

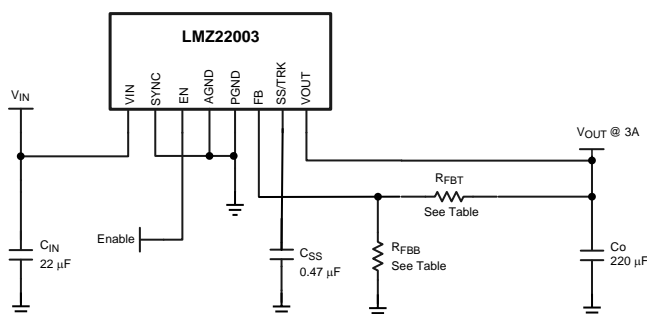
# LMZ22003 3-A SIMPLE SWITCHER® Power Module With 20-V Maximum Input Voltage

## 1 Features

- Integrated Shielded Inductor
- Simple PCB Layout
- Frequency Synchronization Input (650 kHz to 950 kHz)
- Flexible Start-up Sequencing Using External Soft-Start, Tracking and Precision Enable
- Protection Against Inrush Currents and Faults such as Input UVLO and Output Short Circuit
- Junction Temperature Range  $-40^{\circ}\text{C}$  to  $125^{\circ}\text{C}$
- Single Exposed Pad and Standard Pinout for Easy Mounting and Manufacturing
- Fast Transient Response for Powering FPGAs and ASICs
- Fully Enabled for WEBENCH® Power Designer
- Pin Compatible With LMZ23605/LMZ23603/LMZ22005
- Electrical Specifications
  - 18-W Maximum Total Output Power
  - Up to 3-A Output Current
  - Input Voltage Range 6 V to 20 V
  - Output Voltage Range 0.8 V to 6 V
  - Efficiency up to 92%
- Performance Benefits
  - High Efficiency Reduces System Heat Generation
  - Tested To EN55022 Class B<sup>(1)</sup>
  - Low Component Count, Only 5 External Components
  - Low Output Voltage Ripple
  - Uses PCB as Heat Sink, No Airflow Required

NOTE: EN 55022:2006, +A1:2007, FCC Part 15 Subpart B: 2007. See AN-2125 [SNVA473](#) and layout for information on device under test.  $V_{in} = 12\text{ V}$ ,  $V_o = 3.3\text{ V}$ ,  $I_o = 3\text{ A}$

## Simplified Application Schematic



## 2 Applications

- Point-of-load Conversions from 12-V Input Rail
- Time-Critical Projects
- Space Constrained and High Thermal Requirement Applications
- Negative Output Voltage Applications (See AN-2027 [SNVA425](#))

## 3 Description

The LMZ22003 SIMPLE SWITCHER® power module is an easy-to-use step-down DC-DC solution capable of driving up to 3-A load. The LMZ22003 is available in an innovative package that enhances thermal performance and allows for hand or machine soldering.

The LMZ22003 can accept an input voltage rail between 6 V and 20 V and can deliver an adjustable and highly accurate output voltage as low as 0.8 V. The LMZ22003 only requires two external resistors and three external capacitors to complete the power solution. The LMZ22003 is a reliable and robust design with the following protection features: thermal shutdown, programmable input undervoltage lockout, output overvoltage protection, short circuit protection, output current limit, and this device allows start-up into a prebiased output. The sync input allows synchronization over the 650- to 950-kHz switching frequency range.

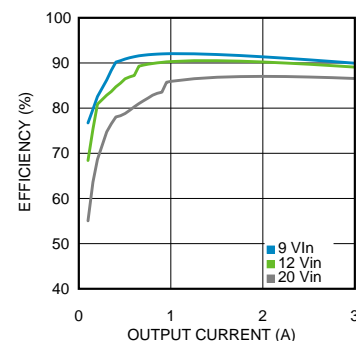
### Device Information<sup>(1)(2)</sup>

PART NUMBER	PACKAGE	BODY SIZE (NOM)
LMZ22003	NDW (7)	10.16 mm x 9.85 mm

(1) For all available packages, see the orderable addendum at the end of the data sheet.

(2) Peak reflow temperature equals  $245^{\circ}\text{C}$ . See [SNAA214](#) for more details.

## Efficiency 5-V Output at 25°C Ambient



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## 4 Revision History

NOTE: Page numbers for previous revisions may differ from page numbers in the current version.

### Changes from Revision H (October 2013) to Revision I

Page

- Added *ESD Ratings* table, *Feature Description* section, *Device Functional Modes*, *Application and Implementation* section, *Power Supply Recommendations* section, *Layout* section, *Device and Documentation Support* section, and *Mechanical, Packaging, and Orderable Information* section. ....

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### Changes from Revision G (March 2013) to Revision H

Page

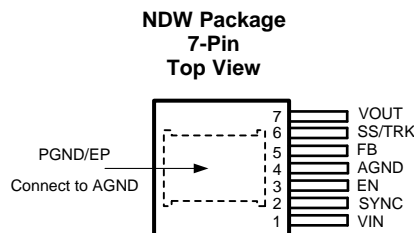
- Deleted 10 mil.....
- Changed 10 mil .....
- Added *Power Module SMT Guidelines*.....

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25

## 5 Pin Configuration and Functions



### Pin Functions

PIN		TYPE	DESCRIPTION
NAME	NO.		
AGND	4	Ground	Analog Ground — Reference point for all stated voltages. Must be externally connected to PGND (EP).
EN	3	Analog	Enable — Input to the precision enable comparator. Rising threshold is 1.279 V typical. Once the module is enabled, a 21- $\mu$ A source current is internally activated to facilitate programmable hysteresis.
FB	5	Analog	Feedback — Internally connected to the regulation amplifier, overvoltage comparators. The regulation reference point is 0.796 V at this input pin. Connect the feedback resistor divider between the output and AGND to set the output voltage.
PGND	—	Ground	Exposed Pad / Power Ground Electrical path for the power circuits within the module. — NOT Internally connected to AGND / pin 4. Used to dissipate heat from the package during operation. Must be electrically connected to pin 4 external to the package.
SS/TRK	6	Analog	Soft-Start/Track — To extend the 1.6-ms internal soft-start connect an external soft-start capacitor. For tracking connect to an external resistive divider connected to a higher priority supply rail. See <a href="#">Design Steps</a> section
SYNC	2	Analog	Sync Input — Apply a CMOS logic level square wave whose frequency is between 650 kHz and 950 kHz to synchronize the PWM operating frequency to an external frequency source. When not using synchronization connect to ground. The module free-running PWM frequency is 812 kHz (typical).
VIN	1	Power	Supply input — Nominal operating range is 6 V to 20 V. A small amount of internal capacitance is contained within the package assembly. Additional external input capacitance is required between this pin and exposed pad (PGND).
VOUT	7	Power	Output Voltage — Output from the internal inductor. Connect the output capacitor between this pin and exposed pad.

## 6 Specifications

### 6.1 Absolute Maximum Ratings

over operating free-air temperature range (unless otherwise noted)<sup>(1)</sup> <sup>(2)</sup><sup>(3)</sup>

	MIN	MAX	UNIT
VIN to PGND	-0.3	24	V
EN, SYNC to AGND	-0.3	5.5	V
SS/TRK, FB to AGND	-0.3	2.5	V
AGND to PGND	-0.3	0.3	V
Junction temperature		150	°C
Peak reflow case temperature (30 sec)		245	°C
Storage temperature, T <sub>stg</sub>	-65	150	°C

- (1) Stresses beyond those listed under *Absolute Maximum Ratings* may cause permanent damage to the device. These are stress ratings only, which do not imply functional operation of the device at these or any other conditions beyond those indicated under *Recommended Operating Conditions*. Exposure to absolute-maximum-rated conditions for extended periods may affect device reliability.
- (2) If Military/Aerospace specified devices are required, please contact the Texas Instruments Sales Office/ Distributors for availability and specifications.
- (3) For soldering specifications, refer to the following document: [SNOA549](#)

## 6.2 ESD Ratings

		VALUE	UNIT
$V_{(ESD)}$	Electrostatic discharge	Human body model (HBM), per ANSI/ESDA/JEDEC JS-001 <sup>(1)</sup>	±2000 V

(1) JEDEC document JEP155 states that 500-V HBM allows safe manufacturing with a standard ESD control process.

## 6.3 Recommended Operating Conditions

over operating free-air temperature range (unless otherwise noted)

	MIN	MAX	UNIT
$V_{IN}$	6	20	V
EN, SYNC	0	5	V
Operation junction temperature	–40	125	°C

## 6.4 Thermal Information

THERMAL METRIC <sup>(1)</sup>		LMZ22003		UNIT
		NDW		
		7 PINS		
$R_{\theta JA}$	Junction-to-ambient thermal resistance <sup>(2)</sup>	4-layer Evaluation Printed-Circuit-Board, 60 vias, No air flow	12.0	°C/W
		2-layer JEDEC Printed-Circuit-Board, No air flow	21.5	
$R_{\theta JC(top)}$	Junction-to-case (top) thermal resistance	No air flow	1.9	°C/W

- (1) For more information about traditional and new thermal metrics, see the *Semiconductor and IC Package Thermal Metrics* application report, [SPRA953](#).
- (2)  $R_{\theta JA}$  measured on a 3.5-in × 3.5-in 4-layer board, with 3-oz. copper on outer layers and 2-oz. copper on inner layers, sixty thermal vias, no air flow, and 1-W power dissipation. Refer to application note layout diagrams.

## 6.5 Electrical Characteristics

Minimum and Maximum limits are ensured through test, design, or statistical correlation. Typical values represent the most likely parametric norm at  $T_J = 25^\circ\text{C}$ , and are provided for reference purposes only. Unless otherwise stated the following conditions apply:  $V_{IN} = 12\text{ V}$ ,  $V_{OUT} = 3.3\text{ V}$ .

PARAMETER	TEST CONDITIONS	MIN <sup>(1)</sup>	TYP <sup>(2)</sup>	MAX <sup>(1)</sup>	UNIT
<b>SYSTEM PARAMETERS</b>					
<b>ENABLE CONTROL</b>					
$V_{EN}$	EN threshold trip point	$V_{EN}$ rising, $T_J = 25^\circ\text{C}$		1.279	V
		$V_{EN}$ rising, $T_J = -40^\circ\text{C}$ to $+125^\circ\text{C}$		1.1      1.458	
$V_{EN-HYS}$	EN input hysteresis current	$V_{EN} > 1.279\text{ V}$		–21	µA
<b>SOFT-START</b>					
$I_{SS}$	SS source current	$V_{SS} = 0\text{ V}$ , $T_J = 25^\circ\text{C}$		50	µA
		$V_{SS} = 0\text{ V}$ , $T_J = -40^\circ\text{C}$ to $+125^\circ\text{C}$		40      50      60	
$t_{SS}$	Internal soft-start interval			1.6	ms
<b>CURRENT LIMIT</b>					
$I_{CL}$	Current limit threshold	DC average, $T_J = -40^\circ\text{C}$ to $+125^\circ\text{C}$		3.4	A

- (1) Minimum and Maximum limits are 100% production tested at  $25^\circ\text{C}$ . Limits over the operating temperature range are ensured through correlation using Statistical Quality Control (SQC) methods. Limits are used to calculate Average Outgoing Quality Level (AOQL).
- (2) Typical numbers are at  $25^\circ\text{C}$  and represent the most likely parametric norm.

