

# LMK00306

## 3-GHz 6-Output Differential Clock Buffer/Level Translator

### 1.0 General Description

The LMK00306 is a 3-GHz, 6-output differential fanout buffer intended for high-frequency, low-jitter clock/data distribution and level translation. The input clock can be selected from two universal inputs or one crystal input. The selected input clock is distributed to two banks of 3 differential outputs and one LVCMOS output. Both differential output banks can be independently configured as LVPECL, LVDS, or HCSL drivers, or disabled. The LVCMOS output has a synchronous enable input for runt-pulse-free operation when enabled or disabled. The LMK00306 operates from a 3.3 V core supply and 3 independent 3.3 V/2.5 V output supplies.

The LMK00306 provides high performance, versatility, and power efficiency, making it ideal for replacing fixed-output buffer devices while increasing timing margin in the system.

### 2.0 Target Applications

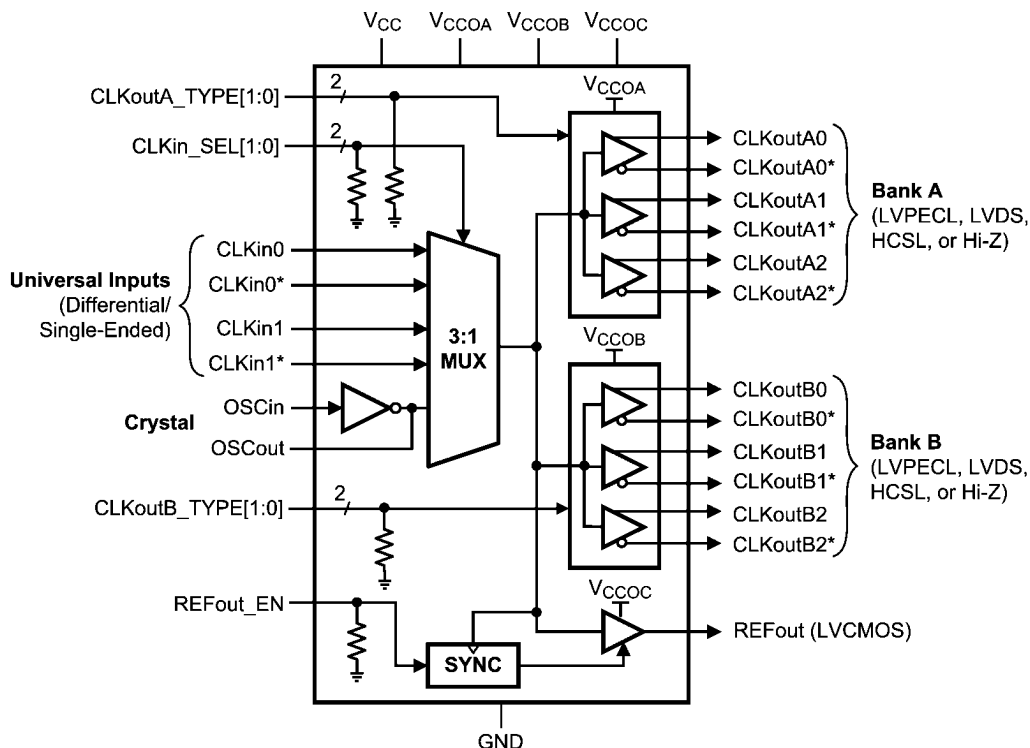
- Clock Distribution and Level Translation for high-speed ADCs, DACs, Serial Interfaces (Multi-Gigabit Ethernet, XAUI, Fibre Channel, PCIe, SATA/SAS, SONET/SDH, CPRI), and high-frequency backplanes
- Remote Radio Units (RRU) and Baseband Units (BBU)
- Switches and Routers

- Servers, Workstations, and Computing

### 3.0 Features

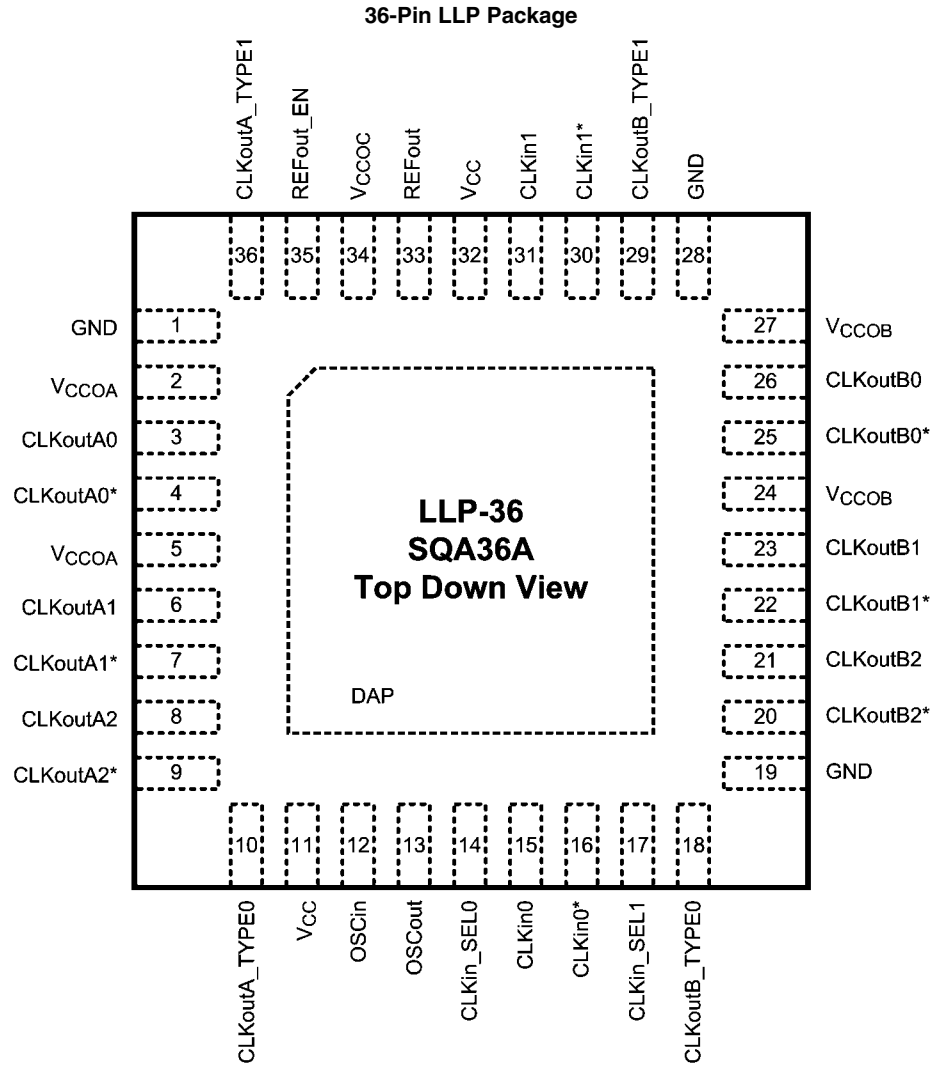
- 3:1 Input Multiplexer
  - Two universal inputs operate up to 3.1 GHz and accept LVPECL, LVDS, CML, SSTL, HSTL, HCSL (AC-coupled), or single-ended clocks
  - One crystal input accepts a 10 to 40 MHz crystal or single-ended clock
- Two Banks with 3 Differential Outputs each
  - LVPECL, LVDS, HCSL, or Hi-Z (selectable per bank)
  - LVPECL Additive Jitter with LMK03806 clock source:
    - 20 fs RMS at 156.25 MHz (10 kHz – 1 MHz)
    - 51 fs RMS at 156.25 MHz (12 kHz – 20 MHz)
- High PSRR: -65 / -76 dBc (LVPECL/LVDS) at 156.25 MHz
- LVCMOS output with synchronous enable input
- Pin-controlled configuration
- V<sub>CC</sub> Core Supply: 3.3 V ± 5%
- 3 Independent V<sub>CCO</sub> Output Supplies: 3.3 V/2.5 V ± 5%
- Industrial temperature range: -40°C to +85°C
- Package: 36-pin LLP (6.0 x 6.0 x 0.8 mm)

### 4.0 Functional Block Diagram



30177401

## 5.0 Connection Diagram



30177402

## 6.0 Pin Descriptions

Pin #	Pin Name(s)	Type	Description
DAP	DAP	GND	Die Attach Pad. Connect to the PCB ground plane for heat dissipation.
1, 19, 28	GND	GND	Ground
2, 5	V <sub>CCOA</sub>	PWR	Power supply for Bank A Output buffers. V <sub>CCOA</sub> can operate from 3.3 V or 2.5 V. The V <sub>CCOA</sub> pins are internally tied together. Bypass with a 0.1 uF low-ESR capacitor placed very close to each Vcco pin. ( <a href="#">Note 1</a> )
3, 4	CLKoutA0, CLKoutA0*	O	Differential clock output A0. Output type set by CLKoutA_TYPE pins.
6, 7	CLKoutA1, CLKoutA1*	O	Differential clock output A1. Output type set by CLKoutA_TYPE pins.
8, 9	CLKoutA2, CLKoutA2*	O	Differential clock output A2. Output type set by CLKoutA_TYPE pins.
10, 36	CLKoutA_TYPE0, CLKoutA_TYPE1	I	Bank A output buffer type selection pins ( <a href="#">Note 2</a> )
11, 32	Vcc	PWR	Power supply for Core and Input buffer blocks. The Vcc supply operates from 3.3 V. Bypass with a 0.1 uF low-ESR capacitor placed very close to each Vcc pin.
12	OSCIin	I	Input for crystal. Can also be driven by a XO, TCXO, or other external single-ended clock.
13	OSCOout	O	Output for crystal. Leave OSCout floating if OSCin is driven by a single-ended clock.
14, 17	CLKin_SEL0, CLKin_SEL1	I	Clock input selection pins ( <a href="#">Note 2</a> )
15, 16	CLKin0, CLKin0*	I	Universal clock input 0 (differential/single-ended)
18, 29	CLKoutB_TYPE0, CLKoutB_TYPE1	I	Bank B output buffer type selection pins ( <a href="#">Note 2</a> )
20, 21	CLKoutB2*, CLKoutB2	O	Differential clock output B2. Output type set by CLKoutB_TYPE pins.
22, 23	CLKoutB1*, CLKoutB1	O	Differential clock output B1. Output type set by CLKoutB_TYPE pins.
24, 27	V <sub>CCOB</sub>	PWR	Power supply for Bank B Output buffers. V <sub>CCOB</sub> can operate from 3.3 V or 2.5 V. The V <sub>CCOB</sub> pins are internally tied together. Bypass with a 0.1 uF low-ESR capacitor placed very close to each Vcco pin. ( <a href="#">Note 1</a> )
25, 26	CLKoutB0*, CLKoutB0	O	Differential clock output B0. Output type set by CLKoutB_TYPE pins.
30, 31	CLKin1*, CLKin1	I	Universal clock input 1 (differential/single-ended)
33	REFout	O	LVC MOS reference output. Enable output by pulling REFout_EN pin high.
34	V <sub>CCOC</sub>	PWR	Power supply for REFout Output buffer. V <sub>CCOC</sub> can operate from 3.3 V or 2.5 V. Bypass with a 0.1 uF low-ESR capacitor placed very close to each Vcco pin. ( <a href="#">Note 1</a> )
35	REFout_EN	I	REFout enable input. Enable signal is internally synchronized to selected clock input. ( <a href="#">Note 2</a> )

**Note 1:** The output supply voltages or pins (V<sub>CCOA</sub>, V<sub>CCOB</sub>, and V<sub>CCOC</sub>) will be called V<sub>CCO</sub> in general when no distinction is needed, or when the output supply can be inferred from the output bank/type.

