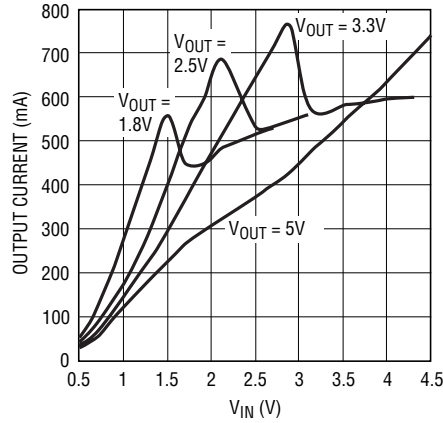
**TYPICAL PERFORMANCE CHARACTERISTICS** ( $T_A = 25^\circ\text{C}$ , unless otherwise noted)

**No-Load Input Current vs  $V_{IN}$**



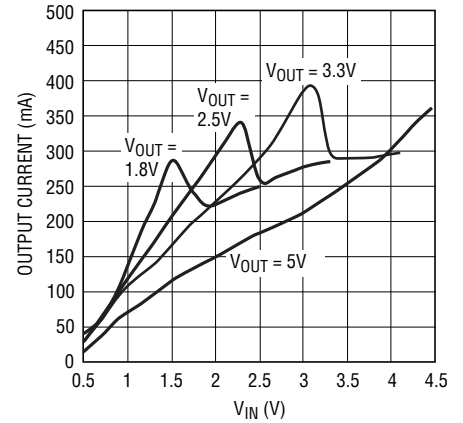
35271 G09

**Maximum Output Current vs  $V_{IN}$  for Converter 1**



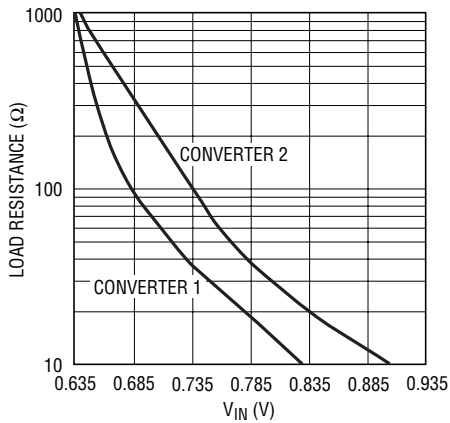
35271 G10

**Maximum Output Current vs  $V_{IN}$  for Converter 2**



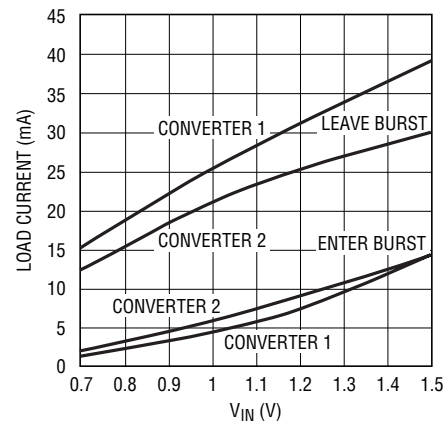
35271 G11

**Minimum Load Resistance During Start-Up vs  $V_{IN}$**



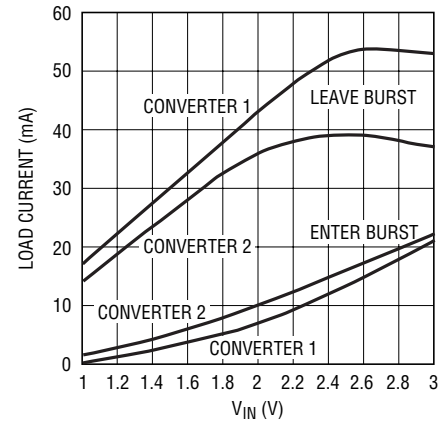
35271 G12

**Burst Mode Threshold Current vs  $V_{IN}$  for  $V_{OUT1} = V_{OUT2} = 1.8\text{V}$**



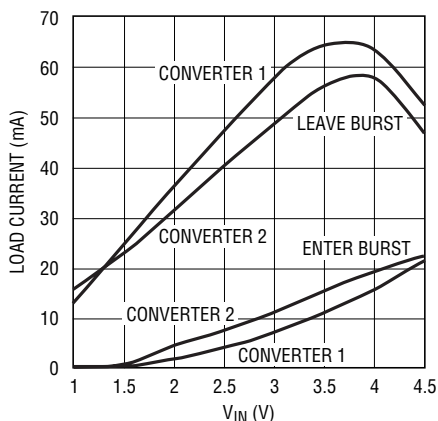
35271 G13

**Burst Mode Threshold Current vs  $V_{IN}$  for  $V_{OUT1} = V_{OUT2} = 3.3\text{V}$**



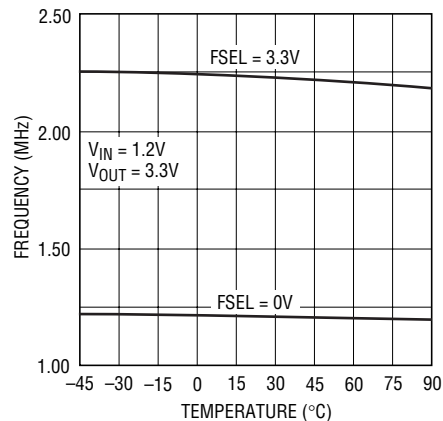
35271 G14

**Burst Mode Threshold Current vs  $V_{IN}$  for  $V_{OUT1} = V_{OUT2} = 5\text{V}$**



35271 G15

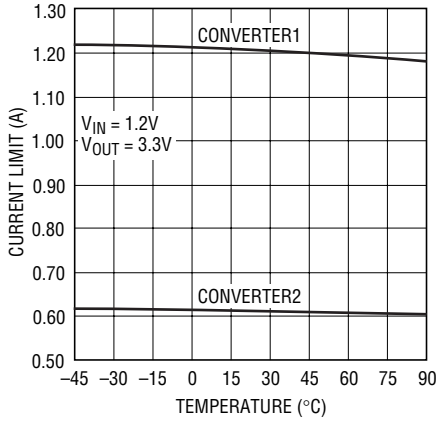
**Oscillator Frequency vs Temperature**



35271 G16

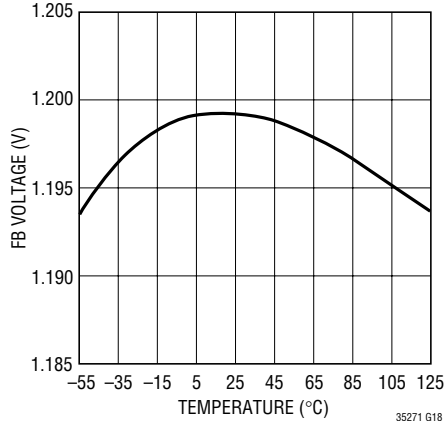
## TYPICAL PERFORMANCE CHARACTERISTICS ( $T_A = 25^\circ\text{C}$ , unless otherwise noted)