## Electrical Characteristics (continued)

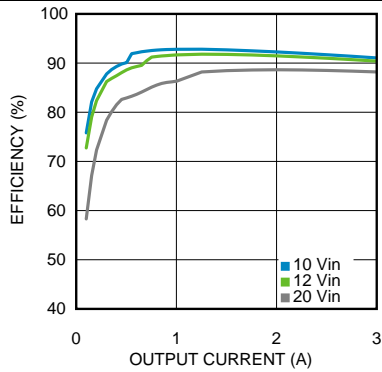
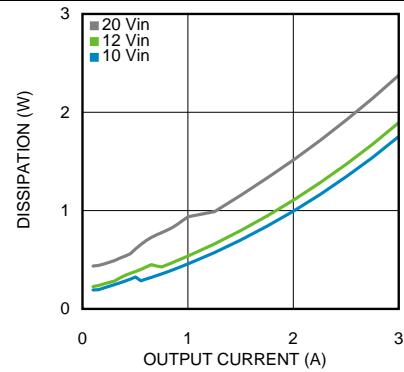
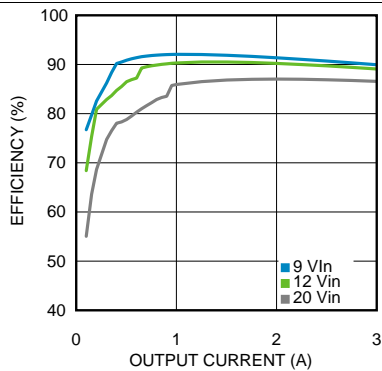
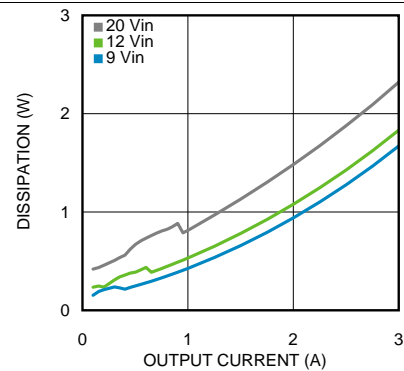
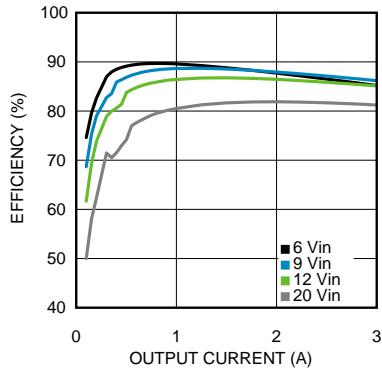
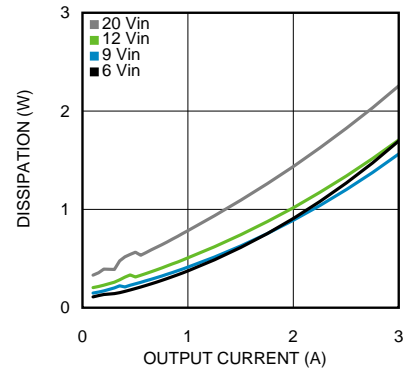
Minimum and Maximum limits are ensured through test, design, or statistical correlation. Typical values represent the most likely parametric norm at  $T_J = 25^\circ\text{C}$ , and are provided for reference purposes only. Unless otherwise stated the following conditions apply:  $V_{IN} = 12\text{ V}$ ,  $V_{OUT} = 3.3\text{ V}$ .

PARAMETER		TEST CONDITIONS	MIN <sup>(1)</sup>	TYP <sup>(2)</sup>	MAX <sup>(1)</sup>	UNIT
<b>INTERNAL SWITCHING OSCILLATOR</b>						
$f_{osc}$	Free-running oscillator frequency	Sync input connected to ground.	711	812	914	kHz
$f_{sync}$	Synchronization range		650		950	kHz
$V_{IL-sync}$	Synchronization logic zero amplitude	Relative to AGND, $T_J = -40^\circ\text{C}$ to $+125^\circ\text{C}$			0.4	V
$V_{IH-sync}$	Synchronization logic one amplitude	Relative to AGND, $T_J = -40^\circ\text{C}$ to $+125^\circ\text{C}$	1.5			V
Sync <sub>dc</sub>	Synchronization duty cycle range		15%	50%	85%	
$D_{max}$	Maximum Duty Factor			83%		
<b>REGULATION AND OVER-VOLTAGE COMPARATOR</b>						
$V_{FB}$	In-regulation feedback voltage	$V_{SS} >+ 0.8\text{ V}$ , $I_O = 3\text{ A}$ , $T_J = 25^\circ\text{C}$	0.796			V
		$V_{SS} >+ 0.8\text{ V}$ , $I_O = 3\text{ A}$ , $T_J = -40^\circ\text{C}$ to $+125^\circ\text{C}$	0.776		0.816	
$V_{FB-OV}$	Feedback overvoltage protection threshold			0.86		V
$I_{FB}$	Feedback input bias current			5		nA
$I_Q$	Non-switching input current	$V_{FB} = 0.86\text{ V}$		2.6		mA
$I_{SD}$	Shutdown quiescent current	$V_{EN} = 0\text{ V}$		70		$\mu\text{A}$
<b>THERMAL CHARACTERISTICS</b>						
$T_{SD}$	Thermal shutdown	Rising		165		$^\circ\text{C}$
$T_{SD-HYST}$	Thermal shutdown hysteresis	Falling		15		$^\circ\text{C}$
<b>PERFORMANCE PARAMETERS<sup>(3)</sup></b>						
$\Delta V_O$	Output voltage ripple	$C_{out} = 220\text{ }\mu\text{F}$ with $7\text{ m}\Omega$ ESR + $100\text{ }\mu\text{F}$ X7R + $2 \times 0.047\text{ }\mu\text{F}$ BW at $20\text{ MHz}$		9		mV <sub>PP</sub>
$\Delta V_O/\Delta V_{IN}$	Line regulation	$V_{IN} = 12\text{ V}$ to $20\text{ V}$ , $I_O = 0.001\text{ A}$		$\pm 0.02\%$		
$\Delta V_O/\Delta I_{OUT}$	Load regulation	$V_{IN} = 12\text{ V}$ , $I_O = 0.001\text{ A}$ to $3\text{ A}$		1		mV/A
$\eta$	Peak efficiency	$V_{IN} = 12\text{ V}$ , $V_O = 3.3\text{ V}$ , $I_O = 1\text{ A}$		86%		
$\eta$	Full load efficiency	$V_{IN} = 12\text{ V}$ , $V_O = 3.3\text{ V}$ , $I_O = 3\text{ A}$		85%		

(3) Refer to BOM in [Table 1](#).

## 6.6 Typical Characteristics

Unless otherwise specified, the following conditions apply:  $V_{IN} = 12V$ ;  $C_{IN} = 2 \times 10 \mu F + 1\text{-}\mu F$  X7R Ceramic;  $C_O = 220\text{-}\mu F$  Specialty Polymer +  $10\text{-}\mu F$  Ceramic;  $T_A = 25^\circ C$  for waveforms. Efficiency and dissipation plots marked with \* have cycle skipping at light loads resulting in slightly higher Output ripple – See [Design Steps](#) section.


**Figure 1. Efficiency 6-V Output at 25°C Ambient**

**Figure 2. Dissipation 6-V Output at 25°C Ambient**

**Figure 3. Efficiency 5-V Output at 25°C Ambient**

**Figure 4. Dissipation 5-V Output at 25°C Ambient**

**Figure 5. Efficiency 3.3-V Output at 25°C Ambient**

**Figure 6. Dissipation 3.3-V Output at 25°C Ambient**

### Typical Characteristics (continued)

Unless otherwise specified, the following conditions apply:  $V_{IN} = 12V$ ;  $C_{IN} = 2 \times 10 \mu F + 1-\mu F$  X7R Ceramic;  $C_O = 220-\mu F$  Specialty Polymer +  $10-\mu F$  Ceramic;  $T_A = 25^\circ C$  for waveforms. Efficiency and dissipation plots marked with \* have cycle skipping at light loads resulting in slightly higher Output ripple – See [Design Steps](#) section.

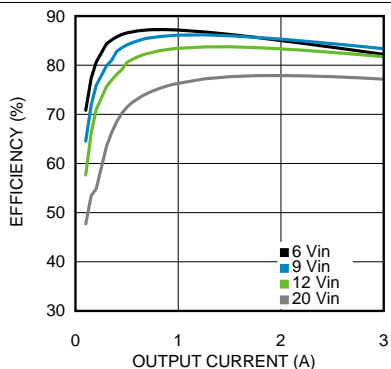


Figure 7. Efficiency 2.5-V Output at 25°C Ambient

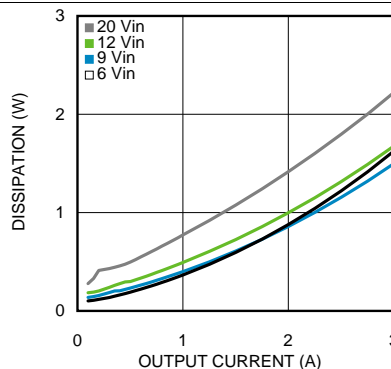


Figure 8. Dissipation 2.5-V Output at 25°C Ambient

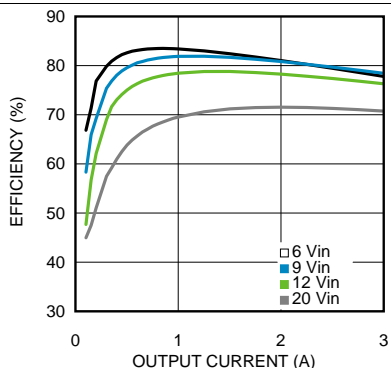


Figure 9. Efficiency 1.8-V Output at 25°C Ambient

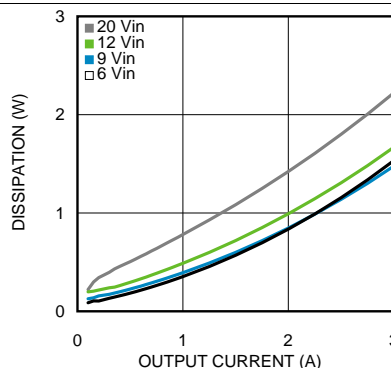


Figure 10. Dissipation 1.8-V Output at 25°C Ambient

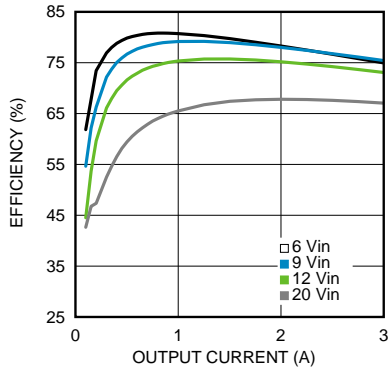


Figure 11. Efficiency 1.5-V Output at 25°C Ambient

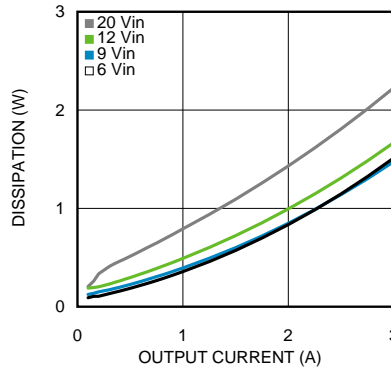


Figure 12. Dissipation 1.5-V Output at 25°C Ambient

### Typical Characteristics (continued)

Unless otherwise specified, the following conditions apply:  $V_{IN} = 12V$ ;  $C_{IN} = 2 \times 10 \mu F + 1-\mu F$  X7R Ceramic;  $C_O = 220-\mu F$  Specialty Polymer +  $10-\mu F$  Ceramic;  $T_A = 25^\circ C$  for waveforms. Efficiency and dissipation plots marked with \* have cycle skipping at light loads resulting in slightly higher Output ripple – See [Design Steps](#) section.