**Note 2:** CMOS control input with internal pull-down resistor.

**Note 3:** Any unused output pins should be left floating with minimum copper length ([Note 5](#)), or properly terminated if connected to a transmission line, or disabled/Hi-Z if possible. See [Section 7.3 Clock Outputs](#) for output configuration or [Section 14.3 Termination and Use of Clock Drivers](#) for output interface and termination techniques.

## 7.0 Functional Description

The LMK00306 is a 6-output differential clock fanout buffer with low additive jitter that can operate up to 3.1 GHz. It features a 3:1 input multiplexer with an optional crystal oscillator input, two banks of 3 differential outputs with multi-mode buffers (LVPECL, LVDS, HCSL, or Hi-Z), one LVCMOS output, and 3 independent output buffer supplies. The input selection and output buffer modes are controlled via pin strapping. The device is offered in a 36-pin LLP package and leverages much of the high-speed, low-noise circuit design employed in the LMK04800 family of clock conditioners.

### 7.1 $V_{CC}$ and $V_{CCO}$ Power Supplies

The LMK00306 has separate 3.3 V core supply ( $V_{CC}$ ) and 3 independent 3.3 V/2.5 V output power supplies ( $V_{CCOA}$ ,  $V_{CCOB}$ ,  $V_{CCOC}$ ). Output supply operation at 2.5 V enables lower power consumption and output-level compatibility with 2.5 V receiver devices. The output levels for LVPECL ( $V_{OH}$ ,  $V_{OL}$ ) and LVCMOS ( $V_{OH}$ ) are referenced to the respective  $V_{CCO}$  supply, while the output levels for LVDS and HCSL are relatively constant over the specified  $V_{CCO}$  range. Refer to [Section 14.4 Power Supply and Thermal Considerations](#) for additional supply related considerations, such as power dissipation, power supply bypassing, and power supply ripple rejection (PSRR).

**Note 4:** Care should be taken to ensure the  $V_{CCO}$  voltages do not exceed the  $V_{CC}$  voltage to prevent turning-on the internal ESD protection circuitry.

### 7.2 Clock Inputs

The input clock can be selected from  $CLKin0/CLKin0^*$ ,  $CLKin1/CLKin1^*$ , or  $OSCin$ . Clock input selection is controlled using the  $CLKin\_SEL[1:0]$  inputs as shown in [Table 1](#). Refer to [Section 14.1 Driving the Clock Inputs](#) for clock input requirements. When  $CLKin0$  or  $CLKin1$  is selected, the crystal circuit is powered down. When  $OSCin$  is selected, the crystal oscillator circuit will start-up and its clock will be distributed to all outputs. Refer to [Section 14.2 Crystal Interface](#) for more information. Alternatively,  $OSCin$  may be driven by a single-ended clock (up to 250 MHz) instead of a crystal.

**TABLE 1. Input Selection**

$CLKin\_SEL1$	$CLKin\_SEL0$	Selected Input
0	0	$CLKin0$ , $CLKin0^*$
0	1	$CLKin1$ , $CLKin1^*$
1	X	$OSCin$

[Table 2](#) shows the output logic state vs. input state when either  $CLKin0/CLKin0^*$  or  $CLKin1/CLKin1^*$  is selected. When  $OSCin$  is selected, the output state will be an inverted copy of the  $OSCin$  input state.

**TABLE 2.  $CLKin$  Input vs. Output States**

State of Selected $CLKin$	State of Enabled Outputs
$CLKinX$ and $CLKinX^*$ inputs floating	Logic low
$CLKinX$ and $CLKinX^*$ inputs shorted together	Logic low
$CLKin$ logic low	Logic low
$CLKin$ logic high	Logic high

### 7.3 Clock Outputs

The differential output buffer type for Bank A and Bank B outputs can be separately configured using the  $CLKoutA\_TYPE[1:0]$  and  $CLKoutB\_TYPE[1:0]$  inputs, respectively, as shown in [Table 3](#). For applications where all differential outputs are not needed, any unused output pin should be left floating with a minimum copper length ([Note 5](#)) to minimize capacitance and potential coupling and reduce power consumption. If an entire output bank will not be used, it is recommended to disable/Hi-Z the bank to reduce power. Refer to [Section 14.3 Termination and Use of Clock Drivers](#) for more information on output interface and termination techniques.

**Note 5:** For best soldering practices, the minimum trace length for any unused output pin should extend to include the pin solder mask. This way during reflow, the solder has the same copper area as connected pins. This allows for good, uniform fillet solder joints helping to keep the IC level during reflow.

**TABLE 3. Differential Output Buffer Type Selection**

$CLKoutX\_TYPE1$	$CLKoutX\_TYPE0$	$CLKoutX$ Buffer Type (Bank A or B)
0	0	LVPECL
0	1	LVDS
1	0	HCSL
1	1	Disabled (Hi-Z)

#### 7.3.1 Reference Output

The reference output ( $REFout$ ) provides a LVCMOS copy of the selected input clock. The LVCMOS output high level is referenced to the  $V_{CCO}$  voltage.  $REFout$  can be enabled or disabled using the enable input pin,  $REFout\_EN$ , as shown in [Table 4](#).

**TABLE 4. Reference Output Enable**

$REFout\_EN$	$REFout$ State
0	Disabled (Hi-Z)
1	Enabled

The  $REFout\_EN$  input is internally synchronized with the selected input clock by the SYNC block. This synchronizing function prevents glitches and runt pulses from occurring on the  $REFout$  clock when enabled or disabled.  $REFout$  will be enabled within 3 cycles ( $t_{EN}$ ) of the input clock after  $REFout\_EN$  is toggled high.  $REFout$  will be disabled within 3 cycles ( $t_{DIS}$ ) of the input clock after  $REFout\_EN$  is toggled low. When  $REFout$  is disabled, the use of a resistive loading can be used to set the output to a predetermined level. For example, if  $REFout$  is configured with a 1 k $\Omega$  load to ground, then the output will be pulled to low when disabled.

## 8.0 Absolute Maximum Ratings (Note 6, Note 7)

If Military/Aerospace specified devices are required, please contact the Texas Instruments Sales Office/ Distributors for availability and specifications.

Parameter	Symbol	Ratings	Units
Supply Voltages	$V_{CC}, V_{CCO}$	-0.3 to 3.6	V
Input Voltage	$V_{IN}$	-0.3 to ( $V_{CC} + 0.3$ )	V
Storage Temperature Range	$T_{STG}$	-65 to +150	°C
Lead Temperature (solder 4 s)	$T_L$	+260	°C
Junction Temperature	$T_J$	+150	°C

## 9.0 Recommended Operating Conditions

Parameter	Symbol	Min	Typ	Max	Units
Ambient Temperature Range	$T_A$	-40	25	85	°C
Junction Temperature	$T_J$			125	°C
Core Supply Voltage Range	$V_{CC}$	3.15	3.3	3.45	V
Output Supply Voltage Range <small>(Note 8, Note 9)</small>	$V_{CCO}$	3.3 – 5% 2.5 – 5%	3.3 2.5	3.3 + 5% 2.5 + 5%	V

**Note 6:** Absolute Maximum Ratings indicate limits beyond which damage to the device may occur. Operating Ratings indicate conditions for which the device is intended to be functional, but do not guarantee specific performance limits. For guaranteed specifications and test conditions, see [Section 11.0 Electrical Characteristics](#). The guaranteed specifications apply only to the test conditions listed.

**Note 7:** This device is a high-performance integrated circuit with an ESD rating up to 2 kV Human Body Model, up to 150 V Machine Model, and up to 750 V Charged Device Model and is ESD sensitive. Handling and assembly of this device should only be done at ESD-free workstations.

**Note 8:** The output supply voltages or pins ( $V_{CCOA}$ ,  $V_{CCOB}$ , and  $V_{CCOC}$ ) will be called  $V_{CCO}$  in general when no distinction is needed, or when the output supply can be inferred from the output bank/type.

**Note 9:**  $V_{CCO}$  should be less than or equal to  $V_{CC}$  ( $V_{CCO} \leq V_{CC}$ ).

## 10.0 Package Thermal Resistance

Package	$\theta_{JA}$	$\theta_{JC}$ (DAP)
36-Lead LLP <small>(Note 10)</small>	31.8 °C/W	7.2 °C/W

**Note 10:** Specification assumes 9 thermal vias connect the die attach pad (DAP) to the embedded copper plane on the 4-layer JEDEC board. These vias play a key role in improving the thermal performance of the LLP. It is recommended that the maximum number of vias be used in the board layout.

**11.0 Electrical Characteristics** Unless otherwise specified:  $V_{CC} = 3.3 V \pm 5\%$ ,  $V_{CCO} = 3.3 V \pm 5\%$ ,  $2.5 V \pm 5\%$ ,  $-40\text{ °C} \leq T_A \leq 85\text{ °C}$ , CLKIn driven differentially, input slew rate  $\geq 3\text{ V/ns}$ . Typical values represent most likely parametric norms at  $V_{CC} = 3.3\text{ V}$ ,  $V_{CCO} = 3.3\text{ V}$ ,  $T_A = 25\text{ °C}$ , and at the Recommended Operation Conditions at the time of product characterization and are not guaranteed. (Note 8, Note 11)

Symbol	Parameter	Conditions	Min	Typ	Max	Units
<b>Current Consumption</b>						
$I_{CC\_CORE}$	Core Supply Current, All Outputs Disabled	CLKinX selected		8.5	10.5	mA
		OSCin selected		10	13.5	mA
$I_{CC\_PECL}$	Additive Core Supply Current, Per LVPECL Bank Enabled			20	26.5	mA
$I_{CC\_LVDS}$	Additive Core Supply Current, Per LVDS Bank Enabled			24	29.5	mA
$I_{CC\_HCSL}$	Additive Core Supply Current, Per HCSL Bank Enabled			29	35	mA
$I_{CC\_CMOS}$	Additive Core Supply Current, LVCMOS Output Enabled			3.5	5.5	mA
$I_{CCO\_PECL}$	Additive Output Supply Current, Per LVPECL Bank Enabled	Includes Output Bank Bias and Load Currents, $R_T = 50\ \Omega$ to $V_{CCO} - 2V$ on all outputs in bank		100	123	mA