### Current Limit vs Temperature



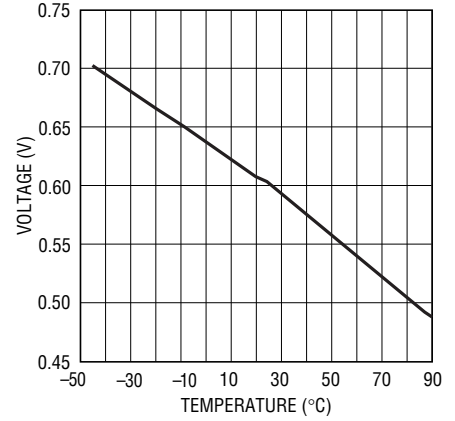
35271 G17

### Feedback Voltage vs Temperature



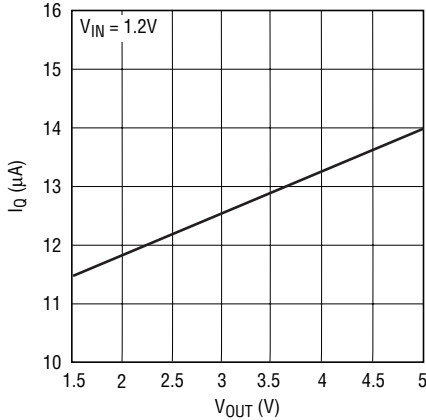
35271 G18

### Start-Up Voltage vs Temperature



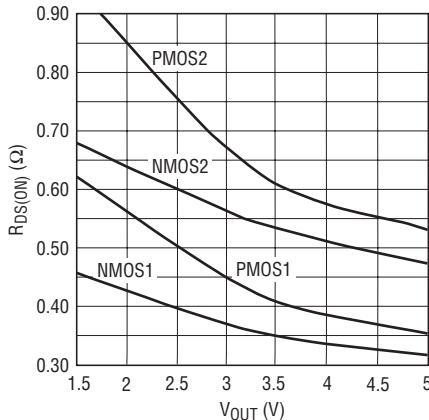
35271 G19

### Burst Mode Quiescent Current vs VOUT



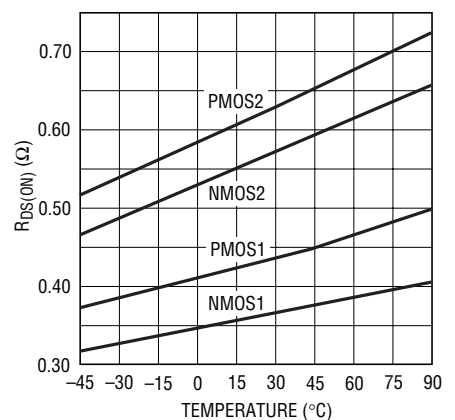
35271 G20

### $R_{DS(ON)}$ (NMOS and PMOS) vs VOUT



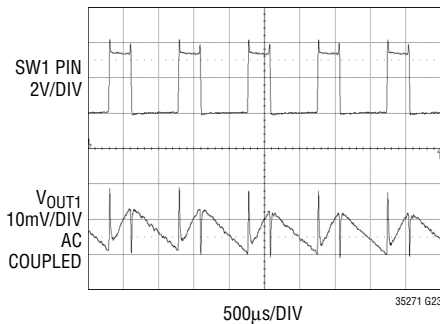
35271 G21

### $R_{DS(ON)}$ (NMOS and PMOS) Change vs Temperature



35271 G22

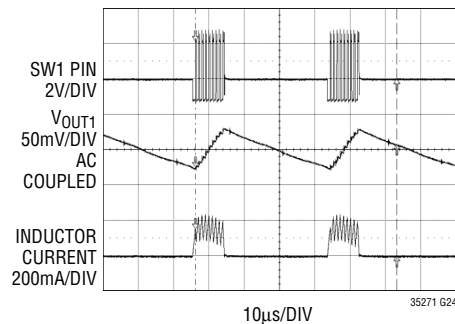
### Fixed Frequency Switching Waveform and $V_{OUT}$ Ripple



35271 G23

$V_{IN1} = 1.2\text{V}$   
 $V_{OUT1} = 3.3\text{V}$  AT 100mA  
 $C_{OUT1} = 10\mu\text{F}$

### Burst Mode Waveforms

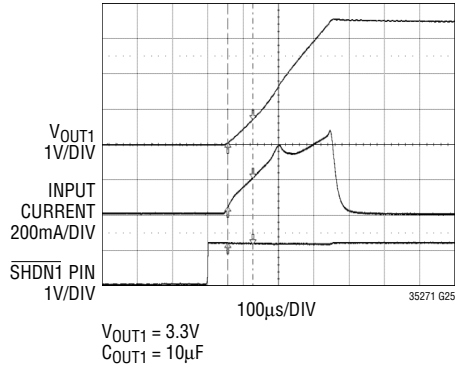


35271 G24

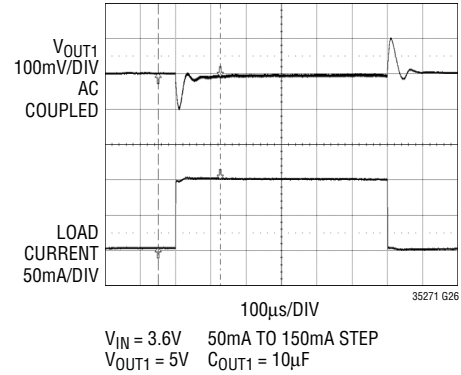
$V_{IN1} = 1.2\text{V}$   
 $V_{OUT1} = 3.3\text{V}$   
 $C_{OUT1} = 10\mu\text{F}$

**TYPICAL PERFORMANCE CHARACTERISTICS** ( $T_A = 25^\circ\text{C}$ , unless otherwise noted)

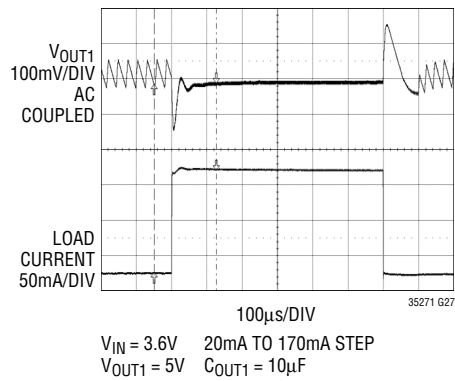
**$V_{OUT1}$  and  $I_{IN}$  During Start-Up**



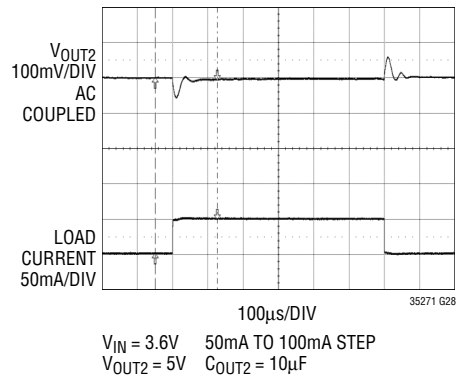
**$V_{OUT1}$  Load Step Response  
Fixed Frequency at 1.2MHz**



**$V_{OUT1}$  Load Step Response  
Burst Mode Operation at 1.2MHz**



**$V_{OUT2}$  Load Step Response  
Fixed Frequency at 2.2MHz**





## PIN FUNCTIONS

**SHDN1 (Pin 1):** Boost Converter 1 Logic-Controlled Shutdown Input. There is an internal  $4M\Omega$  pull-down on this pin.

- $\overline{\text{SHDN1}}$  = High: Normal free running operation, 1.2MHz/2.2MHz typical operating frequency.
- $\overline{\text{SHDN1}}$  = Low: Shutdown, quiescent current  $< 2\mu\text{A}$ .

Note: Both converters must be shut down together to achieve  $< 2\mu\text{A}$  quiescent current.