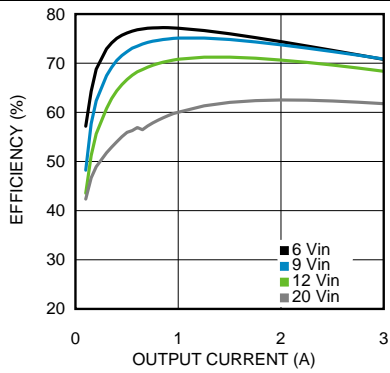


Figure 13. Efficiency 1.2-V Output at 25°C Ambient

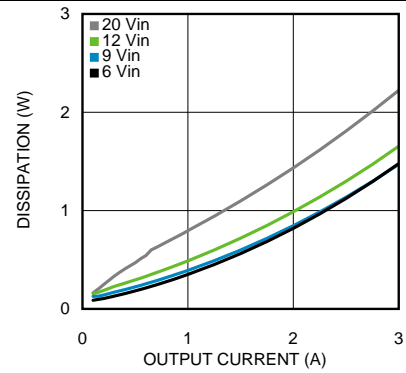


Figure 14. Dissipation 1.2-V Output at 25°C Ambient

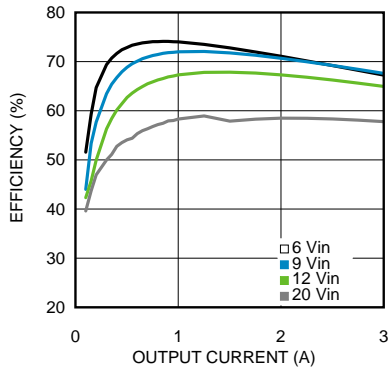


Figure 15. Efficiency 1-V Output at 25°C Ambient

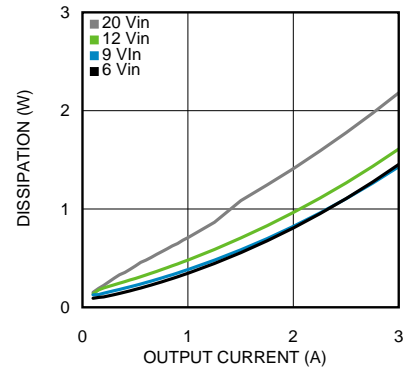


Figure 16. Dissipation 1-V Output at 25°C Ambient

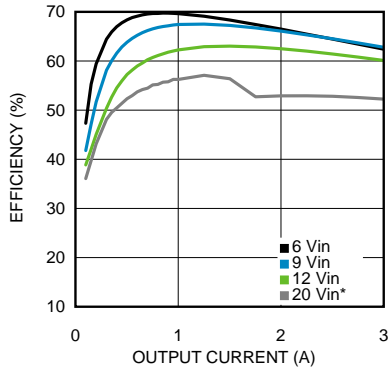


Figure 17. Efficiency 0.8-V Output at 25°C Ambient

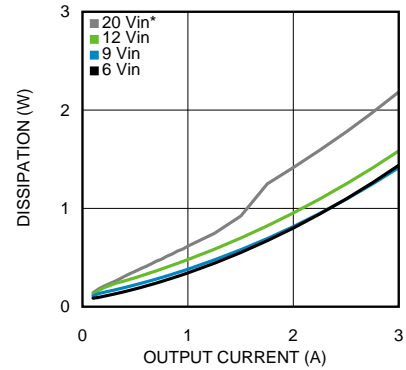


Figure 18. Dissipation 0.8-V Output at 25°C Ambient



Typical Characteristics (continued)

Unless otherwise specified, the following conditions apply:  $V_{IN} = 12V$ ;  $C_{IN} = 2 \times 10 \mu F + 1\text{-}\mu F$  X7R Ceramic;  $C_O = 220\text{-}\mu F$  Specialty Polymer +  $10\text{-}\mu F$  Ceramic;  $T_A = 25^\circ C$  for waveforms. Efficiency and dissipation plots marked with \* have cycle skipping at light loads resulting in slightly higher Output ripple – See [Design Steps](#) section.

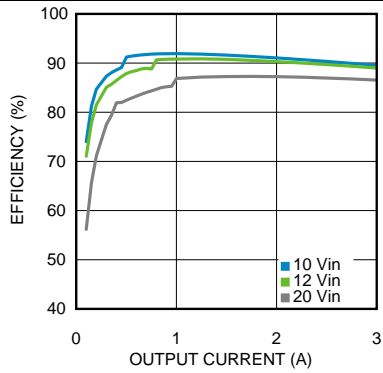


Figure 19. Efficiency 6-V Output at 85°C Ambient

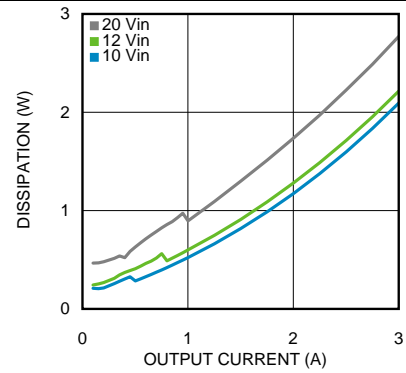


Figure 20. Dissipation 6-V Output at 85°C Ambient

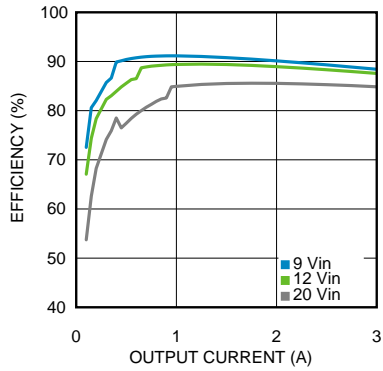


Figure 21. Efficiency 5-V Output at 85°C Ambient

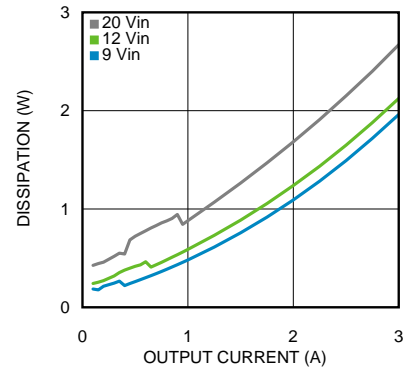


Figure 22. Dissipation 5-V Output at 85°C Ambient

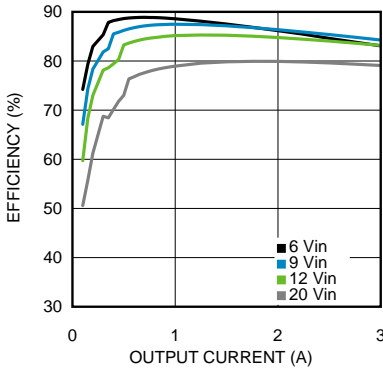


Figure 23. Efficiency 3.3-V Output at 85°C Ambient

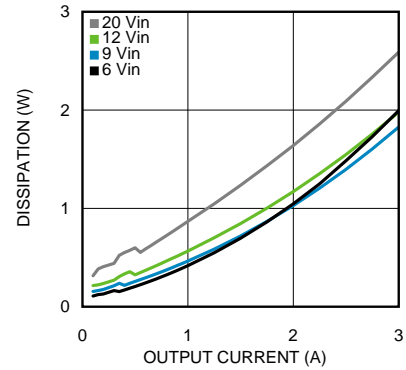


Figure 24. Dissipation 3.3-V Output at 85°C Ambient

### Typical Characteristics (continued)

Unless otherwise specified, the following conditions apply:  $V_{IN} = 12V$ ;  $C_{IN} = 2 \times 10 \mu F + 1-\mu F$  X7R Ceramic;  $C_O = 220-\mu F$  Specialty Polymer +  $10-\mu F$  Ceramic;  $T_A = 25^\circ C$  for waveforms. Efficiency and dissipation plots marked with \* have cycle skipping at light loads resulting in slightly higher Output ripple – See [Design Steps](#) section.

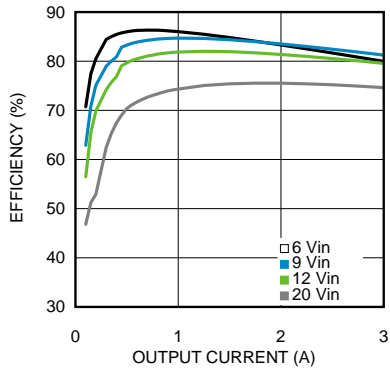


Figure 25. Efficiency 2.5-V Output at 85°C Ambient

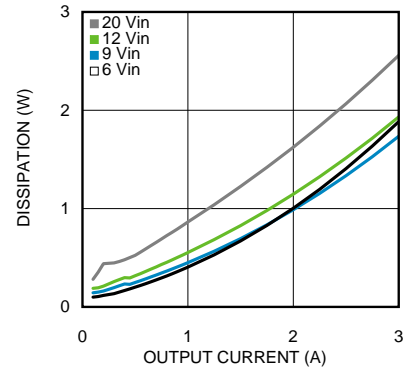


Figure 26. Dissipation 2.5-V Output at 85°C Ambient

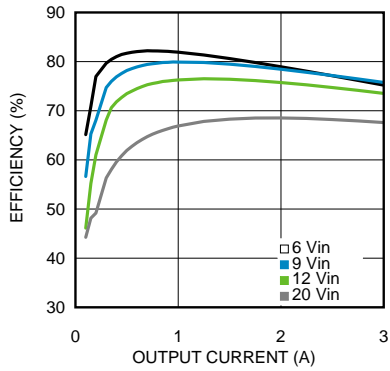


Figure 27. Efficiency 1.8-V Output at 85°C Ambient

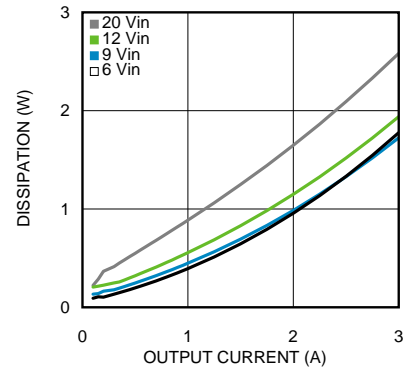


Figure 28. Dissipation 1.8-V Output at 85°C Ambient

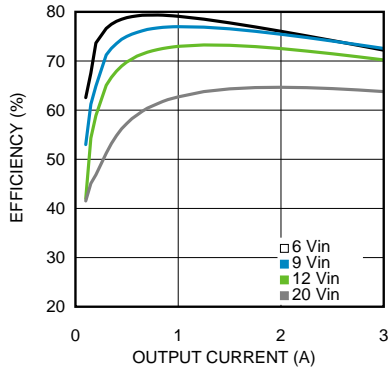


Figure 29. Efficiency 1.5-V Output at 85°C Ambient

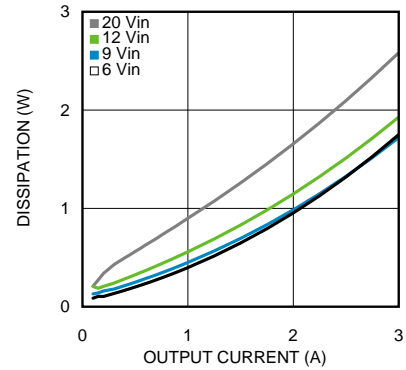


Figure 30. Dissipation 1.5-V Output at 85°C Ambient

Typical Characteristics (continued)

Unless otherwise specified, the following conditions apply:  $V_{IN} = 12V$ ;  $C_{IN} = 2 \times 10 \mu F + 1-\mu F$  X7R Ceramic;  $C_O = 220-\mu F$  Specialty Polymer +  $10-\mu F$  Ceramic;  $T_A = 25^\circ C$  for waveforms. Efficiency and dissipation plots marked with \* have cycle skipping at light loads resulting in slightly higher Output ripple – See [Design Steps](#) section.