Symbol	Parameter	Conditions		Min	Typ	Max	Units
$I_{CCO\_LVDS}$	Additive Output Supply Current, Per LVDS Bank Enabled				20	27.5	mA
$I_{CCO\_HCSL}$	Additive Output Supply Current, Per HCSL Bank Enabled	Includes Output Bank Bias and Load Currents, $R_T = 50 \Omega$ on all outputs in bank			50	65	mA
$I_{CCO\_CMOS}$	Additive Output Supply Current, LVCMOS Output Enabled	200 MHz, $C_L = 5 \text{ pF}$	$V_{CCO} = 3.3 \text{ V} \pm 5\%$		9	10	mA
			$V_{CCO} = 2.5 \text{ V} \pm 5\%$		7	8	mA
<b>Power Supply Ripple Rejection (PSRR)</b>							
$PSRR_{PECL}$	Ripple-Induced Phase Spur Level ( <i>Note 13</i> ) Differential LVPECL Output	100 kHz, 100 mVpp Ripple Injected on $V_{CCO}$ , $V_{CCO} = 2.5 \text{ V}$	156.25 MHz		-65		dBc
			312.5 MHz		-63		
$PSRR_{LVDS}$	Ripple-Induced Phase Spur Level ( <i>Note 13</i> ) Differential LVDS Output		156.25 MHz		-76		dBc
			312.5 MHz		-74		
$PSRR_{HCSL}$	Ripple-Induced Phase Spur Level ( <i>Note 13</i> ) Differential HCSL Output		156.25 MHz		-72		dBc
			312.5 MHz		-63		
<b>CMOS Control Inputs (CLKin_SELn, CLKoutX_TYPEn, REFOut_EN)</b>							
$V_{IH}$	High-Level Input Voltage			1.6		$V_{CC}$	V
$V_{IL}$	Low-Level Input Voltage			GND		0.4	V
$I_{IH}$	High-Level Input Current	$V_{IH} = V_{CC}$ , Internal pull-down resistor				50	$\mu\text{A}$
$I_{IL}$	Low-Level Input Current	$V_{IL} = 0 \text{ V}$ , Internal pull-down resistor		-5	0.1		$\mu\text{A}$
<b>Clock Inputs (CLKin0/CLKin0*, CLKin1/CLKin1*)</b>							
$f_{CLKin}$	Input Frequency Range ( <i>Note 20</i> )	Functional up to 3.1 GHz Output frequency range and timing specified per output type (refer to LVPECL, LVDS, HCSL, LVCMOS output specifications)		DC		3.1	GHz
$V_{IHD}$	Differential Input High Voltage	CLKin driven differentially				$V_{CC}$	V
$V_{ILD}$	Differential Input Low Voltage			GND			V
$V_{ID}$	Differential Input Voltage Swing ( <i>Note 14</i> )			0.15		1.3	V
$V_{CMD}$	Differential Input Common Mode Voltage	$V_{ID} = 150 \text{ mV}$		0.5		$V_{CC} - 1.2$	V
		$V_{ID} = 350 \text{ mV}$		0.5		$V_{CC} - 1.1$	
		$V_{ID} = 800 \text{ mV}$		0.5		$V_{CC} - 0.9$	
$V_{IH}$	Single-Ended Input High Voltage	CLKinX driven single-ended, CLKinX* AC coupled to GND		$V_{CM} + 0.15$		$V_{CC}$	V
$V_{IL}$	Single-Ended Input Low Voltage			GND		$V_{CM} - 0.15$	V
$V_{CM}$	Single-Ended Input Common Mode Voltage			0.5		$V_{CC} - 1.2$	V
$ISO_{MUX}$	Mux Isolation, CLKin0 to CLKin1	$f_{OFFSET} > 50 \text{ kHz}$ , $P_{CLKinX} = 0 \text{ dBm}$	$f_{CLKin0} = 100 \text{ MHz}$		-84		dBc
			$f_{CLKin0} = 200 \text{ MHz}$		-82		
			$f_{CLKin0} = 500 \text{ MHz}$		-71		
			$f_{CLKin0} = 1000 \text{ MHz}$		-65		

Symbol	Parameter	Conditions	Min	Typ	Max	Units
<b>Crystal Interface (OSCin, OSCout)</b>						
$F_{CLK}$	External Clock Frequency Range (Note 20)	OSCin driven single-ended, OSCout floating			250	MHz
$F_{XTAL}$	Crystal Frequency Range	Fundamental mode crystal ESR $\leq 200 \Omega$ (10 to 30 MHz) ESR $\leq 125 \Omega$ (30 to 40 MHz) (Note 15)	10		40	MHz
$C_{IN}$	OSCin Input Capacitance			1		pF
<b>LVPECL Outputs (CLKoutAn/CLKoutAn*, CLKoutBn/CLKoutBn*)</b>						
$f_{CLKout\_FS}$	Maximum Output Frequency Full $V_{OD}$ Swing (Note 20, Note 21)	$V_{OD} \geq 600$ mV, $R_L = 100 \Omega$ differential	$V_{CCO} = 3.3$ V $\pm 5\%$ , $R_T = 160 \Omega$ to GND	1.0	1.2	GHz
			$V_{CCO} = 2.5$ V $\pm 5\%$ , $R_T = 91 \Omega$ to GND	0.75	1.0	
$f_{CLKout\_RS}$	Maximum Output Frequency Reduced $V_{OD}$ Swing (Note 20, Note 21)	$V_{OD} \geq 400$ mV, $R_L = 100 \Omega$ differential	$V_{CCO} = 3.3$ V $\pm 5\%$ , $R_T = 160 \Omega$ to GND	1.5	3.1	GHz
			$V_{CCO} = 2.5$ V $\pm 5\%$ , $R_T = 91 \Omega$ to GND	1.5	2.3	
Jitter <sub>ADD</sub>	Additive RMS Jitter Integration Bandwidth 1 MHz to 20 MHz (Note 16)	$V_{CCO} = 3.3$ V, $R_T = 160 \Omega$ to GND, $R_L = 100 \Omega$ differential	CLKin: 100 MHz, Slew rate $\geq 3$ V/ns		59	fs
			CLKin: 156.25 MHz, Slew rate $\geq 2.7$ V/ns		64	
			CLKin: 625 MHz, Slew rate $\geq 3$ V/ns		30	
Jitter <sub>ADD</sub>	Additive RMS Jitter with LVPECL clock source from LMK03806 (Note 16, Note 17)	$V_{CCO} = 3.3$ V, $R_T = 160 \Omega$ to GND, $R_L = 100 \Omega$ differential	CLKin: 156.25 MHz, $J_{SOURCE} = 190$ fs RMS (10 kHz to 1 MHz)		20	fs
			CLKin: 156.25 MHz, $J_{SOURCE} = 195$ fs RMS (12 kHz to 20 MHz)		51	
Noise Floor	Noise Floor $f_{OFFSET} \geq 10$ MHz	$V_{CCO} = 3.3$ V, $R_T = 160 \Omega$ to GND, $R_L = 100 \Omega$ differential	CLKin: 100 MHz, Slew rate $\geq 3$ V/ns		-162.5	dBc/Hz
			CLKin: 156.25 MHz, Slew rate $\geq 2.7$ V/ns		-158.1	
			CLKin: 625 MHz, Slew rate $\geq 3$ V/ns		-154.4	
DUTY	Duty Cycle (Note 20)	50% input clock duty cycle	45		55	%
$V_{OH}$	Output High Voltage	$T_A = 25$ °C, DC Measurement, $R_T = 50 \Omega$ to $V_{CCO} - 2$ V	$V_{CCO} - 1.2$	$V_{CCO} - 0.9$	$V_{CCO} - 0.7$	V
$V_{OL}$	Output Low Voltage		$V_{CCO} - 2.0$	$V_{CCO} - 1.75$	$V_{CCO} - 1.5$	V
$V_{OD}$	Output Voltage Swing (Note 14)		600	830	1000	mV
$t_R$	Output Rise Time 20% to 80%	$R_T = 160 \Omega$ to GND, $R_L = 100 \Omega$ differential		175		ps
$t_F$	Output Fall Time 80% to 20%			175		ps

Symbol	Parameter	Conditions	Min	Typ	Max	Units
<b>LVDS Outputs (CLKoutAn/CLKoutAn*, CLKoutBn/CLKoutBn*)</b>						
$f_{\text{CLKout\_FS}}$	Maximum Output Frequency Full $V_{\text{OD}}$ Swing ( <i>Note 20, Note 21</i> )	$V_{\text{OD}} \geq 250$ mV, $R_{\text{L}} = 100 \Omega$ differential	1.0	1.6		GHz
$f_{\text{CLKout\_RS}}$	Maximum Output Frequency Reduced $V_{\text{OD}}$ Swing ( <i>Note 20, Note 21</i> )	$V_{\text{OD}} \geq 200$ mV, $R_{\text{L}} = 100 \Omega$ differential	1.5	2.1		GHz
$\text{Jitter}_{\text{ADD}}$	Additive RMS Jitter Integration Bandwidth 1 MHz to 20 MHz ( <i>Note 16</i> )	$V_{\text{CCO}} = 3.3$ V, $R_{\text{L}} = 100 \Omega$ differential	CLKin: 100 MHz, Slew rate $\geq 3$ V/ns	89		fs
			CLKin: 156.25 MHz, Slew rate $\geq 2.7$ V/ns	77		
			CLKin: 625 MHz, Slew rate $\geq 3$ V/ns	37		
Noise Floor	Noise Floor $f_{\text{OFFSET}} \geq 10$ MHz	$V_{\text{CCO}} = 3.3$ V, $R_{\text{L}} = 100 \Omega$ differential	CLKin: 100 MHz, Slew rate $\geq 3$ V/ns	-159.5		dBc/Hz
			CLKin: 156.25 MHz, Slew rate $\geq 2.7$ V/ns	-157.0		
			CLKin: 625 MHz, Slew rate $\geq 3$ V/ns	-152.7		
DUTY	Duty Cycle ( <i>Note 20</i> )	50% input clock duty cycle	45		55	%
$V_{\text{OD}}$	Output Voltage Swing ( <i>Note 14</i> )	$T_{\text{A}} = 25$ °C, DC Measurement, $R_{\text{L}} = 100 \Omega$ differential	250	400	450	mV
$\Delta V_{\text{OD}}$	Change in Magnitude of $V_{\text{OD}}$ for Complementary Output States		-50		50	mV
$V_{\text{OS}}$	Output Offset Voltage		1.125	1.25	1.375	V
$\Delta V_{\text{OS}}$	Change in Magnitude of $V_{\text{OS}}$ for Complementary Output States		-35		35	mV
$I_{\text{SA}}$ $I_{\text{SB}}$	Output Short Circuit Current Single Ended	$T_{\text{A}} = 25$ °C, Single ended outputs shorted to GND	-24		24	mA
$I_{\text{SAB}}$	Output Short Circuit Current Differential	Complementary outputs tied together	-12		12	mA
$t_{\text{R}}$	Output Rise Time 20% to 80%	$R_{\text{L}} = 100 \Omega$ differential		175		ps
$t_{\text{F}}$	Output Fall Time 80% to 20%			175		ps