**FB1 (Pin 2):** Boost Converter 1 Feedback Input to the  $g_m$  Error Amplifier. Connect resistor divider tap to this pin. The output voltage can be adjusted from 1.6V to 5.25V by:

$$V_{\text{OUT1}} = 1.20\text{V} \cdot \left[ 1 + \frac{R1}{R2} \right] \quad (\text{See Block Diagram})$$

**MODE (Pin 3):** Logic-Controlled Mode Input for Both Boost Converters.

- MODE = High: Fixed frequency operation
- MODE = Low: Automatic Burst Mode operation

MODE pin must be 1V or greater to ensure fixed frequency over all operating conditions.

**V<sub>OUT1</sub> (Pin 5):** Boost Converter 1 Output Voltage Sense Input and Drain of the Internal Synchronous Rectifier MOSFET. Driver bias is derived from  $V_{\text{OUT1}}$ . PCB trace length from  $V_{\text{OUT1}}$  to the output filter capacitor(s) should be as short and wide as possible.

**SW1 (Pin 6):** Boost Converter 1 Switch Pin. Connect the inductor between SW1 and  $V_{\text{IN1}}$ . Keep these PCB trace lengths as short and wide as possible to reduce EMI and voltage overshoot. If the inductor current falls to zero or  $\overline{\text{SHDN1}}$  is low, an internal  $100\Omega$  anti-ringing switch is connected from SW1 to  $V_{\text{IN1}}$  to minimize EMI.

**SW2 (Pin 7):** Boost Converter 2 Switch Pin. Connect the inductor between SW2 and  $V_{\text{IN2}}$ . Keep these PCB trace lengths as short and wide as possible to reduce EMI and voltage overshoot. If the inductor current falls to zero or  $\overline{\text{SHDN2}}$  is low, an internal  $100\Omega$  anti-ringing switch is connected from SW2 to  $V_{\text{IN2}}$  to minimize EMI.

**V<sub>OUT2</sub> (Pin 8):** Boost Converter 2 Output Voltage Sense Input and Drain of the Internal Synchronous Rectifier

MOSFET. Driver bias is derived from  $V_{\text{OUT2}}$ . PCB trace length from  $V_{\text{OUT2}}$  to the output filter capacitor(s) should be as short and wide as possible.

**FSEL (Pin 10):** Logic-Controlled Frequency Select Input.

- FSEL = High: 2.2MHz Operation
- FSEL = Low: 1.2MHz Operation

**FB2 (Pin 11):** Boost Converter 2 Feedback Input to the  $g_m$  Error Amplifier. Connect resistor divider tap to this pin. The output voltage can be adjusted from 1.6V to 5.25V by:

$$V_{\text{OUT2}} = 1.20\text{V} \cdot \left[ 1 + \frac{R3}{R4} \right] \quad (\text{See Block Diagram})$$

**SHDN2 (Pin 12):** Boost Converter 2 Logic-Controlled Shutdown Input. There is an internal  $4M\Omega$  pull-down on this pin.

- $\overline{\text{SHDN2}}$  = High: Normal free-running operation, 1.2MHz/2.2MHz typical operating frequency.
- $\overline{\text{SHDN2}}$  = Low: Shutdown, quiescent current  $< 2\mu\text{A}$ .

Note: Both converters must be shut down together to achieve  $< 2\mu\text{A}$  quiescent current.

**PGOOD2 (Pin 13):** Boost Converter 2 Power Good Comparator Output. This open-drain output is low when  $V_{\text{FB}}$  is 9% below its regulation voltage.

**GND (Pin 14):** Signal Ground. This pin is used as a ground reference for the internal circuitry of the LTC3527/LTC3527-1.

**V<sub>IN</sub>, V<sub>IN1</sub>, V<sub>IN2</sub> (Pins 15, 4, 9):** Battery Input Voltage. See Operation section for more information.

**PGOOD1 (Pin 16)** Boost Converter 1 Power Good Comparator Output. This open-drain output is low when  $V_{\text{FB}}$  is 9% below its regulation voltage.

**Exposed Pad (Pin 17):** Backplane. The Exposed Pad is PGND and must be soldered to the PCB ground plane. It serves as the power ground connection for  $V_{\text{OUT1}}$  and  $V_{\text{OUT2}}$ , and as a means of conducting heat away from the package.





## OPERATION (Refer to Block Diagram)

The LTC3527/LTC3527-1 are dual 1.2MHz/2.2MHz synchronous boost converters housed in a 16-lead 3mm × 3mm QFN package. With the ability to start up and operate from inputs less than 880mV, these devices feature fixed frequency, current mode PWM control for exceptional line and load regulation. The current mode architecture with adaptive slope compensation provides excellent transient load response, requiring minimal output filtering. Internal soft-start and loop compensation simplifies the design process while minimizing the number of external components. Each converter has a separate input supply pin and is operated independently of the other, but they share the same oscillator thus providing in-phase switching. If different input supply voltages are used, the third  $V_{IN}$  pin must be wired to the higher of the two supplies and each  $V_{OUT}$  must be higher than the highest  $V_{IN}$ . Bypass capacitors are recommended on all  $V_{IN}$  pins.

With low  $R_{DS(ON)}$  and low gate charge internal N-channel MOSFET switches and P-channel MOSFET synchronous rectifiers, the LTC3527/LTC3527-1 achieve high efficiency over a wide range of load current. With the MODE pin low, automatic Burst Mode operation maintains high efficiency at very light loads, reducing the quiescent current to just 12 $\mu$ A. If MODE is high, fixed frequency PWM switching provides low voltage ripple on the outputs. Operation can be best understood by referring to the Block Diagram.

A PGOOD signal is provided independently for each converter which can be used with the  $\overline{SHDN}$  pins to provide sequencing of the outputs.

The LTC3527-1 provides an instant off feature which discharges  $V_{OUT1}$  or  $V_{OUT2}$  when their respective  $\overline{SHDN}$  pins go low.

A frequency select function allows for 1.2MHz switching (FSEL = Low) or 2.2MHz switching (FSEL = High).

### Low Voltage Start-Up

The LTC3527/LTC3527-1 include an independent start-up oscillator designed to start-up at an input voltage of 0.7V (typical). The two converters can be started together or in either sequence of boost 1 and boost 2 with appropriate control of  $\overline{SHDN1}$  and  $\overline{SHDN2}$ . Soft-start and inrush cur-

rent limiting are provided to each converter independently during start-up, as well as during normal mode.

When  $V_{IN}$ ,  $V_{OUT1}$ , or  $V_{OUT2}$  exceeds 1.4V (typical), the IC enters normal operating mode. Once the higher of  $V_{OUT1}$  or  $V_{OUT2}$  exceeds  $V_{IN}$  by 0.24V, the IC powers itself from the higher  $V_{OUT}$  instead of  $V_{IN}$ . At this point the internal circuitry has no dependency on the  $V_{IN}$  input voltage, eliminating the requirement for a large input capacitor. The input voltage can drop as low as 0.5V.

With single-cell operation, the limiting factor for the application becomes the availability of the power source to supply sufficient energy to the outputs at low voltages, and maximum duty cycle, which is clamped at 90% (typical). Note that at low input voltages, small voltage drops due to the higher series resistance of a depleted cell become critical and greatly limit the power delivery capability of the converter. A higher value, low ESR input capacitor can help to improve this to a small degree.