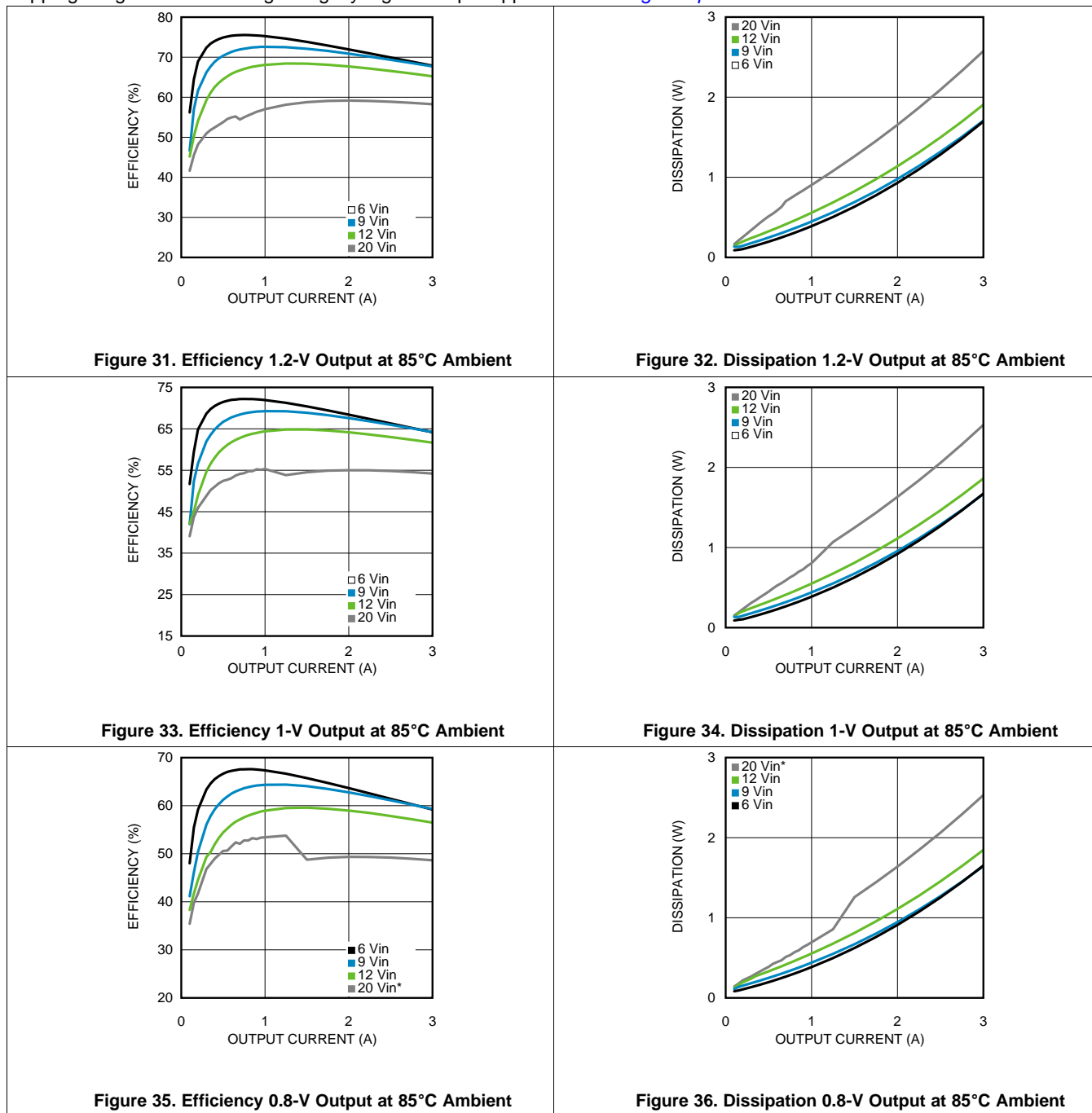


Figure 31. Efficiency 1.2-V Output at 85°C Ambient

Figure 32. Dissipation 1.2-V Output at 85°C Ambient

Figure 33. Efficiency 1-V Output at 85°C Ambient

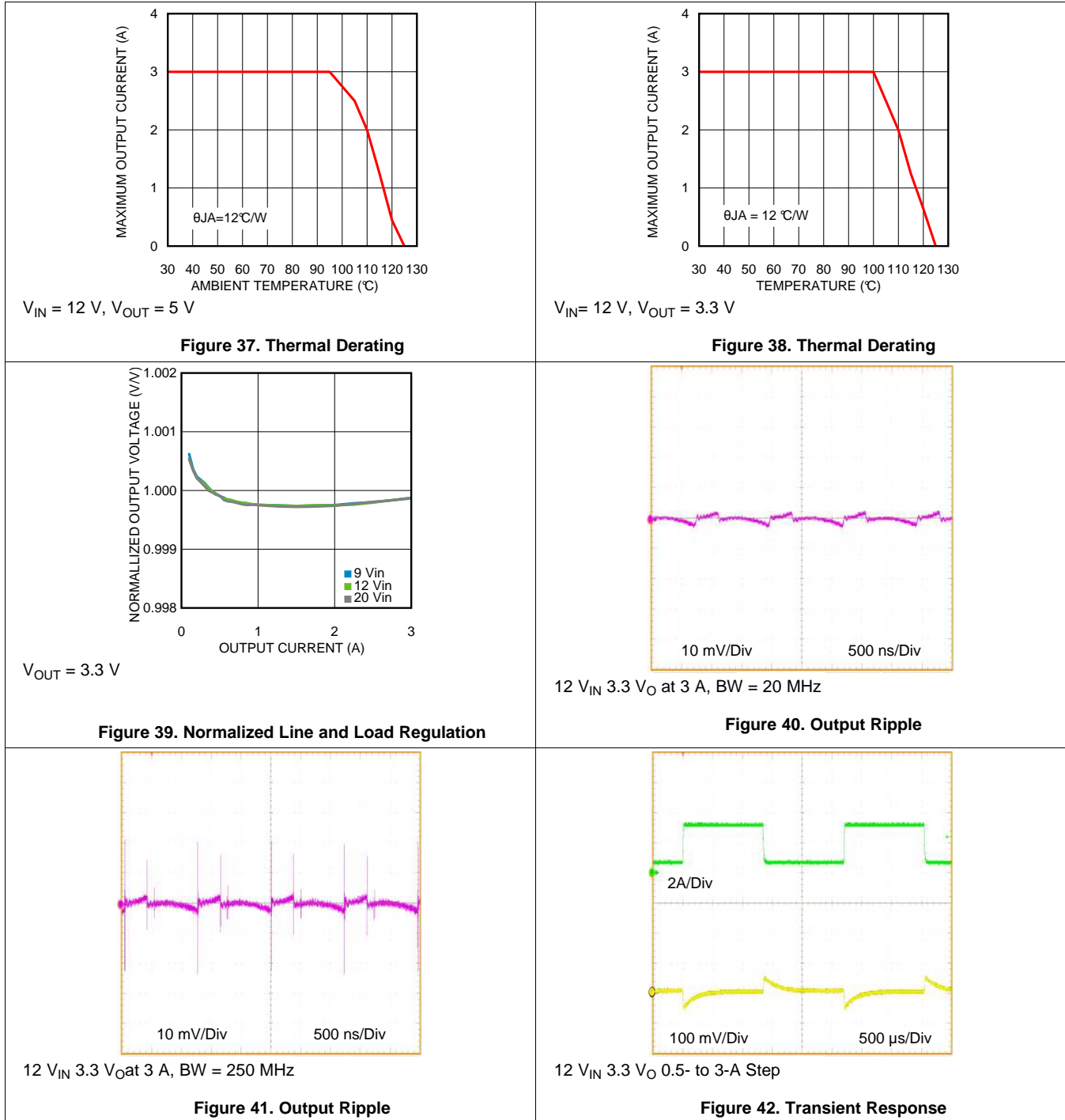
Figure 34. Dissipation 1-V Output at 85°C Ambient

Figure 35. Efficiency 0.8-V Output at 85°C Ambient

Figure 36. Dissipation 0.8-V Output at 85°C Ambient

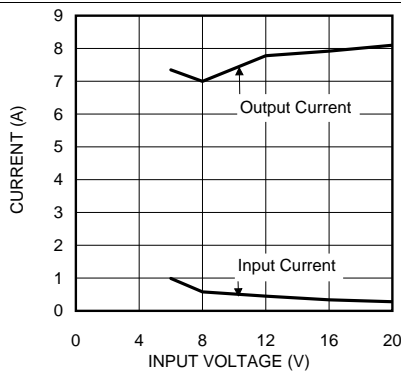
**Typical Characteristics (continued)**

Unless otherwise specified, the following conditions apply:  $V_{IN} = 12V$ ;  $C_{IN} = 2 \times 10 \mu F + 1-\mu F$  X7R Ceramic;  $C_O = 220-\mu F$  Specialty Polymer +  $10-\mu F$  Ceramic;  $T_A = 25^\circ C$  for waveforms. Efficiency and dissipation plots marked with \* have cycle skipping at light loads resulting in slightly higher Output ripple – See [Design Steps](#) section.



### Typical Characteristics (continued)

Unless otherwise specified, the following conditions apply:  $V_{IN} = 12V$ ;  $C_{IN} = 2 \times 10 \mu F + 1\text{-}\mu F$  X7R Ceramic;  $C_O = 220\text{-}\mu F$  Specialty Polymer +  $10\text{-}\mu F$  Ceramic;  $T_A = 25^\circ C$  for waveforms. Efficiency and dissipation plots marked with \* have cycle skipping at light loads resulting in slightly higher Output ripple – See [Design Steps](#) section.



**Figure 43. Short Circuit Current vs Input Voltage**

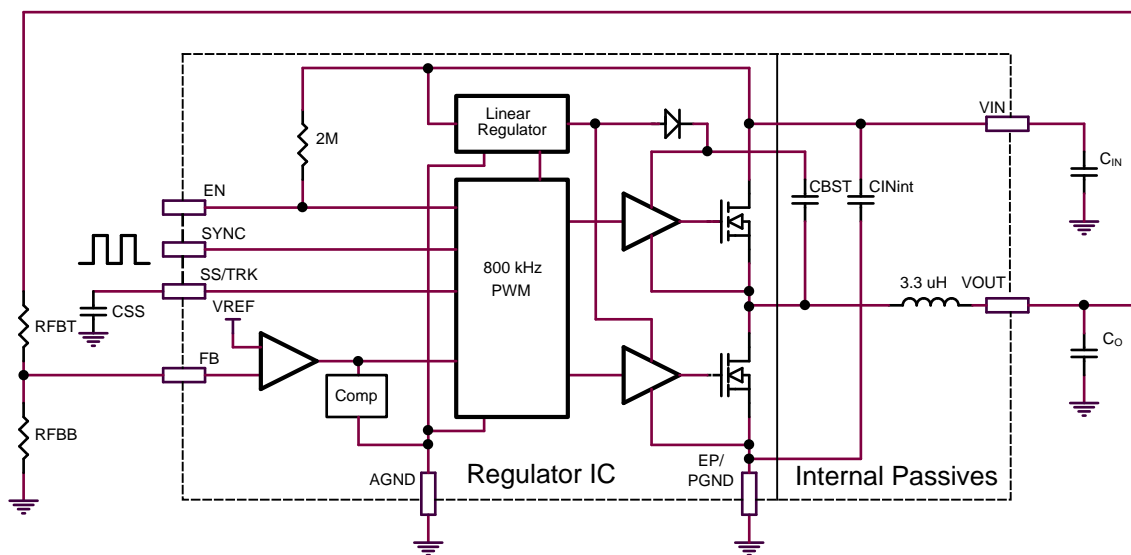
## 7 Detailed Description

### 7.1 Overview

The architecture used is an internally compensated emulated peak current mode control, based on a monolithic synchronous SIMPLE SWITCHER core capable of supporting high load currents. The output voltage is maintained through feedback compared with an internal 0.8-V reference. For emulated peak current-mode, the valley current is sampled on the down-slope of the inductor current. This is used as the DC value of current to start the next cycle.