Symbol	Parameter	Conditions	Min	Typ	Max	Units
<b>HCSL Outputs (CLKoutAn/CLKoutAn*, CLKoutBn/CLKoutBn*)</b>						
$f_{\text{CLKout}}$	Output Frequency Range (Note 20)	$R_L = 50 \Omega$ to GND, $C_L \leq 5 \text{ pF}$	DC		400	MHz
$\text{Jitter}_{\text{ADD}}$	Additive RMS Jitter Integration Bandwidth 1 MHz to 20 MHz (Note 16)	$V_{\text{CCO}} = 3.3 \text{ V}$ , $R_T = 50 \Omega$ to GND	CLKin: 100 MHz, Slew rate $\geq 3 \text{ V/ns}$	77		fs
			CLKin: 156.25 MHz, Slew rate $\geq 2.7 \text{ V/ns}$	86		
Noise Floor	Noise Floor $f_{\text{OFFSET}} \geq 10 \text{ MHz}$	$V_{\text{CCO}} = 3.3 \text{ V}$ , $R_T = 50 \Omega$ to GND	CLKin: 100 MHz, Slew rate $\geq 3 \text{ V/ns}$	-161.3		dBc/Hz
			CLKin: 156.25 MHz, Slew rate $\geq 2.7 \text{ V/ns}$	-156.3		
DUTY	Duty Cycle (Note 20)	50% input clock duty cycle	45		55	%
$V_{\text{OH}}$	Output High Voltage	$T_A = 25^\circ\text{C}$ , DC Measurement, $R_T = 50 \Omega$ to GND	520	810	920	mV
$V_{\text{OL}}$	Output Low Voltage		-150	0.5	150	mV
$V_{\text{CROSS}}$	Absolute Crossing Voltage (Note 20, Note 22)	$R_L = 50 \Omega$ to GND, $C_L \leq 5 \text{ pF}$	160	350	460	mV
$\Delta V_{\text{CROSS}}$	Total Variation of $V_{\text{CROSS}}$ (Note 20, Note 22)				140	mV
$t_{\text{R}}$	Output Rise Time 20% to 80% (Note 22)	250 MHz, $R_L = 50 \Omega$ to GND, $C_L \leq 5 \text{ pF}$		300		ps
$t_{\text{F}}$	Output Fall Time 80% to 20% (Note 22)			300		ps
<b>LVC MOS Output (REFout)</b>						
$f_{\text{CLKout}}$	Output Frequency Range (Note 20)	$C_L \leq 5 \text{ pF}$	DC		250	MHz
$\text{Jitter}_{\text{ADD}}$	Additive RMS Jitter Integration Bandwidth 1 MHz to 20 MHz (Note 16)	$V_{\text{CCO}} = 3.3 \text{ V}$ , $C_L \leq 5 \text{ pF}$	100 MHz, Input Slew rate $\geq 3 \text{ V/ns}$	95		fs
			100 MHz, Input Slew rate $\geq 3 \text{ V/ns}$	-159.3		
Noise Floor	Noise Floor $f_{\text{OFFSET}} \geq 10 \text{ MHz}$	$V_{\text{CCO}} = 3.3 \text{ V}$ , $C_L \leq 5 \text{ pF}$				dBc/Hz
DUTY	Duty Cycle (Note 20)	50% input clock duty cycle	45		55	%
$V_{\text{OH}}$	Output High Voltage	1 mA load	$V_{\text{CCO}} -$ 0.1			V
$V_{\text{OL}}$	Output Low Voltage				0.1	
$I_{\text{OH}}$	Output High Current (Source)	$V_o = V_{\text{CCO}} / 2$	$V_{\text{CCO}} = 3.3 \text{ V}$	28		mA
			$V_{\text{CCO}} = 2.5 \text{ V}$	20		
$I_{\text{OL}}$	Output Low Current (Sink)		$V_{\text{CCO}} = 3.3 \text{ V}$	28		mA
			$V_{\text{CCO}} = 2.5 \text{ V}$	20		
$t_{\text{R}}$	Output Rise Time 20% to 80% (Note 22)	250 MHz, $R_L = 50 \Omega$ to GND, $C_L \leq 5 \text{ pF}$		225		ps
$t_{\text{F}}$	Output Fall Time 80% to 20% (Note 22)			225		ps
$t_{\text{EN}}$	Output Enable Time (Note 23)	$C_L \leq 5 \text{ pF}$			3	cycles
$t_{\text{DIS}}$	Output Disable Time (Note 23)				3	cycles

Symbol	Parameter	Conditions	Min	Typ	Max	Units
<b>Propagation Delay and Output Skew</b>						
$t_{PD\_PECL}$	Propagation Delay CLKin-to-LVPECL	$R_T = 160 \Omega$ to GND, $R_L = 100 \Omega$ differential		360		ps
$t_{PD\_LVDS}$	Propagation Delay CLKin-to-LVDS	$R_L = 100 \Omega$ differential		400		ps
$t_{PD\_HCSL}$	Propagation Delay CLKin-to-HCSL ( <i>Note 22</i> )	$R_T = 50 \Omega$ to GND, $C_L \leq 5$ pF		590		ps
$t_{PD\_CMOS}$	Propagation Delay CLKin-to-LVCMOS ( <i>Note 22</i> )	$C_L \leq 5$ pF	$V_{CCO} = 3.3$ V	1475		ps
			$V_{CCO} = 2.5$ V	1550		
$t_{SK(O)}$	Output Skew LVPECL/LVDS/HCSL ( <i>Note 20, Note 22, Note 24</i> )	Skew specified between any two CLKouts with the same buffer type. Load conditions per output type are the same as propagation delay specifications.		30	50	ps
$t_{SK(PP)}$	Part-to-Part Output Skew LVPECL/LVDS/HCSL ( <i>Note 22, Note 24</i> )			80		ps

**Note 11:** The Electrical Characteristics tables list guaranteed specifications under the listed Recommended Operating Conditions except as otherwise modified or specified by the Electrical Characteristics Conditions and/or Notes. Typical specifications are estimations only and are not guaranteed.

**Note 12:** See [Section 14.4 Power Supply and Thermal Considerations](#) for more information on current consumption and power dissipation calculations.

**Note 13:** Power supply ripple rejection, or PSRR, is defined as the single-sideband phase spur level (in dBc) modulated onto the clock output when a single-tone sinusoidal signal (ripple) is injected onto the  $V_{CCO}$  supply. Assuming no amplitude modulation effects and small index modulation, the peak-to-peak deterministic jitter (DJ) can be calculated using the measured single-sideband phase spur level (PSRR) as follows:  $DJ$  (ps pk-pk) =  $[ (2 * 10^{(PSRR / 20)}) / (TT * f_{CLK}) ] * 1E12$

**Note 14:** See [Section 12.1 Differential Voltage Measurement Terminology](#) for definition of  $V_{ID}$  and  $V_{OD}$  voltages.

**Note 15:** The ESR requirements stated must be met to ensure that the oscillator circuitry has no startup issues. However, lower ESR values for the crystal may be necessary to stay below the maximum power dissipation (drive level) specification of the crystal. Refer to [Section 14.2 Crystal Interface](#) for crystal drive level considerations.

**Note 16:** For the 100 MHz and 156.25 MHz clock input conditions, Additive RMS Jitter ( $J_{ADD}$ ) is calculated using Method #1:  $J_{ADD} = \text{SQRT}(J_{OUT}^2 - J_{SOURCE}^2)$ , where  $J_{OUT}$  is the total RMS jitter measured at the output driver and  $J_{SOURCE}$  is the RMS jitter of the clock source applied to CLKin. For the 625 MHz clock input condition, Additive RMS Jitter is approximated using Method #2:  $J_{ADD} = \text{SQRT}(2 * 10^{dBc/10}) / (2 * TT * f_{CLK})$ , where dBc is the phase noise power of the Output Noise Floor integrated from 1 to 20 MHz bandwidth. The phase noise power can be calculated as:  $dBc = \text{Noise Floor} + 10 * \log_{10}(20 \text{ MHz} - 1 \text{ MHz})$ . The additive RMS jitter was approximated for 625 MHz using Method #2 because the RMS jitter of the clock source was not sufficiently low enough to allow practical use of Method #1. Refer to the “Noise Floor vs. CLKin Slew Rate” and “RMS Jitter vs. CLKin Slew Rate” plots in [Section 13.0 Typical Performance Characteristics](#).

**Note 17:** (*Note 16*) 156.25 MHz LVPECL clock source from LMK03806 with 20 MHz crystal reference (crystal part number: ECS-200-20-30BU-DU).  $J_{SOURCE} = 190$  fs RMS (10 kHz to 1 MHz) and 195 fs RMS (12 kHz to 20 MHz). Refer to the LMK03806 datasheet for more information.

**Note 18:** The noise floor of the output buffer is measured as the far-out phase noise of the buffer. Typically this offset is  $\geq 10$  MHz, but for lower frequencies this measurement offset can be as low as 5 MHz due to measurement equipment limitations.

**Note 19:** Phase noise floor will degrade as the clock input slew rate is reduced. Compared to a single-ended clock, a differential clock input (LVPECL, LVDS) will be less susceptible to degradation in noise floor at lower slew rates due to its common mode noise rejection. However, it is recommended to use the highest possible input slew rate for differential clocks to achieve optimal noise floor performance at the device outputs.

**Note 20:** Specification is guaranteed by characterization and is not tested in production.

**Note 21:** See [Section 13.0 Typical Performance Characteristics](#) for output operation over frequency.

**Note 22:** AC timing parameters for HCSL or CMOS are dependent on output capacitive loading.

**Note 23:** Output Enable Time is the number of input clock cycles it takes for the output to be enabled after REFout\_EN is pulled high. Similarly, Output Disable Time is the number of input clock cycles it takes for the output to be disabled after REFout\_EN is pulled low. The REFout\_EN signal should have an edge transition much faster than that of the input clock period for accurate measurement.

**Note 24:** Output skew is the propagation delay difference between any two outputs with identical output buffer type and equal loading while operating at the same supply voltage and temperature conditions.

## 12.0 Measurement Definitions

### 12.1 Differential Voltage Measurement Terminology

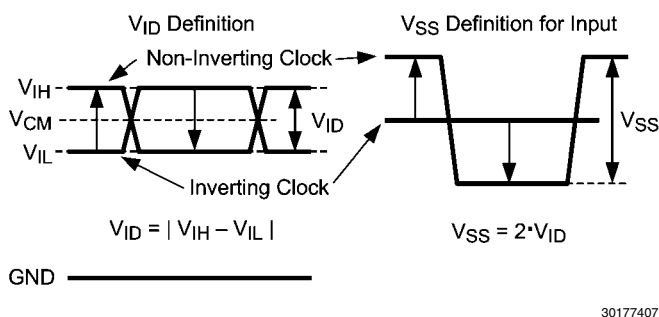
The differential voltage of a differential signal can be described by two different definitions causing confusion when reading datasheets or communicating with other engineers. This section will address the measurement and description of a differential signal so that the reader will be able to understand and discern between the two different definitions when used.

The first definition used to describe a differential signal is the absolute value of the voltage potential between the inverting and non-inverting signal. The symbol for this first measurement is typically  $V_{ID}$  or  $V_{OD}$  depending on if an input or output voltage is being described.