### Low Noise Fixed Frequency Operation

**Soft-Start:** The LTC3527/LTC3527-1 contain internal circuitry to provide independent soft-start operation to each converter. The soft-start circuitry ramps the peak inductor current from zero to its peak value of 900mA (typical) for converter 1 or 500mA (typical) for converter 2 in approximately 0.5ms, allowing start-up into heavy loads. The soft-start circuitry for both channels is reset in the event of a thermal shutdown or shutdown command.

**Oscillator:** An internal oscillator sets the switching frequency to 1.2MHz if the FSEL pin is below 0.35V, or 2.2MHz if the FSEL pin is above 0.88V.

**Shutdown:** Shutdown is accomplished independently for each converter by pulling its respective  $\overline{SHDN}$  pin below 0.35V, and enabled by pulling each  $\overline{SHDN}$  pin above 0.88V. Note that the  $\overline{SHDN}$  pins can be driven above  $V_{IN}$  or  $V_{OUT}$ , as long as it is limited to less than the absolute maximum rating.

**Error Amplifier:** The non-inverting input of each transconductance error amplifier is internally connected to the 1.20V reference. The inverting inputs are connected to FB1 for converter 1 and FB2 for converter 2. Clamps

## OPERATION

limit the minimum and maximum error amp output voltages for improved large-signal transient response. Power converter control loop compensation is provided internally. An external resistive voltage divider from  $V_{OUT1}$  ( $V_{OUT2}$ ) to ground programs the respective output voltage via FB1 (FB2) from 1.6V to 5.25V.

$$V_{OUT1} = 1.20V \cdot \left[ 1 + \frac{R1}{R2} \right]$$

$$V_{OUT2} = 1.20V \cdot \left[ 1 + \frac{R3}{R4} \right] \quad (\text{See Block Diagram})$$

**Current Sensing:** Lossless current sensing converts the peak current signal of each N-channel MOSFET switch into a voltage which is summed with its corresponding internal slope compensation. The summed signals are compared to their respective error amplifier outputs to provide individual peak current control commands for the PWM of each converter.

**Current Limit:** The current limit comparators shut off the N-channel MOSFET switches once their threshold is reached. Each current limit comparator delay time to output is typically 60ns. Peak switch current is limited to approximately 900mA for converter 1 and 500mA for converter 2, independent of input or output voltage. If  $V_{OUT1}$  or  $V_{OUT2}$  falls below 1V, its respective current limit is cut in half.

**Zero Current Comparator:** The zero current comparators monitor the inductor current to the outputs and shut off the synchronous rectifiers when the current reduces to approximately 30mA. This prevents the inductor current from reversing in polarity, improving efficiency at light loads.

**Synchronous Rectifier:** To control inrush current and to prevent the inductor currents from running away when  $V_{OUT1}$  or  $V_{OUT2}$  is close to  $V_{IN}$ , the P-channel MOSFET synchronous rectifiers are only enabled when their respective  $V_{OUT} > (V_{IN} + 0.24V)$ .

**Anti-Ringing Control:** The anti-ringing control connects a resistor across the inductor to prevent high frequency ringing on the SW1 (SW2) pins during discontinuous current mode operation. Although the ringing of the resonant circuit formed by the inductors and  $C_{SW}$  (capacitance on SW1 or SW2 pins) is low energy, it can cause EMI radiation.

**Output Disconnect:** The LTC3527/LTC3527-1 are designed to allow true output disconnect by eliminating body diode conduction of the internal P-channel MOSFET rectifiers. This allows  $V_{OUT1}$  and  $V_{OUT2}$  to go to zero volts during shutdown, drawing no current from the input source. It also allows for inrush current limiting at turn-on, minimizing surge currents seen by the input supply. Note that to obtain the advantages of output disconnect, there must not be external Schottky diodes connected between the SW1 (SW2) pins and  $V_{OUT1}$  ( $V_{OUT2}$ ). The output disconnect feature also allows  $V_{OUT1}$  or  $V_{OUT2}$  to be pulled high, without any reverse current into a battery on  $V_{IN}$ .

**Thermal Shutdown:** If the die temperature exceeds 160°C, the device will go into thermal shutdown. All switches will be turned off and the soft-start capacitors will be discharged. The device will be enabled again when the die temperature drops by about 15°C.

### Burst Mode Operation

To realize the efficiency benefits of Burst Mode operation, both  $V_{OUT1}$  and  $V_{OUT2}$  must be under a light load current condition, if they are both enabled. If one channel is shut down, then Burst Mode operation is enabled on the other channel. With the MODE pin low, the LTC3527/LTC3527-1 will automatically enter Burst Mode operation at light load and return to fixed frequency PWM mode when the load increases. Refer to the Typical Performance Characteristics to see the Output Load Burst Mode Threshold Current vs  $V_{IN}$ . The load current at which Burst Mode operation is entered can be changed by adjusting the inductor value. Raising the inductor value will lower the load current at which Burst Mode is operation entered.

In Burst Mode operation, the LTC3527/LTC3527-1 still switches at a fixed frequency of 1.2MHz (FSEL = 0) or 2.2MHz (FSEL = 1), using the same error amplifier and loop compensation for peak current mode control. This control method eliminates the output transient when switching between modes. In Burst Mode operation, energy is delivered to the output until it reaches the nominal regulation value, then the LTC3527/LTC3527-1 transitions to sleep mode where the outputs are off and the LTC3527/LTC3527-1 consumes only 12µA of quiescent current from the higher of  $V_{OUT1}$  or  $V_{OUT2}$ . When

## OPERATION

the output voltage droops slightly, switching resumes. This maximizes efficiency at very light loads by minimizing switching and quiescent current losses. Burst Mode output voltage ripple, which is typically 1% peak-to-peak, can be reduced by using more output capacitance (10 $\mu$ F or greater), or with a small capacitor (10pF to 50pF) connected between  $V_{OUT1}$  ( $V_{OUT2}$ ) and FB1 (FB2).

If either load current increases, the LTC3527/LTC3527-1 will automatically leave Burst Mode operation. Note that larger output capacitor values may cause this transition to occur at lighter loads. Once the LTC3527/LTC3527-1

has left Burst Mode operation and returned to normal operation, it will remain there until both output loads are reduced below the burst threshold current.

Burst Mode operation is inhibited during start-up and soft-start and until both  $V_{OUT1}$  and  $V_{OUT2}$  are at least 0.24V greater than  $V_{IN}$  if neither channel is in shutdown.

When the MODE pin is high, LTC3527/LTC3527-1 features continuous PWM fixed frequency operation at 1.2MHz (FSEL = Low) or 2.2MHz (FSEL = High). At very light loads, the LTC3527/LTC3527-1 will exhibit pulse-skip operation.

## APPLICATIONS INFORMATION

### $V_{IN} > V_{OUT}$ Operation

The LTC3527/LTC3527-1 will maintain output voltage regulation even when the input voltage is above one or both of the desired output voltages. Since this mode is less efficient and will dissipate more power in the LTC3527/LTC3527-1, the maximum output current capability is limited in order to maintain an acceptable junction temperature. When operating with  $V_{IN} > V_{OUT}$  the power is defined by:

$$P_{OUT} = I_{OUT} [(V_{IN} + 1.5) - V_{OUT}]$$

To maintain a junction temperature below 125°C, the following formula must be adhered to:

$$(P_{OUT1} + P_{OUT2}) 68^{\circ}\text{C/W} = 125 - T_A$$

where  $T_A$  is the ambient temperature.

### Short-Circuit Protection

The LTC3527/LTC3527-1 output disconnect feature allows an output short-circuit while maintaining a maximum internally set current limit. The converters also incorporate internal features such as current limit foldback and thermal shutdown for protection from an excessive overload or short circuit. To reduce power dissipation under short-circuit conditions, the peak switch current limit is reduced to 500mA (typical) for converter 1 and 350mA (typical) for converter 2 when  $V_{OUT}$  is less than 1V.