The primary application for emulated peak current-mode is high input voltage to low output voltage operating at a narrow duty cycle. By sampling the inductor current at the end of the switching cycle and adding an external ramp, the minimum ON-time can be significantly reduced, without the need for blanking or filtering which is normally required for peak current-mode control.

### 7.2 Functional Block Diagram



### 7.3 Feature Description

#### 7.3.1 Synchronization Input

The PWM switching frequency can be synchronized to an external frequency source. If this feature is not used, connect this input either directly to ground, or connect to ground through a resistor of 1.5 k $\Omega$  or less. The allowed synchronization frequency range is 650 kHz to 950 kHz. The typical input threshold is 1.4-V transition level. Ideally the input clock should overdrive the threshold by a factor of 2, so direct drive from 3.3-V logic through a 1.5-k $\Omega$  Thevenin source resistance is recommended.

**NOTE**

Applying a sustained logic 1 corresponds to zero Hz PWM frequency and will cause the module to stop switching.

#### 7.3.2 Output Over-voltage Protection

If the voltage at FB is greater than a 0.86-V internal reference, the output of the error amplifier is pulled toward ground, causing  $V_O$  to fall.

## Feature Description (continued)

### 7.3.3 Current Limit

The LMZ22003 is protected by both low-side (LS) and high-side (HS) current limit circuitry. The LS current limit detection is carried out during the OFF-time by monitoring the current through the LS synchronous MOSFET. Referring to the [Functional Block Diagram](#), when the top MOSFET is turned off, the inductor current flows through the load, the PGND pin and the internal synchronous MOSFET. If this current exceeds the low-side current limit value, the current limit comparator disables the start of the next switching period. Switching cycles are prohibited until current drops below the limit.

#### NOTE

DC current limit is dependent on both duty cycle as shown in the graph in the [Typical Characteristics](#) section.

The HS current limit monitors the current of top side MOSFET. Once HS current limit is detected, the HS MOSFET is shutoff immediately, until the next cycle. Exceeding HS current limit causes  $V_O$  to fall. Typical behavior of exceeding LS current limit is that  $f_{SW}$  drops to 1/2 of the operating frequency.

### 7.3.4 Thermal Protection

The junction temperature of the LMZ22003 should not be allowed to exceed its maximum ratings. Thermal protection is implemented by an internal Thermal Shutdown circuit which activates at 165°C (typical) causing the device to enter a low power standby state. In this state the main MOSFET remains off causing  $V_O$  to fall, and additionally the  $C_{SS}$  capacitor is discharged to ground. Thermal protection helps prevent catastrophic failures for accidental device overheating. When the junction temperature falls back below 150°C (typical hysteresis = 15°C) the SS pin is released,  $V_O$  rises smoothly, and normal operation resumes.

Applications requiring maximum output current especially those at high input voltage may require additional derating at elevated temperatures.

### 7.3.5 Prebiased Start-Up

The LMZ22003 will properly start up into a prebiased output. This start-up situation is common in multiple rail logic applications where current paths may exist between different power rails during the start-up sequence. [Figure 44](#) shows proper behavior in this mode. Trace one is Enable going high. Trace two is 1.5-V prebias rising to 3.3 V. Rise-time determined by  $C_{SS}$ , trace three.

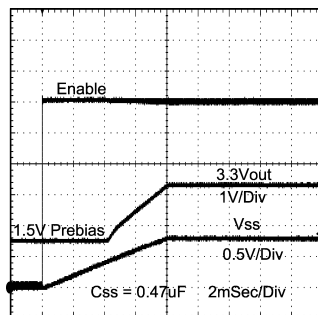


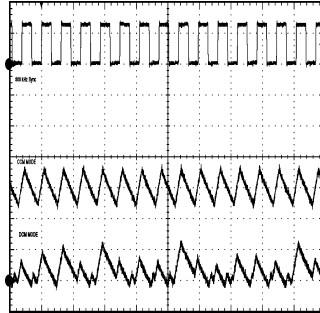
Figure 44. Prebiased Start-Up

## 7.4 Device Functional Modes

### 7.4.1 Discontinuous Conduction and Continuous Conduction Modes

At light load the regulator will operate in discontinuous conduction mode (DCM). With load currents above the critical conduction point, it will operate in continuous conduction mode (CCM). In CCM, current flows through the inductor through the entire switching cycle and never falls to zero during the OFF-time. When operating in DCM, inductor current is maintained to an average value equaling  $I_{OUT}$ . Inductor current exhibits normal behavior for the emulated current mode control method used. Output voltage ripple typically increases during this mode of operation.

Figure 45 is a comparison pair of waveforms of the showing both CCM (upper) and DCM operating modes.



$V_{IN} = 12\text{ V}$ ,  $V_O = 3.3\text{ V}$ ,  $I_O = 3\text{ A} / 0.3\text{ A}$  2  $\mu\text{s}/\text{div}$

**Figure 45. CCM and DCM Operating Modes**



## 8 Application and Implementation

### NOTE

Information in the following applications sections is not part of the TI component specification, and TI does not warrant its accuracy or completeness. TI's customers are responsible for determining suitability of components for their purposes. Customers should validate and test their design implementation to confirm system functionality.

### 8.1 Application Information

The LMZ22003 is a step-down DC-to-DC power module. It is typically used to convert a higher DC voltage to a lower DC voltage with a maximum output current of 3 A. The following design procedure can be used to select components for the LMZ22003. Alternately, the WEBENCH software may be used to generate complete designs.

When generating a design, the WEBENCH software uses iterative design procedure and accesses comprehensive databases of components. Please go to [www.ti.com](http://www.ti.com) for more details.

### 8.2 Typical Application

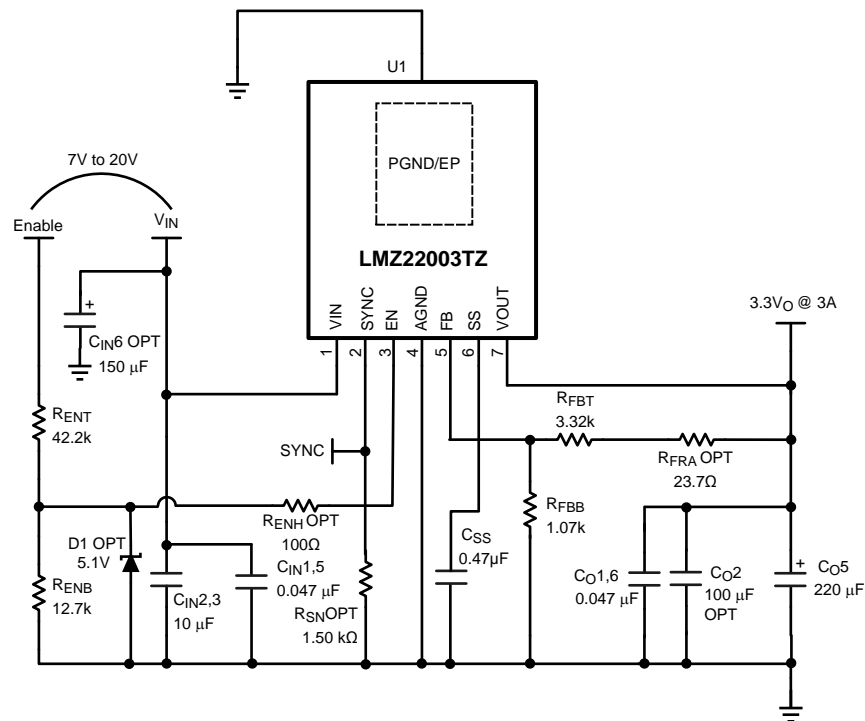


Figure 46. Typical Application Schematic

#### 8.2.1 Design Requirements

For this example the following application parameters exist:

- $V_{IN}$  Range = Up to 20 V
- $V_{OUT}$  = 0.8 V to 6 V
- $I_{OUT}$  = 3 A

## Typical Application (continued)

### 8.2.2 Detailed Design Procedure

#### 8.2.2.1 Design Steps

The LMZ22003 is fully supported by WEBENCH which offers: component selection, electrical and thermal simulations. Additionally there are both evaluation and demonstration boards that may be used as a starting point for design. The following list of steps can be used to manually design the LMZ22003 application.

All references to values refer to the typical applications schematic [Figure 46](#).

1. Select minimum operating  $V_{IN}$  with enable divider resistors
2. Program  $V_O$  with resistor divider selection
3. Select  $C_O$
4. Select  $C_{IN}$
5. Determine module power dissipation
6. Layout PCB for required thermal performance

#### 8.2.2.2 Enable Divider, $R_{ENT}$ , $R_{ENB}$ and $R_{ENH}$ Selection

Internal to the module is a 2-M $\Omega$  pullup resistor connected from  $V_{IN}$  to Enable. For applications not requiring precision undervoltage lockout (UVLO), the Enable input may be left open circuit and the internal resistor will always enable the module. In such case, the internal UVLO occurs typically at 4.3 V ( $V_{IN,rising}$ ).

In applications with separate supervisory circuits Enable can be directly interfaced to a logic source. In the case of sequencing supplies, the divider is connected to a rail that becomes active earlier in the power-up cycle than the LMZ22003 output rail.

Enable provides a precise 1.279 V threshold to allow direct logic drive or connection to a voltage divider from a higher enable voltage such as  $V_{IN}$ . Additionally there is 21  $\mu$ A (typical) of switched offset current allowing programmable hysteresis. See [Figure 47](#).

The function of the enable divider is to allow the designer to choose an input voltage below which the circuit will be disabled. This implements the feature of programmable UVLO. The two resistors should be chosen based on the following ratio:

$$R_{ENT} / R_{ENB} = (V_{IN,UVLO} / 1.279 V) - 1 \quad (1)$$

The LMZ22003 typical application shows 12.7 k $\Omega$  for  $R_{ENB}$  and 42.2 k $\Omega$  for  $R_{ENT}$  resulting in a rising UVLO of 5.46 V. Note that this divider presents 8.33 V to the input when the divider is raised to 20 V which would exceed the recommended 5.5-V limit for Enable. A midpoint 5.1-V Zener clamp is applied to allow the application to cover the full 6 V to 20 V range of operation. The zener clamp is not required if the target application prohibits the maximum Enable input voltage from being exceeded.

Additional enable voltage hysteresis can be added with the inclusion of  $R_{ENH}$ . It is possible to select values for  $R_{ENT}$  and  $R_{ENB}$  such that  $R_{ENH}$  is a value of zero allowing it to be omitted from the design.

Rising threshold can be calculated as follows:

$$V_{EN(rising)} = 1.279 ( 1 + (R_{ENT} || 2 \text{ meg}) / R_{ENB} ) \quad (2)$$

Whereas the falling threshold level can be calculated using:

$$V_{EN(falling)} = V_{EN(rising)} - 21 \mu A ( R_{ENT} || 2 \text{ meg} || R_{ENB} + R_{ENH} ) \quad (3)$$

Typical Application (continued)

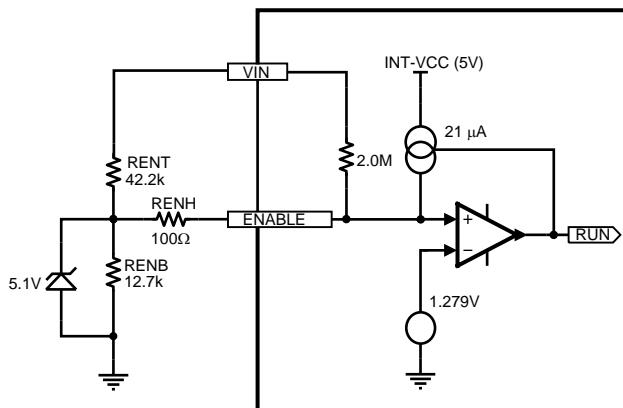


Figure 47. Enable Input Detail

8.2.2.3 Output Voltage Selection

Output voltage is determined by a divider of two resistors connected between  $V_O$  and ground. The midpoint of the divider is connected to the FB input.