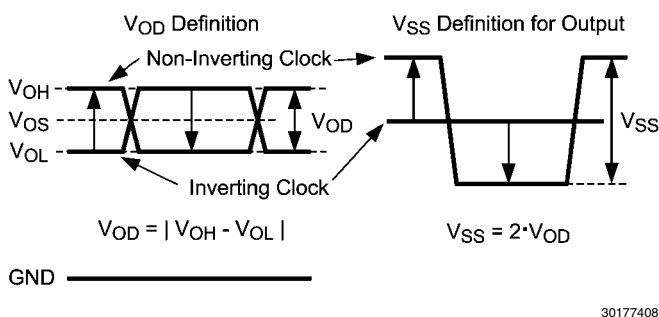
The second definition used to describe a differential signal is to measure the potential of the non-inverting signal with respect to the inverting signal. The symbol for this second measurement is  $V_{SS}$  and is a calculated parameter. Nowhere in the IC does this signal exist with respect to ground, it only exists in reference to its differential pair.  $V_{SS}$  can be measured directly by oscilloscopes with floating references, otherwise this value can be calculated as twice the value of  $V_{OD}$  as described in the first description.

*Figure 1* illustrates the two different definitions side-by-side for inputs and *Figure 2* illustrates the two different definitions side-by-side for outputs. The  $V_{ID}$  (or  $V_{OD}$ ) definition show the DC levels,  $V_{IH}$  and  $V_{OL}$  (or  $V_{OH}$  and  $V_{OL}$ ), that the non-inverting and inverting signals toggle between with respect to ground.  $V_{SS}$  input and output definitions show that if the inverting signal is considered the voltage potential reference, the non-inverting signal voltage potential is now increasing and decreasing above and below the non-inverting reference. Thus the peak-to-peak voltage of the differential signal can be measured.

$V_{ID}$  and  $V_{OD}$  are often defined as volts (V) and  $V_{SS}$  is often defined as volts peak-to-peak ( $V_{PP}$ ).



**FIGURE 1. Two Different Definitions for Differential Input Signals**



**FIGURE 2. Two Different Definitions for Differential Output Signals**

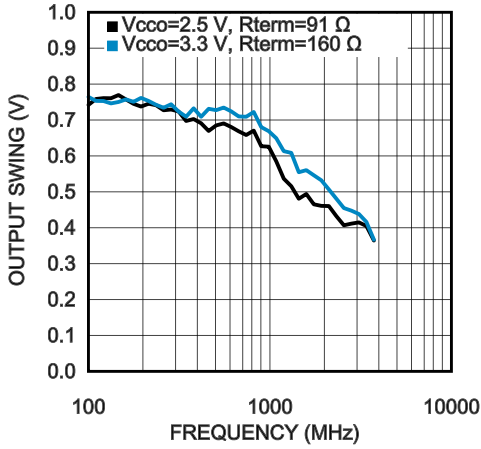
**Note 25:** Refer to Application Note AN-912 Common Data Transmission Parameters and their Definitions for more information.

### 13.0 Typical Performance Characteristics

Unless otherwise specified:  $V_{CC} = 3.3\text{ V}$ ,  $V_{CCO} = 3.3\text{ V}$ ,

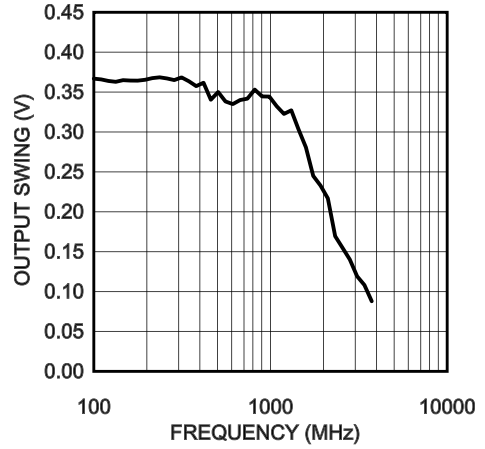
$T_A = 25\text{ }^\circ\text{C}$ , CLKin driven differentially, input slew rate  $\geq 3\text{ V/ns}$ .

LVPECL Output Swing ( $V_{OD}$ ) vs. Frequency



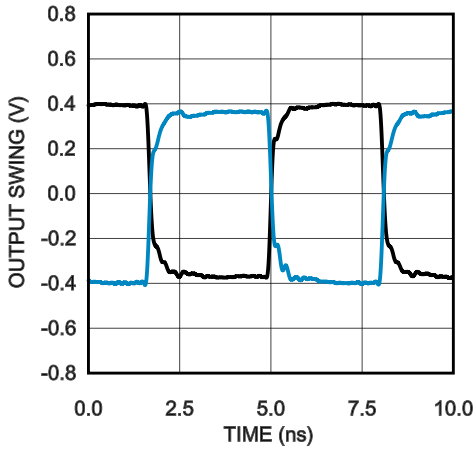
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LVDS Output Swing ( $V_{OD}$ ) vs. Frequency



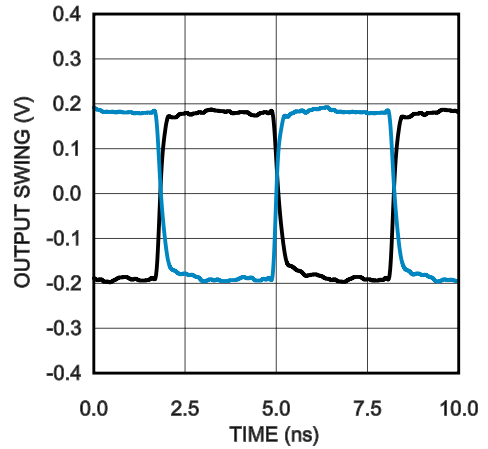
30177475

LVPECL Output Swing @ 156.25 MHz



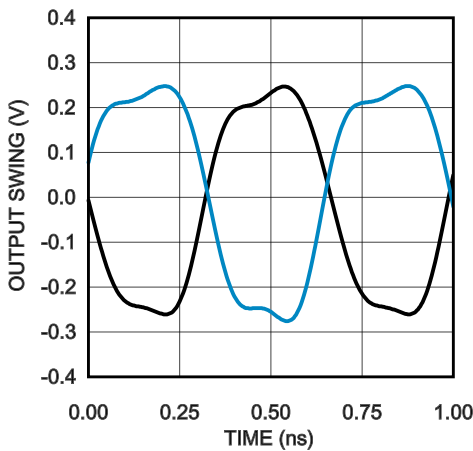
30177491

LVDS Output Swing @ 156.25 MHz



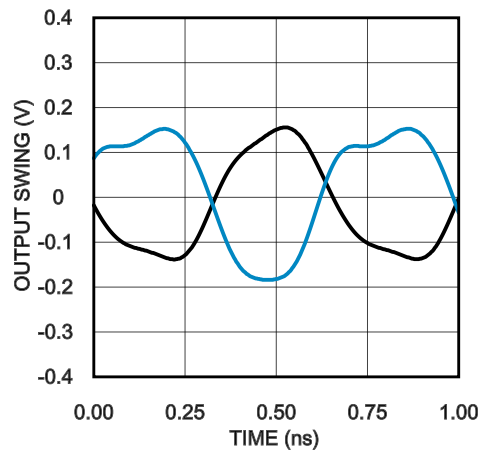
30177492

LVPECL Output Swing @ 1.5 GHz

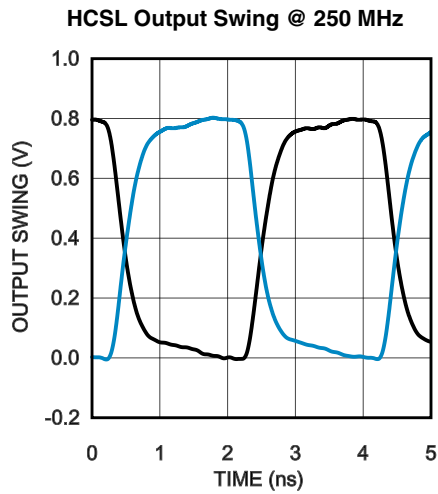


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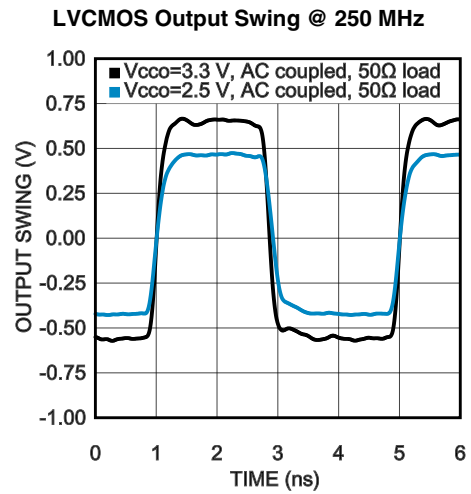
LVDS Output Swing @ 1.5 GHz



30177494

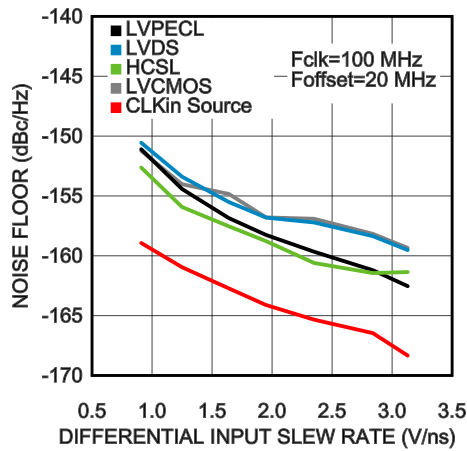


30177498



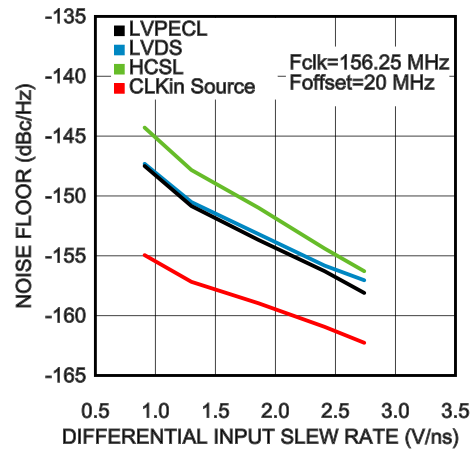
30177499

Noise Floor vs. CLKin Slew Rate @ 100 MHz



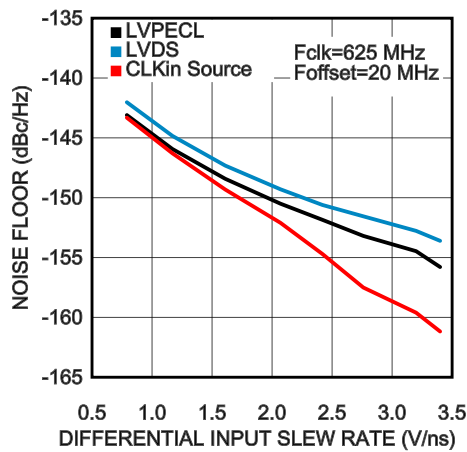
30177477

Noise Floor vs. CLKin Slew Rate @ 156.25 MHz



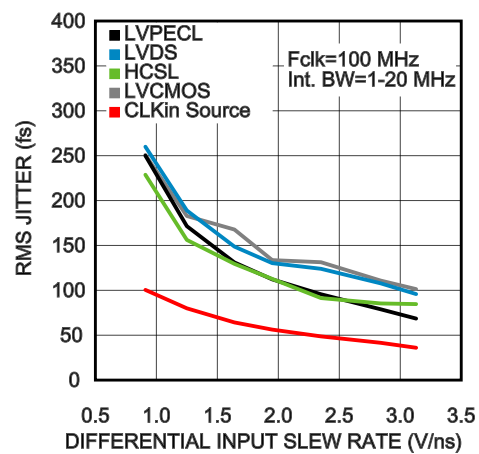
30177478

Noise Floor vs. CLKin Slew Rate @ 625 MHz



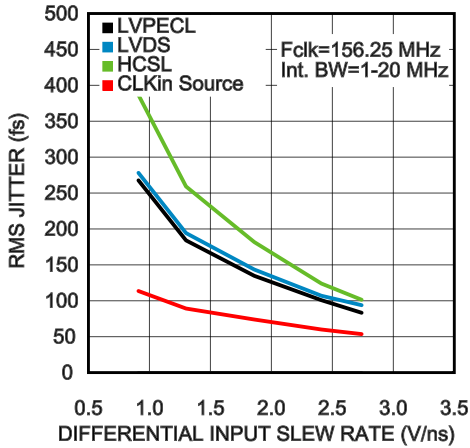
30177479

RMS Jitter vs. CLKin Slew Rate @ 100 MHz (Note 26)