### Schottky Diode

Although it is not required, adding a Schottky diode from SW1 (SW2) to  $V_{OUT1}$  ( $V_{OUT2}$ ) will improve efficiency by about 2%. Note that this defeats the output disconnect and short-circuit protection features.

### PCB Layout Guidelines

The high speed operation of the LTC3527/LTC3527-1 demands careful attention to board layout. A careless layout will result in reduced performance. Figure 1 shows the recommended component placement. A large ground pin copper area will help to lower the die temperature. A multilayer board with a separate ground plane is ideal, but not absolutely necessary.

## COMPONENT SELECTION

### Inductor Selection

The LTC3527/LTC3527-1 can utilize small surface mount inductors due to their fast 1.2MHz/2.2MHz switching frequencies. Inductor values between 3.3 $\mu$ H and 4.7 $\mu$ H are suitable for most 1.2MHz applications. Inductor values between 1.5 $\mu$ H and 2.2 $\mu$ H are suitable for most 2.2MHz applications. Larger values of inductance will allow slightly greater output current capability (and lower the Burst

## APPLICATIONS INFORMATION

Mode threshold) by reducing the inductor ripple current. Increasing the inductance above 10 $\mu$ H will increase size while providing little improvement in output current capability.

The minimum inductance value is given by:

$$L > \frac{V_{IN(MIN)} \cdot (V_{OUT(MAX)} - V_{IN(MIN)})}{f \cdot \text{Ripple} \cdot V_{OUT(MAX)}}$$

Where:

Ripple = Allowable inductor current ripple (amps peak-to-peak)

$V_{IN(MIN)}$  = Minimum input voltage

$V_{OUT(MAX)}$  = Maximum output voltage

f = Oscillator frequency (MHz)

The inductor current ripple is typically set for 20% to 40% of the maximum inductor current. High frequency ferrite core inductor materials reduce frequency dependent power losses compared to cheaper powdered iron types, improving efficiency. The inductor should have low ESR

(series resistance of the windings) to reduce the  $I^2R$  power losses, and must be able to support the peak inductor current without saturating. Molded chokes and some chip inductors usually do not have enough core area to support the peak inductor currents of 900mA (500mA) seen on the LTC3527/LTC3527-1. To minimize radiated noise, use shielded inductors. See Table 1 for suggested components and suppliers.

### Output and Input Capacitor Selection

Low ESR (equivalent series resistance) capacitors should be used to minimize output voltage ripple. Multilayer ceramic capacitors are an excellent choice as they have extremely low ESR and are available in small footprints. A 4.7 $\mu$ F to 10 $\mu$ F output capacitor is sufficient for most applications. Larger values up to 22 $\mu$ F may be used to obtain lower output voltage ripple and improve transient response. X5R and X7R dielectric materials are preferred for their ability to maintain capacitance over wide voltage and temperature ranges. Y5V types should not be used.

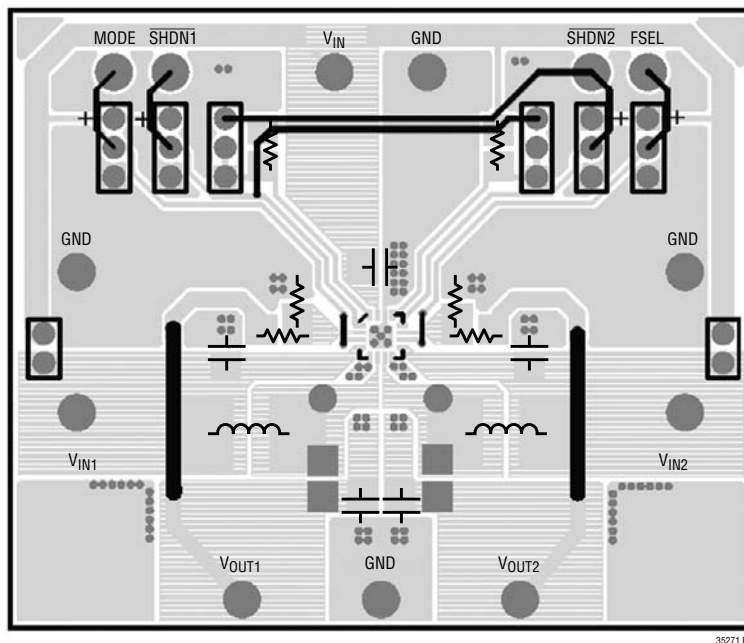


Figure 1. Recommended Component Placement for a Dual-Layer Board



## APPLICATIONS INFORMATION

**Table 1. Recommended Inductors**

VENDOR	PART/STYLE	L( $\mu$ H)	MAXIMUM CURRENT (mA)	DCR ( $\Omega$ )	DIMENSIONS L x W x H (mm)
Coilcraft www.coilcraft.com	MSS5131	2.2-10	1900-870	0.023-0.083	5.1 x 5.1 x 1
	MSS4020	3.3-10	1100-540	0.085-0.210	4 x 4 x 2
	ME3220	1-10	3000-780	0.05-0.90	3.2 x 2.5 x 2
Coiltronics www.cooperet.com	SD10	1-10	1930-760	0.045-0.289	5.2 x 5.2 x 1
	SD12	1.2-10	2450-818	0.037-0.284	5.2 x 5.2 x 1.2
FDK www.fdk.com	MIP3226D	1.5-6.8	1400-1000	0.07-0.12	3.2 x 2.6 x 1
	MIPF2520D	1.5-4.7	1500-1000	0.07-0.11	2.5 x 2 x 1
Murata www.murata.com	LQH43C	1-10	1080-650	0.08-0.24	4.5 x 3.2 x 2.6
	LQH32C	1-4.7	800-650	0.09-0.15	3.2 x 2.5 x 2
Sumida www.sumida.com	CDRH3D16	4.7-15	900-450	0.11-0.29	3.8 x 3.8 x 1.8
	CDRH2D14	4.7-12	680-420	0.12-0.32	3.2 x 3.2 x 1.5
TDK www.global.tdk.co.jp	VLF3010A	1.5-10	1200-490	0.068-0.58	2.6 x 2.8 x 1
	VLF5012A	2.2-10	1500-800	0.090-0.30	4.5 x 4.7 x 1.2
Taiyo Yuden www.t-yuden.com	NR3010	4.7-15	750-400	0.19-0.74	3 x 3 x 1
	NR3015	4.7-15	1000-560	0.12-0.36	3 x 3 x 1.5

The internal loop compensation of the LTC3527/LTC3527-1 is designed to be stable with output capacitor values of 4.7 $\mu$ F or greater. Although ceramic capacitors are recommended, low ESR tantalum capacitors may be used as well.

A small ceramic capacitor in parallel with a larger tantalum capacitor may be used in demanding applications which have large load transients. Another method of improving the transient response is to add a small feed-forward capacitor across the top resistor of the feedback divider [from  $V_{OUT1}$  ( $V_{OUT2}$ ) to FB1 (FB2)]. A typical value of 22pF will generally suffice.