The regulated output voltage determined by the external divider resistors  $R_{FBT}$  and  $R_{FBB}$  is:

$$V_O = 0.796 \text{ V} \times (1 + R_{FBT} / R_{FBB}) \tag{4}$$

Rearranging terms; the ratio of the feedback resistors for a desired output voltage is:

$$R_{FBT} / R_{FBB} = (V_O / 0.796 \text{ V}) - 1 \tag{5}$$

These resistors should generally be chosen from values in the range of 1.0 kΩ to 10.0 kΩ.

For  $V_O = 0.8 \text{ V}$  the FB pin can be connected to the output directly and  $R_{FBB}$  can be set to 8.06 kΩ to provide minimum output load.

Table 1 lists the values for  $R_{FBT}$ , and  $R_{FBB}$ .

Table 1. Typical Application Bill of Materials

REF DES	DESCRIPTION	CASE SIZE	MANUFACTURER	MANUFACTURER P/N
U1	SIMPLE SWITCHER	PFM-7	Texas Instruments	LMZ22003TZ
$C_{in1,5}$	0.047 μF, 50 V, X7R	1206	Yageo America	CC1206KRX7R9BB473
$C_{in2,3}$	10 μF, 50 V, X7R	1210	Taiyo Yuden	UMK325BJ106MM-T
$C_{in6}$ (OPT)	CAP, AL, 150 μF, 50 V	Radial G	Panasonic	EEE-FK1H151P
$C_{O1,6}$	0.047 μF, 50 V, X7R	1206	Yageo America	CC1206KRX7R9BB473
$C_{O2}$ (OPT)	100 μF, 6.3 V, X7R	1210	TDK	C3225X5R0J107M
$C_{O5}$	220 μF, 6.3 V, SP-Cap	(7343)	Panasonic	EEF-UE0J221LR
$R_{FBT}$	3.32 kΩ	0805	Panasonic	ERJ-6ENF3321V
$R_{FBB}$	1.07 kΩ	0805	Panasonic	ERJ-6ENF1071V
$R_{SN}$ (OPT)	1.50 kΩ	0805	Vishay Dale	CRCW08051K50FKEA
$R_{ENT}$	42.2 kΩ	0805	Panasonic	ERJ-6ENF4222V
$R_{ENB}$	12.7 kΩ	0805	Panasonic	ERJ-6ENF1272V
$R_{FRA}$ (OPT)	23.7Ω	0805	Vishay Dale	CRCW080523R7FKEA
$R_{ENH}$	100 Ω	0805	Vishay Dale	CRCW0805100RFKEA
$C_{SS}$	0.47 μF, ±10%, X7R, 16 V	0805	AVX	0805YC474KAT2A
D1(OPT)	5.1 V, 0.5 W	SOD-123	Diodes Inc.	MMSZ5231BS-7-F

### 8.2.2.4 Soft-Start Capacitor Selection

Programmable soft-start permits the regulator to slowly ramp to its steady-state operating point after being enabled, thereby reducing current inrush from the input supply and slowing the output voltage rise-time.

Upon turnon, after all UVLO conditions have been passed, an internal 1.6-ms circuit slowly ramps the SS/TRK input to implement internal soft start. If 2 ms is an adequate turnon time then the  $C_{SS}$  capacitor can be left unpopulated. Longer soft-start periods are achieved by adding an external capacitor to this input.

Soft-start duration is given by the formula:

$$t_{SS} = V_{REF} \times C_{SS} / I_{SS} = 0.796 \text{ V} \times C_{SS} / 50 \mu\text{A} \quad (6)$$

This equation can be rearranged as follows:

$$C_{SS} = t_{SS} \times 50 \mu\text{A} / 0.796 \text{ V} \quad (7)$$

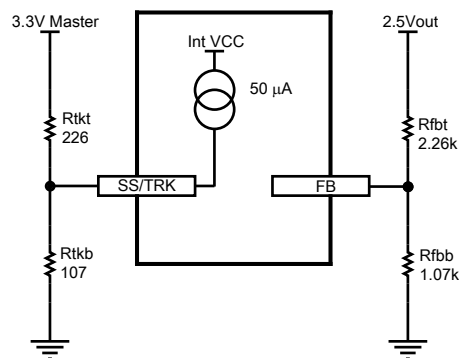
Using a 0.22- $\mu\text{F}$  capacitor results in 3.5-ms typical soft-start duration; and 0.47  $\mu\text{F}$  results in 7.5-ms typical. 0.47  $\mu\text{F}$  is a recommended initial value.

As the soft-start input exceeds 0.796 V, the output of the power stage will be in regulation and the 50- $\mu\text{A}$  current is deactivated. Note that the following conditions will reset the soft-start capacitor by discharging the SS input to ground with an internal current sink.

- The Enable input being *pulled low*
- Thermal shutdown condition
- Internal  $V_{CC}$  UVLO (Approx 4.3-V input to  $V_{IN}$ )

### 8.2.2.5 Tracking Supply Divider Option

The tracking function allows the module to be connected as a slave supply to a primary voltage rail (often the 3.3-V system rail) where the slave module output voltage is lower than that of the master. Proper configuration allows the slave rail to power up coincident with the master rail such that the voltage difference between the rails during ramp-up is small (that is, < 0.15 V typical). The values for the tracking resistive divider should be selected such that the effect of the internal 50- $\mu\text{A}$  current source is minimized. In most cases the ratio of the tracking divider resistors is the same as the ratio of the output voltage setting divider. Proper operation in tracking mode dictates the soft-start time of the slave rail be shorter than the master rail; a condition that is easy satisfy since the  $C_{SS}$  cap is replaced by  $R_{TKB}$ . The tracking function is only supported for the power-up interval of the master supply; once the SS/TRK rises past 0.8 V the input is no longer enabled and the 50- $\mu\text{A}$  internal current source is switched off.



**Figure 48. Tracking Option Input Detail**

### 8.2.2.6 $C_O$ Selection

None of the required  $C_O$  output capacitance is contained within the module. A minimum value of 200  $\mu\text{F}$  is required based on the values of internal compensation in the error amplifier. Low ESR tantalum, organic semiconductor or specialty polymer capacitor types are recommended for obtaining lowest ripple. The output capacitor  $C_O$  may consist of several capacitors in parallel placed in close proximity to the module. The output capacitor assembly must also meet the worst case minimum ripple current rating of  $0.5 \times I_{LR P-P}$ , as calculated in Equation 13. Beyond that, additional capacitance will reduce output ripple so long as the ESR is low enough to permit it. Loop response verification is also valuable to confirm closed loop behavior.

For applications with dynamic load steps; the following equation provides a good first pass approximation of  $C_O$  for load transient requirements. Where  $V_{O-Trans}$  is 100 mV on a 3.3-V output design.

$$C_O \geq I_{O-Trans} / [ ( V_{O-Trans} - ESR \times I_{O-Trans} ) \times ( F \times f_{SW} / V_O ) ] \quad (8)$$

Solving:

$$C_O \geq 2.5 \text{ A} / ( 0.1 \text{ V} - 0.007 \times 2.5 \text{ A} ) \times ( 800000 \text{ Hz} / 3.3 \text{ V} ) \geq 125 \text{ } \mu\text{F} \quad (9)$$

The stability requirement for 200- $\mu\text{F}$  minimum output capacitance will take precedence.

One recommended output capacitor combination is a 220- $\mu\text{F}$ , 7-m $\Omega$  ESR specialty polymer cap in parallel with a 100- $\mu\text{F}$  6.3-V X5R ceramic. This combination provides excellent performance that may exceed the requirements of certain applications. Additionally some small ceramic capacitors can be used for high-frequency EMI suppression.

### 8.2.2.7 $C_{IN}$ Selection

The LMZ22003 module contains a small amount of internal ceramic input capacitance. Additional input capacitance is required external to the module to handle the input ripple current of the application. The input capacitor can be several capacitors in parallel. This input capacitance should be located in very close proximity to the module. Input capacitor selection is generally directed to satisfy the input ripple current requirements rather than by capacitance value. Input ripple current rating is dictated by the equation:

$$I(C_{IN(RMS)}) \approx 1 / 2 \times I_O \times \text{SQRT} ( D / 1 - D )$$

where

- $D \approx V_O / V_{IN}$  (10)

As a point of reference, the worst case ripple current will occur when the module is presented with full load current and when  $V_{IN} = 2 \times V_O$ .

Recommended minimum input capacitance is 22- $\mu\text{F}$  X7R (or X5R) ceramic with a voltage rating at least 25% higher than the maximum applied input voltage for the application. TI recommends to pay attention to the voltage and temperature derating of the capacitor selected.

#### NOTE

The ripple current rating of ceramic capacitors may be missing from the capacitor data sheet and you may have to contact the capacitor manufacturer for this parameter.

If the system design requires a certain minimum value of peak-to-peak input ripple voltage ( $\Delta V_{IN}$ ) be maintained then the following equation may be used.

$$C_{IN} \geq I_O \times D \times ( 1 - D ) / f_{SW-CCM} \times \Delta V_{IN} \quad (11)$$

If  $\Delta V_{IN}$  is 1% of  $V_{IN}$  for a 12-V input to 3.3-V output application this equals 120 mV and  $f_{SW} = 812 \text{ kHz}$ .

$$C_{IN} \geq 3 \text{ A} \times 3.3 \text{ V} / 12 \text{ V} \times ( 1 - 3.3 \text{ V} / 12 \text{ V} ) / ( 812000 \times 0.120 \text{ V} ) \geq 6.14 \text{ } \mu\text{F}$$

Additional bulk capacitance with higher ESR may be required to damp any resonant effects of the input capacitance and parasitic inductance of the incoming supply lines. The LMZ22003 typical applications schematic and evaluation board include a 150- $\mu\text{F}$ , 50-V aluminum capacitor for this function. There are many situations where this capacitor is not necessary.

### 8.2.2.8 Discontinuous Conduction and Continuous Conduction Modes Selection

The approximate formula for determining the DCM/CCM boundary is as follows:

$$I_{DCB} \approx V_O \times ( V_{IN} - V_O ) / ( 2 \times 3.3 \text{ } \mu\text{H} \times f_{SW(CCM)} \times V_{IN} ) \quad (12)$$

The inductor internal to the module is 3.3  $\mu\text{H}$ . This value was chosen as a good balance between low and high input voltage applications. The main parameter affected by the inductor is the amplitude of the inductor ripple current ( $I_{LR}$ ).  $I_{LR}$  can be calculated with:

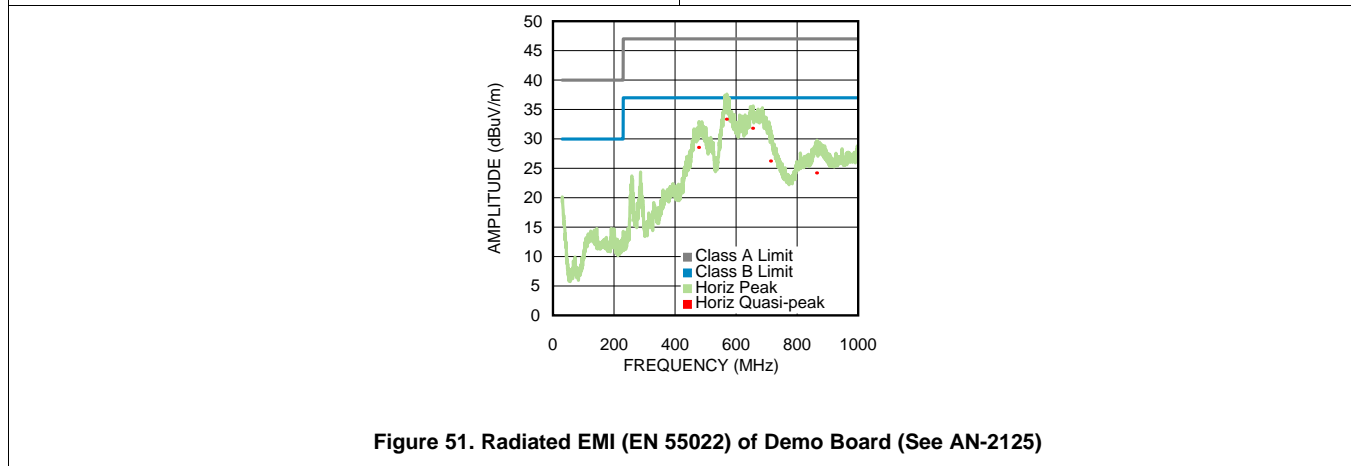
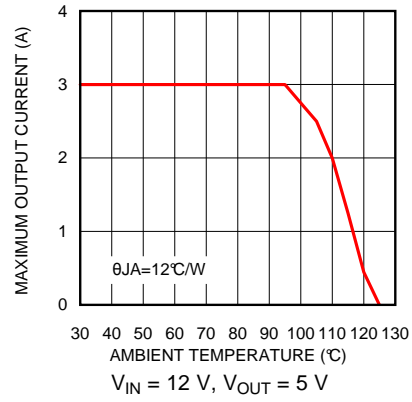
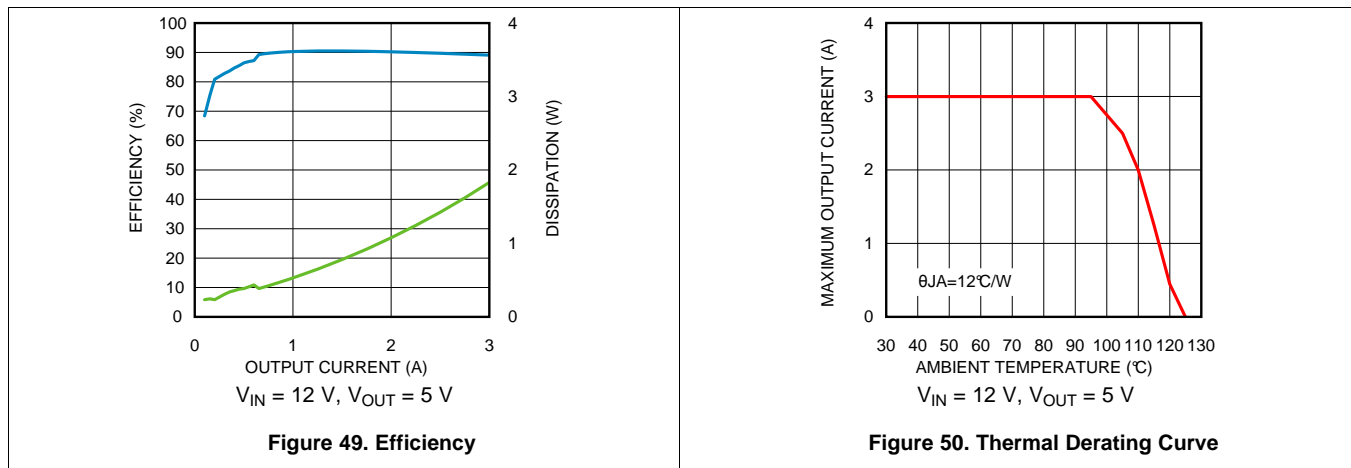
$$I_{LR P-P} = V_O \times ( V_{IN} - V_O ) / ( 3.3 \text{ } \mu\text{H} \times f_{SW} \times V_{IN} )$$

where

- $V_{IN}$  is the maximum input voltage
- and  $f_{SW}$  is typically 812 kHz. (13)

If the output current  $I_O$  is determined by assuming that  $I_O = I_L$ , the higher and lower peak of  $I_{LR}$  can be determined.

### 8.2.3 Application Curves



## 9 Power Supply Recommendations

The LMZ22003 device is designed to operate from an input voltage supply range between 6 V and 20 V. This input supply should be well regulated and able to withstand maximum input current and maintain a stable voltage. The resistance of the input supply rail should be low enough that an input current transient does not cause a high enough drop at the LMZ22003 supply voltage that can cause a false UVLO fault triggering and system reset. If the input supply is more than a few inches from the LMZ22003, additional bulk capacitance may be required in addition to the ceramic bypass capacitors. The amount of bulk capacitance is not critical, but a 47- $\mu$ F or 100- $\mu$ F electrolytic capacitor is a typical choice.

## 10 Layout

### 10.1 Layout Guidelines

PCB layout is an important part of DC-DC converter design. Poor board layout can disrupt the performance of a DC-DC converter and surrounding circuitry by contributing to EMI, ground bounce and resistive voltage drop in the traces. These can send erroneous signals to the DC-DC converter resulting in poor regulation or instability. Good layout can be implemented by following a few simple design rules. A good example layout is shown in [Figure 54](#).

### 10.2 Layout Examples

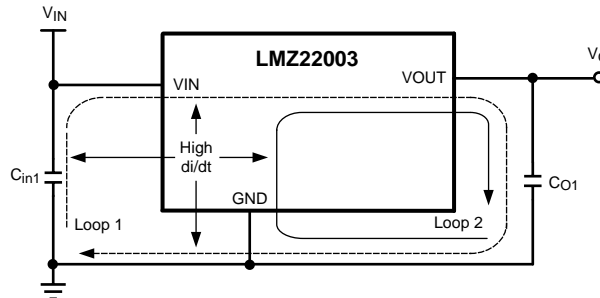


Figure 52. Critical Current Loops to Minimize

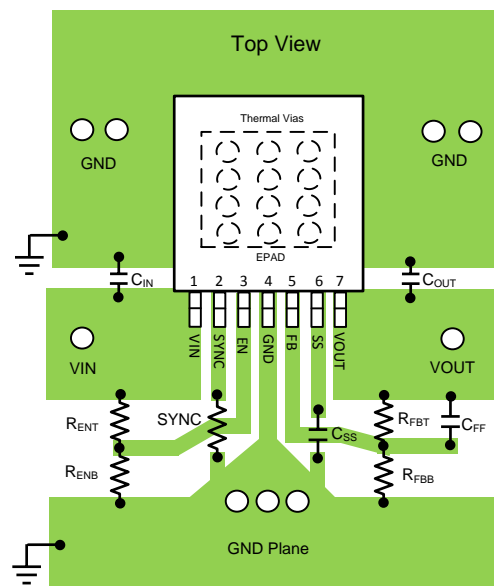
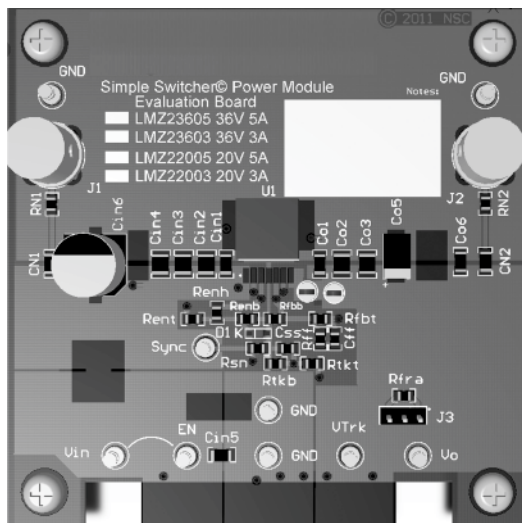
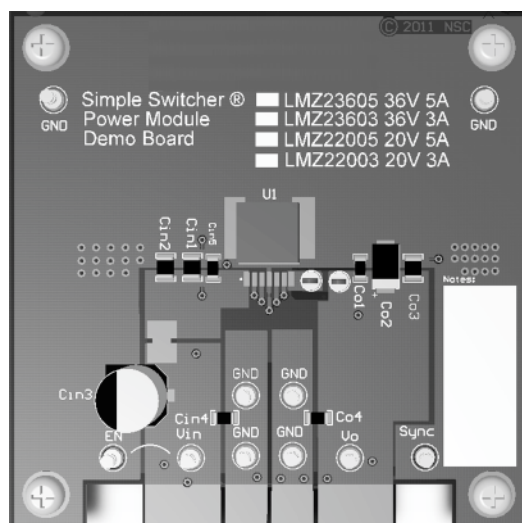


Figure 53. PCB Layout Guide

**Layout Examples (continued)**

**Figure 54. Top View Evaluation Board – See AN-2085**

**Figure 55. Bottom View Demonstration Board**
**10.3 Power Dissipation and Thermal Considerations**

When calculating module dissipation use the maximum input voltage and the average output current for the application. Many common operating conditions are provided in the characteristic curves such that less common applications can be derived through interpolation. In all designs, the junction temperature must be kept below the rated maximum of 125°C.

For the design case of  $V_{IN} = 12\text{ V}$ ,  $V_O = 3.3\text{ V}$ ,  $I_O = 3\text{ A}$ , and  $T_{AMB(MAX)} = 85^\circ\text{C}$ , the module must see a thermal resistance from case to ambient of less than:

$$R_{\theta CA} < (T_{J-MAX} - T_{A-MAX}) / P_{IC-LOSS} - R_{\theta JC} \quad (14)$$

Given the typical thermal resistance from junction to case to be 1.9°C/W. Use the 85°C power dissipation curves in the [Typical Characteristics](#) section to estimate the  $P_{IC-LOSS}$  for the application being designed. In this application it is 2W.

$$R_{\theta CA} = (125 - 85) / 2\text{ W} - 1.9 = 18.1 \quad (15)$$



### Power Dissipation and Thermal Considerations (continued)

To reach  $R_{\theta CA} = 18.1$ , the PCB is required to dissipate heat effectively. With no airflow and no external heat-sink, a good estimate of the required board area covered by 2-oz. copper on both the top and bottom metal layers is:

$$\text{Board\_Area\_cm}^2 = 500^{\circ}\text{C} \times \text{cm}^2/\text{W} / R_{\theta CA} \tag{16}$$

As a result, approximately 28 square cm of 2-oz. copper on top and bottom layers is required for the PCB design. The PCB copper heat sink must be connected to the exposed pad. Approximately sixty, 8 mil thermal vias spaced 39 mils (1.0 mm) apart connect the top copper to the bottom copper. For an example of a high thermal performance PCB layout for SIMPLE SWITCHER power modules, refer to AN-2085 (SNVA457), AN-2125 (SNVA437), AN-2020 (SNVA419) and AN-2026 (SNVA424).