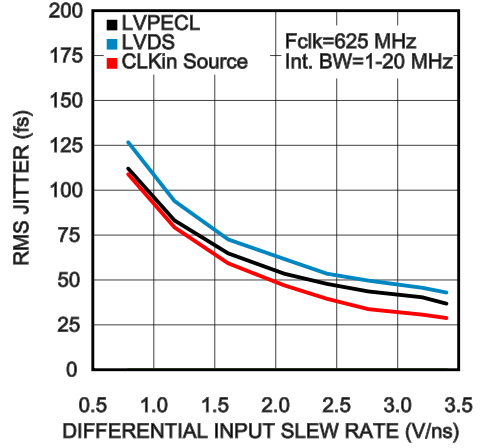
30177480

RMS Jitter vs. CLKin Slew Rate @ 156.25 MHz (Note 26)



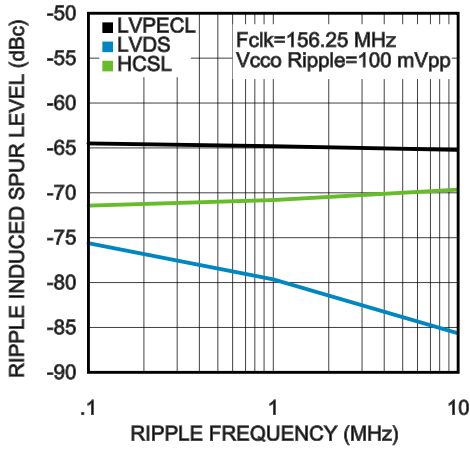
30177481

RMS Jitter vs. CLKin Slew Rate @ 625 MHz



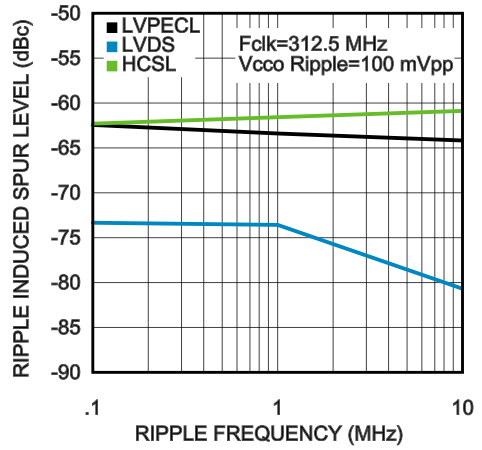
30177482

PSRR vs. Ripple Frequency @ 156.25 MHz



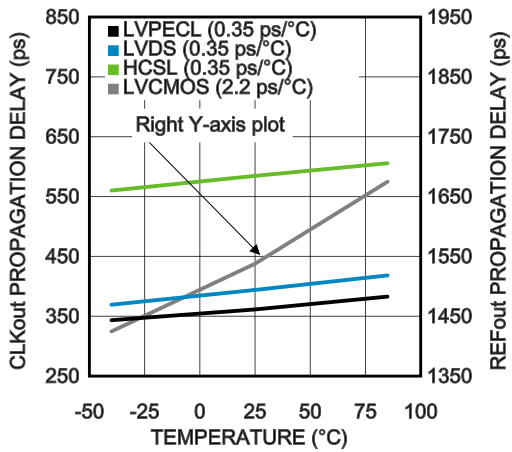
30177483

PSRR vs. Ripple Frequency @ 312.5 MHz



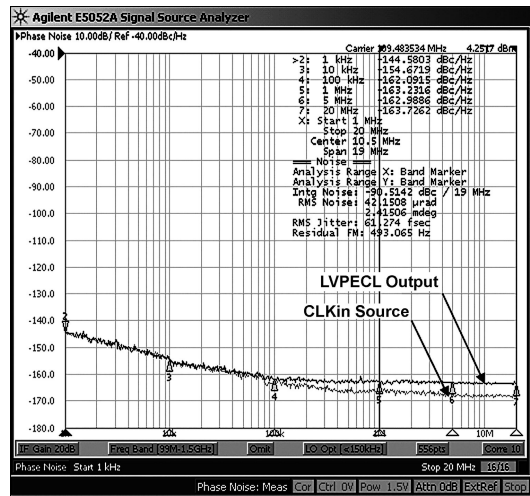
30177484

Propagation Delay vs. Temperature



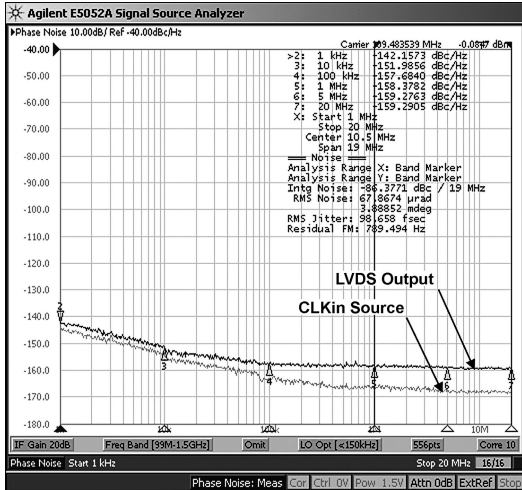
30177485

LVPECL Phase Noise @ 100 MHz (Note 26)



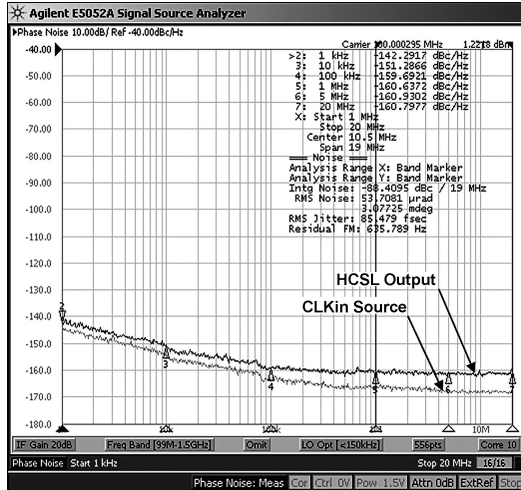
30177495

LVDS Phase Noise @ 100 MHz (Note 26)



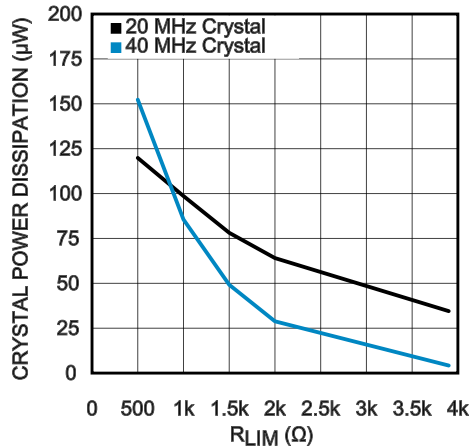
30177496

HCSSL Phase Noise @ 100 MHz (Note 26)



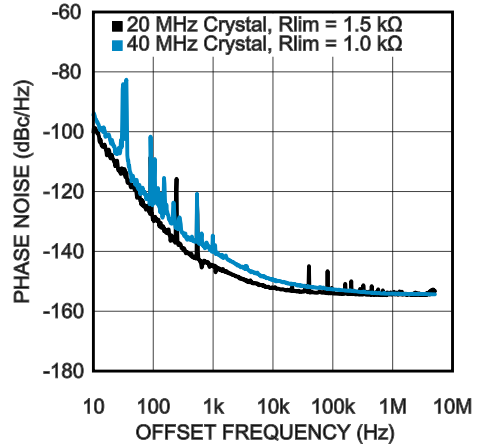
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Crystal Power Dissipation vs.  $R_{LIM}$  (Note 27, Note 28)



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LVDS Phase Noise in Crystal Mode (Note 27, Note 28)



30177432

**Note 26:** The typical RMS jitter values in the plots show the total output RMS jitter ( $J_{OUT}$ ) for each output buffer type and the source clock RMS jitter ( $J_{SOURCE}$ ). From these values, the Additive RMS Jitter can be calculated as:  $J_{ADD} = \text{SQRT}(J_{OUT}^2 - J_{SOURCE}^2)$ .

**Note 27:** 20 MHz crystal characteristics: Abracon ABL series, AT cut,  $C_L = 18$  pF,  $C_0 = 4.4$  pF measured (7 pF max), ESR = 8.5  $\Omega$  measured (40  $\Omega$  max), and Drive Level = 1 mW max (100  $\mu$ W typical).

**Note 28:** 40 MHz crystal characteristics: Abracon ABL2 series, AT cut,  $C_L = 18$  pF,  $C_0 = 5$  pF measured (7 pF max), ESR = 5  $\Omega$  measured (40  $\Omega$  max), and Drive Level = 1 mW max (100  $\mu$ W typical).

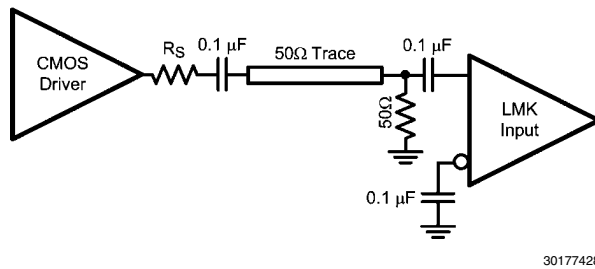
## 14.0 Application Information

### 14.1 Driving the Clock Inputs

The LMK00306 has two universal inputs (CLKin0/CLKin0\* and CLKin1/CLKin1\*) that can accept AC- or DC-coupled 3.3V/2.5V LVPECL, LVDS, CML, SSTL, and other differential and single-ended signals that meet the input requirements specified in [Section 11.0 Electrical Characteristics](#). The device can accept a wide range of signals due to its wide input common mode voltage range ( $V_{CM}$ ) and input voltage swing ( $V_{ID}$ ) / dynamic range. For 50% duty cycle and DC-balanced signals, AC coupling may also be employed to shift the input signal to within the  $V_{CM}$  range. Refer to [Section 14.3 Termination and Use of Clock Drivers](#) for signal interfacing and termination techniques.