Low ESR input capacitors reduce input switching noise and reduce the peak current drawn from the battery. It follows

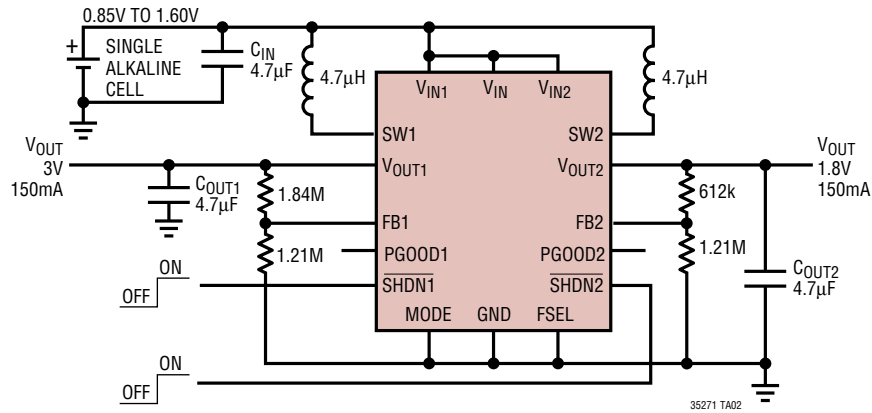
that ceramic capacitors are also a good choice for input decoupling and should be located as close as possible to the device. A 2.2 $\mu$ F input capacitor is sufficient for most applications, although larger values may be used without limitations. Table 2 shows a list of several ceramic capacitor manufacturers. Consult the manufacturers directly for detailed information on their selection of ceramic parts.

**Table 2. Capacitor Vendor Information**

SUPPLIER	PHONE	WEBSITE
AVX	(803) 448-9411	www.avxcorp.com
Murata	(714) 852-2001	www.murata.com
Taiyo-Yuden	(408) 573-4150	www.t-yuden.com
TDK	(847) 803-6100	www.component.tdk.com

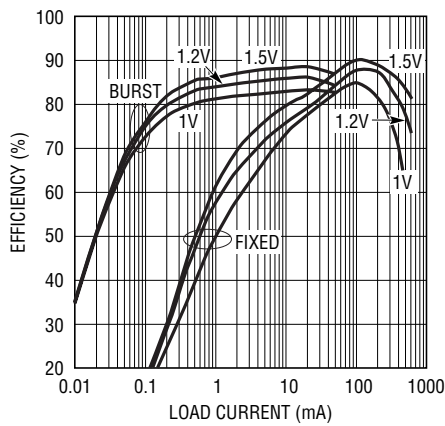
# TYPICAL APPLICATIONS

1.2MHz, 1-Cell to  $V_{OUT1} = 3V$ ,  $V_{OUT2} = 1.8V$



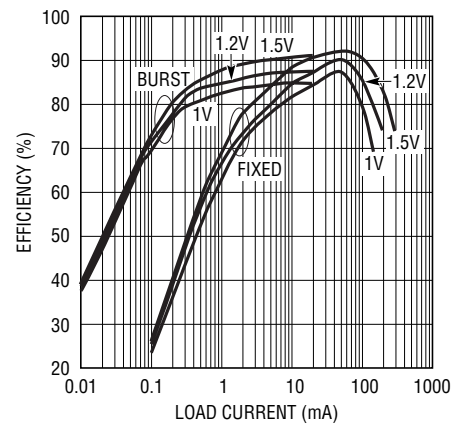
L: SUMIDA CDRH3D164R7  
 $C_{IN}$ ,  $C_{OUT}$ : TAIYO YUDEN X5R JMK212BJ475MD

Boost 1 Efficiency



35271 TA02b

Boost 2 Efficiency

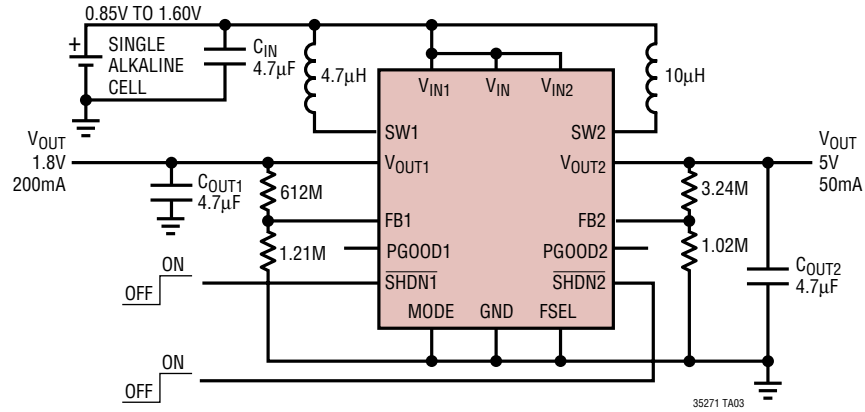


35271 TA02c



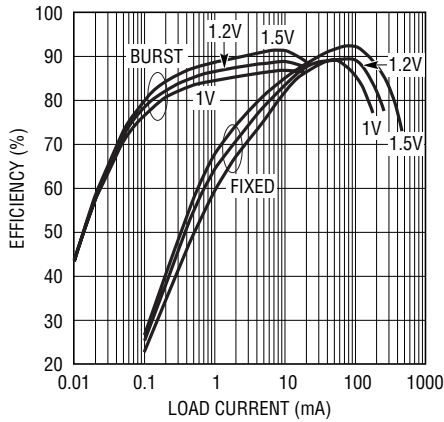
## TYPICAL APPLICATIONS

1.2MHz, 1-Cell to  $V_{OUT1} = 1.8V$ ,  $V_{OUT2} = 5V$



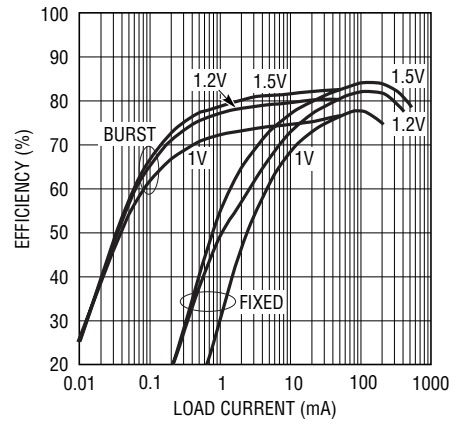
$C_{IN}$ ,  $C_{OUT}$ : TAIYO YUDEN X5R JMK212BJ475MD