### 10.4 Power Module SMT Guidelines

The recommendations below are for a standard module surface mount assembly

- Land Pattern — Follow the PCB land pattern with either soldermask defined or non-soldermask defined pads
- Stencil Aperture
  - For the exposed die attach pad (DAP), adjust the stencil for approximately 80% coverage of the PCB land pattern
  - For all other I/O pads use a 1:1 ratio between the aperture and the land pattern recommendation
- Solder Paste — Use a standard SAC Alloy such as SAC 305, type 3 or higher
- Stencil Thickness — 0.125 to 0.15mm
- Reflow - Refer to solder paste supplier recommendation and optimized per board size and density
- Refer to *Design Summary LMZ1xxx and LMZ2xxx Power Modules Family* (SNAA214) for reflow information
- Maximum number of reflows allowed is one

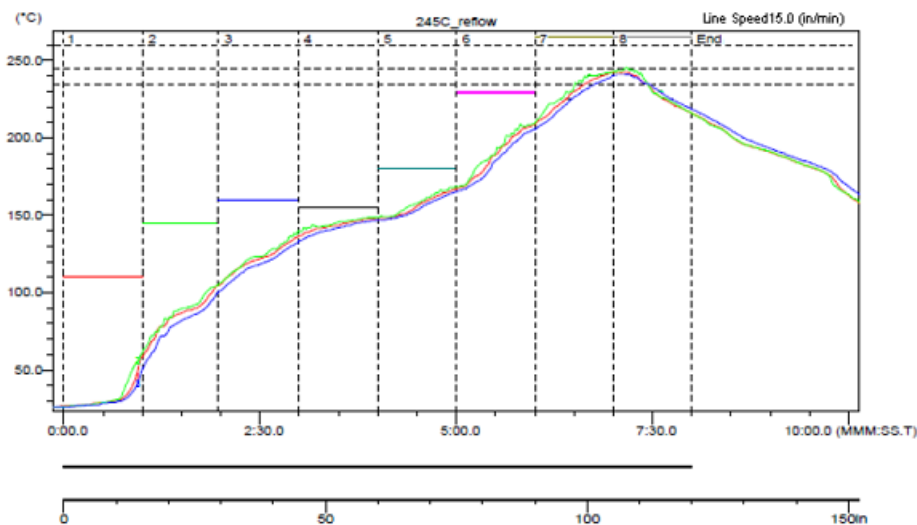


Figure 56. Sample Reflow Profile

Table 2. Sample Reflow Profile Table

PROBE	MAX TEMP (°C)	REACHED MAX TEMP	TIME ABOVE 235°C	REACHED 235°C	TIME ABOVE 245°C	REACHED 245°C	TIME ABOVE 260°C	REACHED 260°C
1	242.5	6.58	0.49	6.39	0.00	–	0.00	–
2	242.5	7.10	0.55	6.31	0.00	7.10	0.00	–
3	241.0	7.09	0.42	6.44	0.00	–	0.00	–

## 11 Device and Documentation Support

### 11.1 Device Support

#### 11.1.1 Third-Party Products Disclaimer

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#### 11.1.2 Development Support

For developmental support, see the following:

WEBENCH Tool, <http://www.ti.com/webench>

### 11.2 Documentation Support

#### 11.2.1 Related Documentation

For related documentation, see the following:

- AN-2027 *Inverting Application for the LMZ14203 SIMPLE SWITCHER Power Module*, ([SNVA425](#))
- *Absolute Maximum Ratings for Soldering*, ([SNOA549](#))
- AN-2024 *LMZ1420x / LMZ1200x Evaluation Board* ([SNVA422](#))
- AN-2085 *LMZ23605/03, LMZ22005/03 Evaluation Board* ([SNVA457](#))
- AN-2054 *Evaluation Board for LM10000 - PowerWise AVS System Controller* ([SNVA437](#))
- AN-2020 *Thermal Design By Insight, Not Hindsight* ([SNVA419](#))
- AN-2026 *Effect of PCB Design on Thermal Performance of SIMPLE SWITCHER Power Modules* ([SNVA424](#))
- *Design Summary LMZ1xxx and LMZ2xxx Power Modules Family* ([SNAA214](#))

### 11.3 Community Resources

The following links connect to TI community resources. Linked contents are provided "AS IS" by the respective contributors. They do not constitute TI specifications and do not necessarily reflect TI's views; see TI's [Terms of Use](#).

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**Design Support** *TI's Design Support* Quickly find helpful E2E forums along with design support tools and contact information for technical support.

### 11.4 Trademarks

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### 11.5 Electrostatic Discharge Caution



These devices have limited built-in ESD protection. The leads should be shorted together or the device placed in conductive foam during storage or handling to prevent electrostatic damage to the MOS gates.

### 11.6 Glossary

[SLYZ022](#) — *TI Glossary*.

This glossary lists and explains terms, acronyms, and definitions.

## 12 Mechanical, Packaging, and Orderable Information

The following pages include mechanical, packaging, and orderable information. This information is the most current data available for the designated devices. This data is subject to change without notice and revision of this document. For browser-based versions of this data sheet, refer to the left-hand navigation.

**PACKAGING INFORMATION**

Orderable Device	Status (1)	Package Type	Package Drawing	Pins	Package Qty	Eco Plan (2)	Lead/Ball Finish (6)	MSL Peak Temp (3)	Op Temp (°C)	Device Marking (4/5)	Samples
LMZ22003TZ/NOPB	ACTIVE	TO-PMOD	NDW	7	45	Green (RoHS & no Sb/Br)	CU SN	Level-3-245C-168 HR	-40 to 85	LMZ22003	<a href="#">Samples</a>
LMZ22003TZE/NOPB	ACTIVE	TO-PMOD	NDW	7	250	Green (RoHS & no Sb/Br)	CU SN	Level-3-245C-168 HR	-40 to 85	LMZ22003	<a href="#">Samples</a>
LMZ22003TZX/NOPB	ACTIVE	TO-PMOD	NDW	7	500	Green (RoHS & no Sb/Br)	CU SN	Level-3-245C-168 HR	-40 to 85	LMZ22003	<a href="#">Samples</a>

(1) The marketing status values are defined as follows:

**ACTIVE:** Product device recommended for new designs.

**LIFEBUY:** TI has announced that the device will be discontinued, and a lifetime-buy period is in effect.

**NRND:** Not recommended for new designs. Device is in production to support existing customers, but TI does not recommend using this part in a new design.

**PREVIEW:** Device has been announced but is not in production. Samples may or may not be available.

**OBsolete:** TI has discontinued the production of the device.

(2) Eco Plan - The planned eco-friendly classification: Pb-Free (RoHS), Pb-Free (RoHS Exempt), or Green (RoHS & no Sb/Br) - please check <http://www.ti.com/productcontent> for the latest availability information and additional product content details.

**TBD:** The Pb-Free/Green conversion plan has not been defined.

**Pb-Free (RoHS):** TI's terms "Lead-Free" or "Pb-Free" mean semiconductor products that are compatible with the current RoHS requirements for all 6 substances, including the requirement that lead not exceed 0.1% by weight in homogeneous materials. Where designed to be soldered at high temperatures, TI Pb-Free products are suitable for use in specified lead-free processes.

**Pb-Free (RoHS Exempt):** This component has a RoHS exemption for either 1) lead-based flip-chip solder bumps used between the die and package, or 2) lead-based die adhesive used between the die and leadframe. The component is otherwise considered Pb-Free (RoHS compatible) as defined above.

**Green (RoHS & no Sb/Br):** TI defines "Green" to mean Pb-Free (RoHS compatible), and free of Bromine (Br) and Antimony (Sb) based flame retardants (Br or Sb do not exceed 0.1% by weight in homogeneous material)

(3) MSL, Peak Temp. - The Moisture Sensitivity Level rating according to the JEDEC industry standard classifications, and peak solder temperature.

(4) There may be additional marking, which relates to the logo, the lot trace code information, or the environmental category on the device.

(5) Multiple Device Markings will be inside parentheses. Only one Device Marking contained in parentheses and separated by a "~" will appear on a device. If a line is indented then it is a continuation of the previous line and the two combined represent the entire Device Marking for that device.

(6) Lead/Ball Finish - Orderable Devices may have multiple material finish options. Finish options are separated by a vertical ruled line. Lead/Ball Finish values may wrap to two lines if the finish value exceeds the maximum column width.

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**TAPE AND REEL INFORMATION**

**QUADRANT ASSIGNMENTS FOR PIN 1 ORIENTATION IN TAPE**


\*All dimensions are nominal

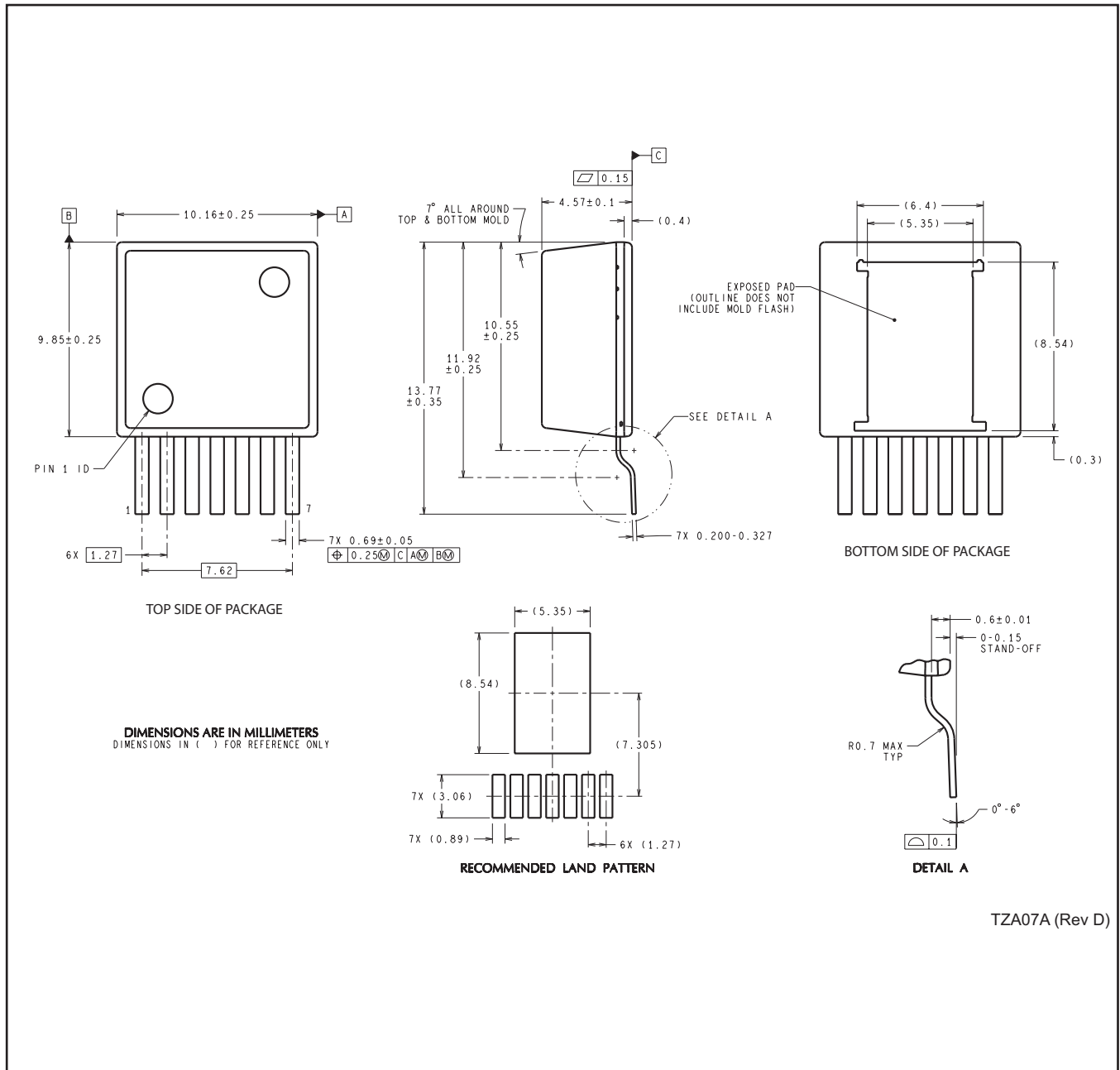
Device	Package Type	Package Drawing	Pins	SPQ	Reel Diameter (mm)	Reel Width W1 (mm)	A0 (mm)	B0 (mm)	K0 (mm)	P1 (mm)	W (mm)	Pin1 Quadrant
LMZ22003TZE/NOPB	TO-PMOD	NDW	7	250	330.0	24.4	10.6	14.22	5.0	16.0	24.0	Q2
LMZ22003TZX/NOPB	TO-PMOD	NDW	7	500	330.0	24.4	10.6	14.22	5.0	16.0	24.0	Q2

**TAPE AND REEL BOX DIMENSIONS**


\*All dimensions are nominal

Device	Package Type	Package Drawing	Pins	SPQ	Length (mm)	Width (mm)	Height (mm)
LMZ22003TZE/NOPB	TO-PMOD	NDW	7	250	367.0	367.0	45.0
LMZ22003TZX/NOPB	TO-PMOD	NDW	7	500	367.0	367.0	45.0

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