To achieve the best possible phase noise and jitter performance, it is mandatory for the input to have high slew rate of 3 V/ns (differential) or higher. Driving the input with a lower slew rate will degrade the noise floor and jitter. For this reason, a differential signal input is recommended over single-ended because it typically provides higher slew rate and common-mode-rejection. Refer to the “Noise Floor vs. CLKin Slew Rate” and “RMS Jitter vs. CLKin Slew Rate” plots in [Section 13.0 Typical Performance Characteristics](#).

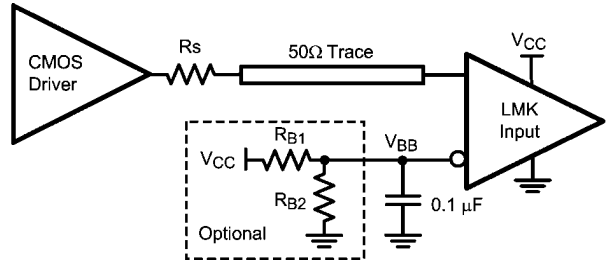
While it is recommended to drive the CLKin0 and CLKin1 with a differential signal input, it is possible to drive them with a single-ended clock. Again, the single-ended input slew rate should be as high as possible to minimize performance degradation. The CLKin input has an internal bias voltage of about 1.4 V, so the input can be AC coupled as shown in [Figure 3](#).



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**FIGURE 3. Single-Ended LVCMOS Input, AC Coupling**

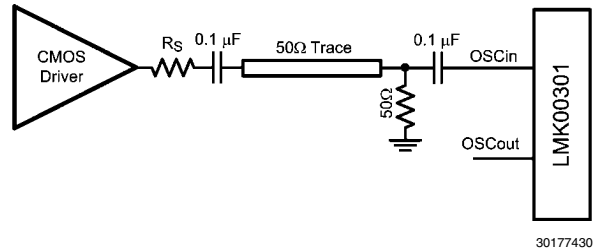
A single-ended clock may also be DC coupled to CLKinX as shown in [Figure 4](#). If the DC coupled input swing has a common mode level near the device's internal bias voltage of 1.4 V, then only a 0.1 uF bypass cap is required on CLKinX\*. Otherwise, if the input swing is not optimally centered near the internal bias voltage, then CLKinX\* should be externally biased to the midpoint voltage of the input swing. This can be achieved using external biasing resistors,  $R_{B1}$  and  $R_{B2}$ , or another low-noise voltage reference. The external bias voltage should be within the specified input common voltage ( $V_{CM}$ ) range. This will ensure the input swing crosses the threshold voltage at a point where the input slew rate is the highest.



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**FIGURE 4. Single-Ended LVCMOS Input, DC Coupling with Common Mode Biasing**

If the crystal oscillator circuit is not used, it is possible to drive the OSCin input with a single-ended external clock as shown in [Figure 5](#). The input clock should be AC coupled to the OSCin pin, which has an internally-generated input bias voltage, and the OSCout pin should be left floating. While OSCin provides an alternative input to multiplex an external clock, it is recommended to use either universal input (CLKinX) since it offers higher operating frequency, better common mode and power supply noise rejection, and greater performance over supply voltage and temperature variations.

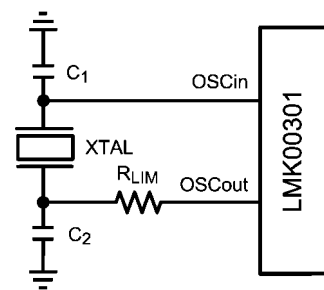


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**FIGURE 5. Driving OSCin with a Single-Ended Input**

### 14.2 Crystal Interface

The LMK00306 has an integrated crystal oscillator circuit that supports a fundamental mode, AT-cut crystal. The crystal interface is shown in [Figure 6](#).



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**FIGURE 6. Crystal Interface**

The load capacitance ( $C_L$ ) is specific to the crystal, but usually on the order of 18 - 20 pF. While  $C_L$  is specified for the crystal, the OSCin input capacitance ( $C_{IN} = 1$  pF typical) of the device and PCB stray capacitance ( $C_{STRAY} \sim 1\sim3$  pF) can affect the discrete load capacitor values,  $C_1$  and  $C_2$ .

For the parallel resonant circuit, the discrete capacitor values can be calculated as follows:

$$C_L = (C_1 * C_2) / (C_1 + C_2) + C_{IN} + C_{STRAY} \quad (1)$$



Typically,  $C_1 = C_2$  for optimum symmetry, so Equation 1 can be rewritten in terms of  $C_1$  only:

$$C_L = C_1^2 / (2 * C_1) + C_{IN} + C_{STRAY} \quad (2)$$

Finally, solve for  $C_1$ :

$$C_1 = (C_L - C_{IN} - C_{STRAY}) * 2 \quad (3)$$

Section 11.0 Electrical Characteristics provides crystal interface specifications with conditions that ensure start-up of the crystal, but it does not specify crystal power dissipation. The designer will need to ensure the crystal power dissipation does not exceed the maximum drive level specified by the crystal manufacturer. Overdriving the crystal can cause premature aging, frequency shift, and eventual failure. Drive level should be held at a sufficient level necessary to start-up and maintain steady-state operation.

The power dissipated in the crystal,  $P_{XTAL}$ , can be computed by:

$$P_{XTAL} = I_{RMS}^2 * R_{ESR} * (1 + C_0/C_L)^2 \quad (4)$$

Where:

- $I_{RMS}$  is the RMS current through the crystal.
  - $R_{ESR}$  is the max. equivalent series resistance specified for the crystal
  - $C_L$  is the load capacitance specified for the crystal
  - $C_0$  is the min. shunt capacitance specified for the crystal
- $I_{RMS}$  can be measured using a current probe (e.g. Tektronix CT-6 or equivalent) placed on the leg of the crystal connected to OSCout with the oscillation circuit active.

As shown in Figure 6, an external resistor,  $R_{LIM}$ , can be used to limit the crystal drive level, if necessary. If the power dissipated in the selected crystal is higher than the drive level specified for the crystal with  $R_{LIM}$  shorted, then a larger resistor value is mandatory to avoid overdriving the crystal. However, if the power dissipated in the crystal is less than the drive level with  $R_{LIM}$  shorted, then a zero value for  $R_{LIM}$  can be used. As a starting point, a suggested value for  $R_{LIM}$  is 1.5 k $\Omega$ .

### 14.3 Termination and Use of Clock Drivers

When terminating clock drivers keep in mind these guidelines for optimum phase noise and jitter performance:

- Transmission line theory should be followed for good impedance matching to prevent reflections.
- Clock drivers should be presented with the proper loads.
  - LVDS outputs are current drivers and require a closed current loop.
  - HCSL drivers are switched current outputs and require a DC path to ground via 50  $\Omega$  termination.
  - LVPECL outputs are open emitter and require a DC path to ground.
- Receivers should be presented with a signal biased to their specified DC bias level (common mode voltage) for proper operation. Some receivers have self-biasing inputs that automatically bias to the proper voltage level; in this case, the signal should normally be AC coupled.

It is possible to drive a non-LVPECL or non-LVDS receiver with a LVDS or LVPECL driver as long as the above guidelines are followed. Check the datasheet of the receiver or input being driven to determine the best termination and coupling method to be sure the receiver is biased at the optimum DC voltage (common mode voltage).

#### 14.3.1 Termination for DC Coupled Differential Operation

For DC coupled operation of an LVDS driver, terminate with 100  $\Omega$  as close as possible to the LVDS receiver as shown in Figure 7.

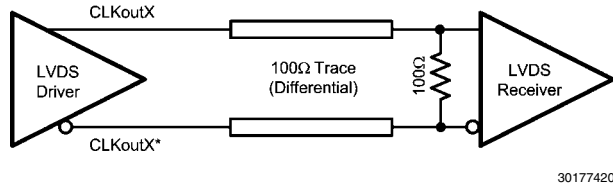


FIGURE 7. Differential LVDS Operation, DC Coupling, No Biasing by the Receiver

For DC coupled operation of an HCSL driver, terminate with 50  $\Omega$  to ground near the driver output as shown in Figure 8. Series resistors,  $R_s$ , may be used to limit overshoot due to the fast transient current. Because HCSL drivers require a DC path to ground, AC coupling is not allowed between the output drivers and the 50  $\Omega$  termination resistors.

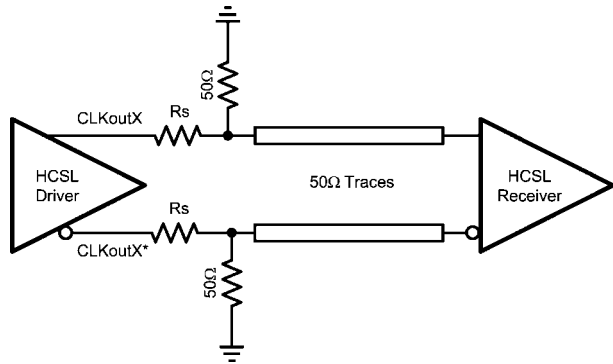


FIGURE 8. HCSL Operation, DC Coupling

For DC coupled operation of an LVPECL driver, terminate with 50  $\Omega$  to  $V_{CC0} - 2V$  as shown in Figure 9. Alternatively terminate with a Thevenin equivalent circuit as shown in Figure 10 for  $V_{CC0}$  (output driver supply voltage) = 3.3 V and 2.5 V. In the Thevenin equivalent circuit, the resistor dividers set the output termination voltage ( $V_{TT}$ ) to  $V_{CC0} - 2V$ .

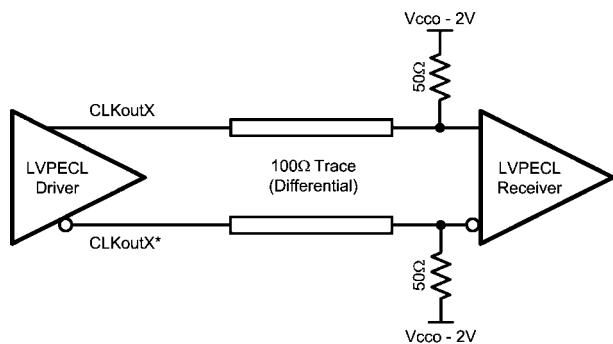
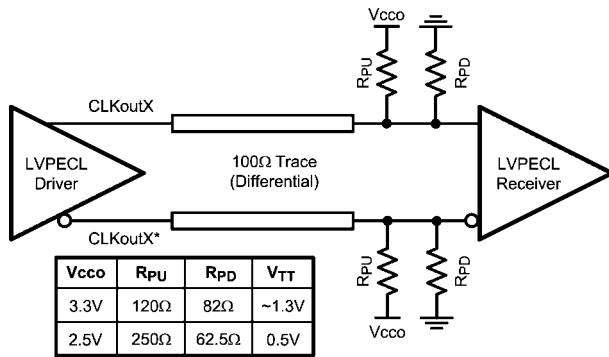


FIGURE 9. Differential LVPECL Operation, DC Coupling



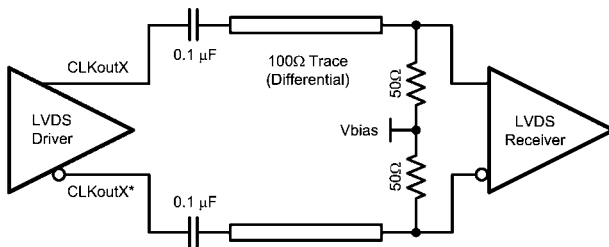
30177422

FIGURE 10. Differential LVPECL Operation, DC Coupling, Thevenin Equivalent

14.3.2 Termination for AC Coupled Differential Operation

AC coupling allows for shifting the DC bias level (common mode voltage) when driving different receiver standards. Since AC coupling prevents the driver from providing a DC bias voltage at the receiver, it is important to ensure the receiver is biased to its ideal DC level.