**Boost 1 Efficiency**



35271 TA03b

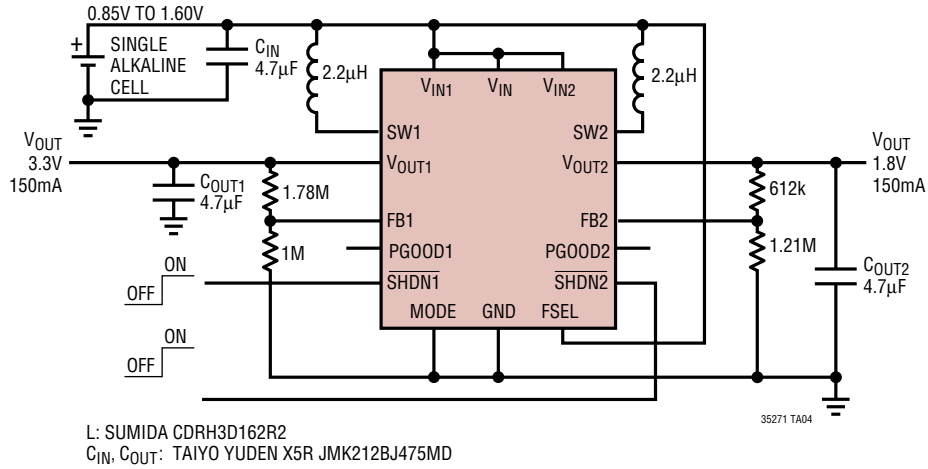
**Boost 2 Efficiency**



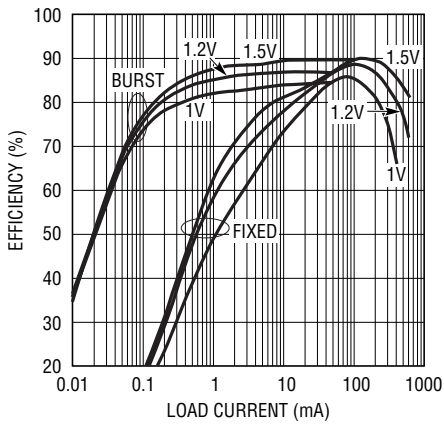
35271 TA03c

# TYPICAL APPLICATIONS

2.2MHz, 1-Cell to  $V_{OUT1} = 3.3V$ ,  $V_{OUT2} = 1.8V$

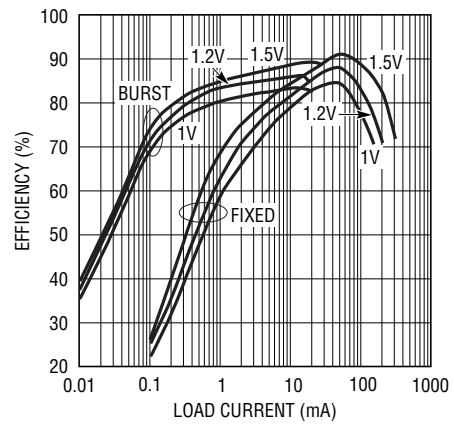


Boost 1 Efficiency



35271 TA04b

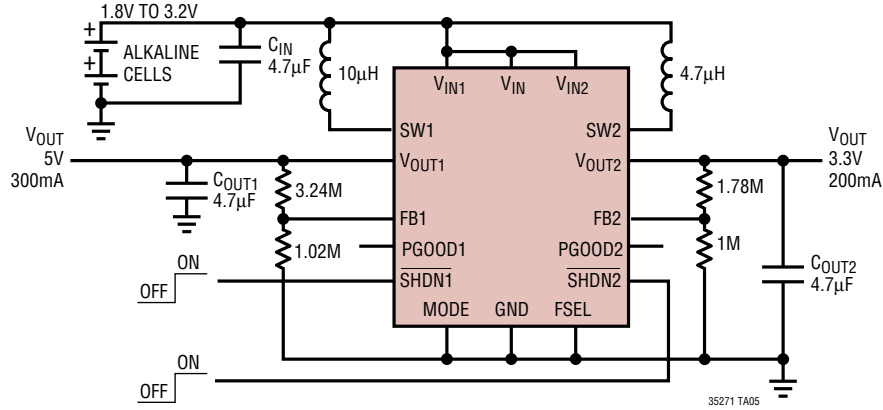
Boost 2 Efficiency



35271 TA04c

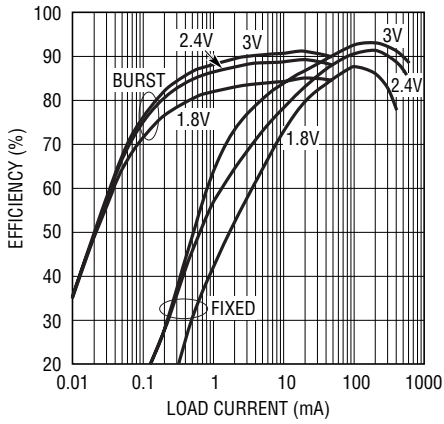
## TYPICAL APPLICATIONS

1.2MHz, 2-Cell to  $V_{OUT1} = 5V$ ,  $V_{OUT2} = 3.3V$

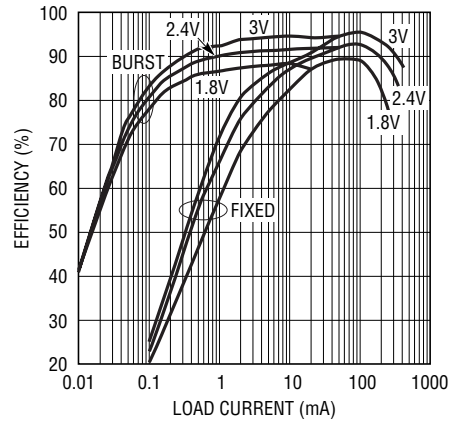


L: SUMIDA CDRH3D164R7  
 C<sub>IN</sub>, C<sub>OUT</sub>: TAIYO YUDEN X5R JMK212BJ475MD

**Boost 1 Efficiency**

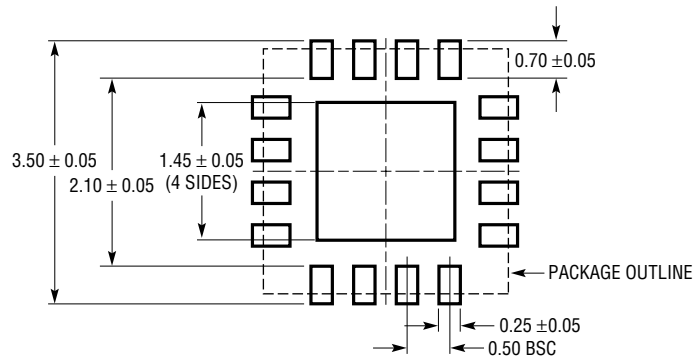


**Boost 2 Efficiency**

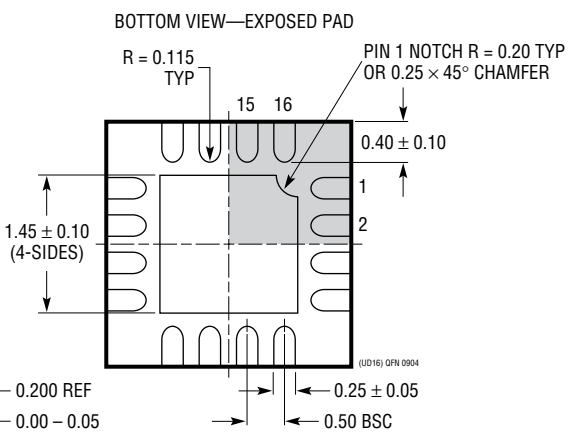
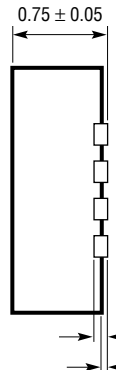
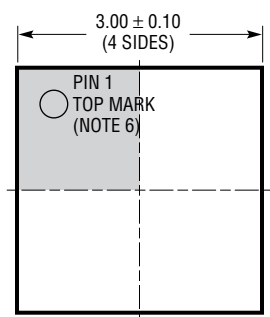


# PACKAGE DESCRIPTION

**UD Package**  
**16-Lead Plastic QFN (3mm × 3mm)**  
 (Reference LTC DWG # 05-08-1691)



RECOMMENDED SOLDER PAD PITCH AND DIMENSIONS

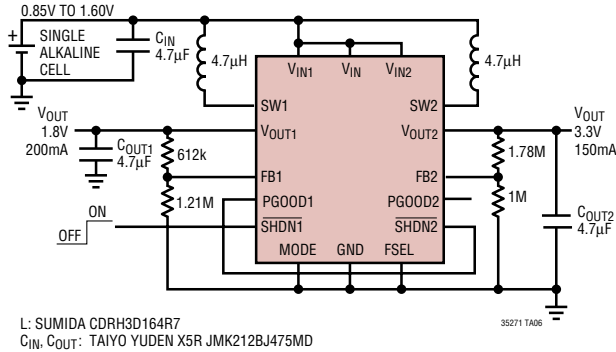


- NOTE:
1. DRAWING CONFORMS TO JEDEC PACKAGE OUTLINE MO-220 VARIATION (WEED-2)
  2. DRAWING NOT TO SCALE
  3. ALL DIMENSIONS ARE IN MILLIMETERS
  4. DIMENSIONS OF EXPOSED PAD ON BOTTOM OF PACKAGE DO NOT INCLUDE MOLD FLASH. MOLD FLASH, IF PRESENT, SHALL NOT EXCEED 0.15mm ON ANY SIDE
  5. EXPOSED PAD SHALL BE SOLDER PLATED
  6. SHADED AREA IS ONLY A REFERENCE FOR PIN 1 LOCATION ON THE TOP AND BOTTOM OF PACKAGE

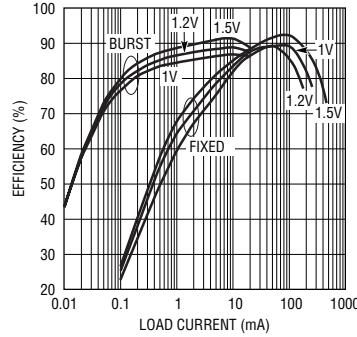
# LTC3527/LTC3527-1

## TYPICAL APPLICATION

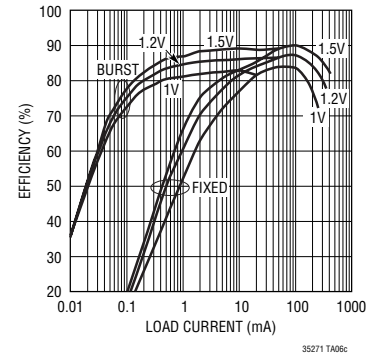
Sequenced Start-Up  $V_{OUT1}$  to  $V_{OUT2}$   
1.2MHz, 1-Cell to  $V_{OUT1} = 1.8V$ ,  $V_{OUT2} = 3.3V$



Boost 1 Efficiency



Boost 2 Efficiency



## RELATED PARTS

PART NUMBER	DESCRIPTION	COMMENTS
LTC3400/ LTC3400B	600mA $I_{SW}$ , 1.2MHz Synchronous Step-Up DC/DC Converters	92% Efficiency, $V_{IN}$ : 0.85V to 5V, $V_{OUT(MAX)}$ = 5V, $I_Q$ = 19µA/300µA, $I_{SD}$ < 1µA, ThinSOT™ Package
LTC3401	1A $I_{SW}$ , 3MHz Synchronous Step-Up DC/DC Converter	97% Efficiency, $V_{IN}$ : 0.5V to 5V, $V_{OUT(MAX)}$ = 6V, $I_Q$ = 38µA, $I_{SD}$ < 1µA, 10-Lead MS Package
LTC3421	3A $I_{SW}$ , 3MHz Synchronous Step-Up DC/DC Converter with Output Disconnect	95% Efficiency, $V_{IN}$ : 0.5V to 4.5V, $V_{OUT(MAX)}$ = 5.25V, $I_Q$ = 12µA, $I_{SD}$ < 1µA, QFN-24 Package
LTC3422	1.5A $I_{SW}$ , 3MHz Synchronous Step-Up DC/DC Converter with Output Disconnect	95% Efficiency, $V_{IN}$ : 0.5V to 4.5V, $V_{OUT(MAX)}$ = 5.25V, $I_Q$ = 25µA, $I_{SD}$ < 1µA, 3mm × 3mm DFN Package
LTC3423/ LTC3424	2A $I_{SW}$ , 3MHz Synchronous Step-Up DC/DC Converter	97% Efficiency, $V_{IN}$ : 0.5V to 5V, $V_{OUT(MAX)}$ = 6V, $I_Q$ = 38µA, $I_{SD}$ < 1µA, 10-Lead MS Package
LTC3426	2A $I_{SW}$ , 1.2MHz Synchronous Step-Up DC/DC Converter	92% Efficiency, $V_{IN}$ : 1.6V to 4.3V, $V_{OUT(MAX)}$ = 5V, $I_{SD}$ < 1µA, SOT-23 Package
LTC3428	500mA $I_{SW}$ , 1.25MHz/2.5MHz Synchronous Step-Up DC/DC Converter with Output Disconnect	92% Efficiency, $V_{IN}$ : 1.8V to 5V, $V_{OUT(MAX)}$ = 5.25V, $I_{SD}$ < 1µA, 2mm × 2mm DFN Package
LTC3429	600mA $I_{SW}$ , 500kHz Synchronous Step-Up DC/DC Converter with Output Disconnect and Soft-Start	96% Efficiency, $V_{IN}$ : 0.5V to 4.4V, $V_{OUT(MAX)}$ = 5V, $I_Q$ = 20µA/300µA, $I_{SD}$ < 1µA, ThinSOT Package
LTC3458	1.4A $I_{SW}$ , 1.5MHz Synchronous Step-Up DC/DC Converter/ Output Disconnect/Burst Mode Operation	93% Efficiency, $V_{IN}$ : 1.5V to 6V, $V_{OUT(MAX)}$ = 7.5V, $I_Q$ = 15µA, $I_{SD}$ < 1µA, DFN-12 Package
LTC3458L	1.7A $I_{SW}$ , 1.5MHz Synchronous Step-Up DC/DC Converter with Output Disconnect, Automatic Burst Mode Operation	94% Efficiency, $V_{OUT(MAX)}$ = 6V, $I_Q$ = 12µA, DFN-12 Package
LTC3459	70mA $I_{SW}$ , 10V Micropower Synchronous Boost Converter/ Output Disconnect/Burst Mode Operation	$V_{IN}$ : 1.5V to 5.5V, $V_{OUT(MAX)}$ = 10V, $I_Q$ = 10µA, $I_{SD}$ < 1µA, ThinSOT Package
LTC3525L-3	500mA $I_{SW}$ , 1.2MHz Synchronous Step-Up DC/DC Converters with Output Disconnect, Automatic Burst Mode Operation	94% Efficiency, $V_{IN}$ : 0.85V to 5V, $V_{OUT(MAX)}$ = 5.25V, $I_Q$ = 7µA, $I_{SD}$ < 1µA, SC70 Package
LTC3526/ LTC3526B	500mA $I_{SW}$ , 1.2MHz Synchronous Step-Up DC/DC Converters with Output Disconnect, Automatic Burst Mode Operation (LTC3526), PWM Only (LTC3526B)	94% Efficiency, $V_{IN}$ : 0.85V to 5V, $V_{OUT(MAX)}$ = 5.25V, $I_Q$ = 10µA/300µA, $I_{SD}$ < 1µA, 2mm × 2mm DFN Package
LTC3528/ LTC3528B	1A, 1MHz Synchronous Step-Up DC/DC Converter with Output Disconnect, Automatic Burst Mode Operation, PWM Only (LTC3528B)	94% Efficiency, $V_{IN}$ : 0.85V to 5V, $V_{OUT(MAX)}$ = 5.25V, $I_Q$ = 10µA/300µA, $I_{SD}$ < 1µA, 2mm × 3mm DFN Package

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