When driving non-biased LVDS receivers with an LVDS driver, the signal may be AC coupled by adding DC blocking capacitors; however the proper DC bias point needs to be established at the receiver. One way to do this is with the termination circuitry in Figure 11. When driving self-biased LVDS receivers, the circuit shown in Figure 11 may be modified by replacing the 50 Ω terminations to V<sub>bias</sub> with a single 100 Ω resistor across the input pins of the receiver. When using AC coupling with LVDS outputs, there may be a startup delay observed in the clock output due to capacitor charging. The previous example uses a 0.1 μF capacitor, but this may need to be adjusted to meet the startup requirements for the particular application. Another variant of AC coupling to a self-biased LVDS receiver is to move the 0.1 μF capacitors between the 100 Ω differential termination and the receiver inputs.

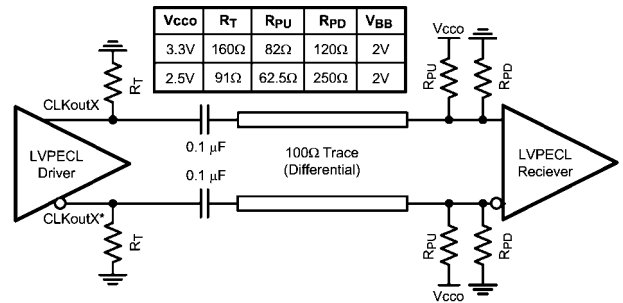


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FIGURE 11. Differential LVDS Operation, AC Coupling, No Biasing by the Receiver

LVPECL drivers require a DC path to ground. When AC coupling an LVPECL signal use 160 Ω emitter resistors (or 91 Ω for V<sub>CCO</sub> = 2.5 V) close to the LVPECL driver to provide a DC path to ground as shown in Figure 15. For proper receiver operation, the signal should be biased to the DC bias level (common mode voltage) specified by the receiver. The typical DC bias voltage (common mode voltage) for LVPECL receivers is 2 V. Alternatively, a Thevenin equivalent circuit forms a valid termination as shown in Figure 12 for V<sub>CCO</sub> = 3.3 V and 2.5 V. Note: this Thevenin circuit is different from the

DC coupled example in Figure 10, since the voltage divider is setting the input common mode voltage of the receiver.



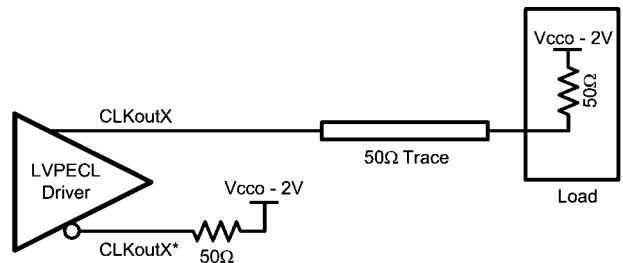
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FIGURE 12. Differential LVPECL Operation, AC Coupling, Thevenin Equivalent

14.3.3 Termination for Single-Ended Operation

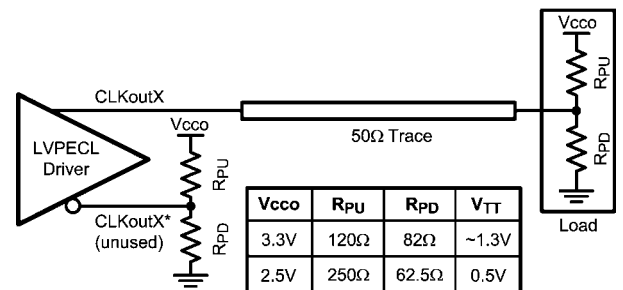
A balun can be used with either LVDS or LVPECL drivers to convert the balanced, differential signal into an unbalanced, single-ended signal.

It is possible to use an LVPECL driver as one or two separate 800 mV p-p signals. When DC coupling one of the LMK00306 LVPECL driver of a CLKoutX/CLKoutX\* pair, be sure to properly terminate the unused driver. When DC coupling on of the LMK00306 LVPECL drivers, the termination should be 50 Ω to V<sub>CCO</sub> - 2 V as shown in Figure 13. The Thevenin equivalent circuit is also a valid termination as shown in Figure 14 for V<sub>CCO</sub> = 3.3 V.



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FIGURE 13. Single-Ended LVPECL Operation, DC Coupling

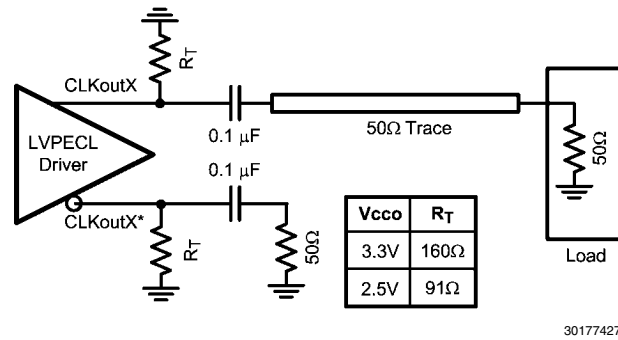


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FIGURE 14. Single-Ended LVPECL Operation, DC Coupling, Thevenin Equivalent

When AC coupling an LVPECL driver use a 160 Ω emitter resistor (or 91 Ω for V<sub>CCO</sub> = 2.5 V) to provide a DC path to ground and ensure a 50 Ω termination with the proper DC bias level for the receiver. The typical DC bias voltage for LVPECL

receivers is 2 V. If the companion driver is not used, it should be terminated with either a proper AC or DC termination. This latter example of AC coupling a single-ended LVPECL signal can be used to measure single-ended LVPECL performance using a spectrum analyzer or phase noise analyzer. When using most RF test equipment no DC bias point (0 VDC) is required for safe and proper operation. The internal 50  $\Omega$  termination the test equipment correctly terminates the LVPECL driver being measured as shown in [Figure 15](#). When using only one LVPECL driver of a CLKoutX/CLKoutX\* pair, be sure to properly terminate the unused driver.



**FIGURE 15. Single-Ended LVPECL Operation, AC Coupling**

## 14.4 Power Supply and Thermal Considerations

### 14.4.1 Current Consumption and Power Dissipation Calculations

The current consumption values specified in [Section 11.0 Electrical Characteristics](#) can be used to calculate the total power dissipation and IC power dissipation for any device configuration. The total  $V_{CC}$  core supply current ( $I_{CC\_TOTAL}$ ) can be calculated using [Equation 5](#):

$$I_{CC\_TOTAL} = I_{CC\_CORE} + I_{CC\_BANK\_A} + I_{CC\_BANK\_B} + I_{CC\_CMOS} \quad (5)$$

Where:

- $I_{CC\_CORE}$  is the current for core logic and input blocks and depends on selected input (CLKinX or OSCin).
- $I_{CC\_BANK\_A}$  is the current for Bank A and depends on output type ( $I_{CC\_PECL}$ ,  $I_{CC\_LVDS}$ ,  $I_{CC\_HCSL}$ , or 0 mA if disabled).
- $I_{CC\_BANK\_B}$  is the current for Bank B and depends on output type ( $I_{CC\_PECL}$ ,  $I_{CC\_LVDS}$ ,  $I_{CC\_HCSL}$ , or 0 mA if disabled).
- $I_{CC\_CMOS}$  is the current for the LVCMOS output (or 0 mA if REFout is disabled).

Since the output supplies ( $V_{CCOA}$ ,  $V_{CCOB}$ ,  $V_{CCOC}$ ) can be powered from 3 independent voltages, the respective output supply currents ( $I_{CCO\_BANK\_A}$ ,  $I_{CCO\_BANK\_B}$ , and  $I_{CCO\_CMOS}$ ) should be calculated separately.

$I_{CCO\_BANK}$  for either Bank A or B can be directly taken from the corresponding output supply current spec ( $I_{CCO\_PECL}$ ,  $I_{CCO\_LVDS}$ , or  $I_{CCO\_HCSL}$ ) **provided the output loading matches the specified conditions**. Otherwise,  $I_{CCO\_BANK}$  should be calculated as follows:

$$I_{CCO\_BANK} = I_{BANK\_BIAS} + (N * I_{OUT\_LOAD}) \quad (6)$$

Where:

- $I_{BANK\_BIAS}$  is the output bank bias current (fixed value).
- $I_{OUT\_LOAD}$  is the DC load current per loaded output pair.
- N is the number of loaded output pairs per bank (N = 0 to 3).

[Table 5](#) shows the typical  $I_{BANK\_BIAS}$  values and  $I_{OUT\_LOAD}$  expressions for LVPECL, LVDS, and HCSL.

For LVPECL, it is possible to use a larger termination resistor ( $R_T$ ) to ground instead of terminating with  $50 \Omega$  to  $V_{TT} = V_{CCO} - 2 V$ ; this technique is commonly used to eliminate the extra termination voltage supply ( $V_{TT}$ ) and potentially reduce device power dissipation at the expense of lower output swing. For example, when  $V_{CCO}$  is 3.3 V, a  $R_T$  value of  $160 \Omega$  to ground will eliminate the 1.3 V termination supply without sacrificing much output swing. In this case, the typical  $I_{OUT\_LOAD}$  is 25 mA, so  $I_{CCO\_PECL}$  for a fully-loaded bank reduces to 95 mA (vs. 100 mA with  $50 \Omega$  resistors to  $V_{CCO} - 2 V$ ).

**TABLE 5. Typical Output Bank Bias and Load Currents**

Current Parameter	LVPECL	LVDS	HCSL
$I_{BANK\_BIAS}$	20 mA	17.4 mA	3.6 mA
$I_{OUT\_LOAD}$	$(V_{OH} - V_{TT})/R_T + (V_{OL} - V_{TT})/R_T$	0 mA (No DC load current)	$V_{OH}/R_T$

Once the current consumption is known for each supply, the total power dissipation ( $P_{TOTAL}$ ) can be calculated as:

$$P_{TOTAL} = (V_{CC} * I_{CC\_TOTAL}) + (V_{CCOA} * I_{CCO\_BANK\_A}) + (V_{CCOB} * I_{CCO\_BANK\_B}) + (V_{CCOC} * I_{CCO\_CMOS}) \quad (7)$$

If the device is configured with LVPECL or HCSL outputs, then it is also necessary to calculate the power dissipated in any termination resistors ( $P_{RT\_PECL}$  and  $P_{RT\_HCSL}$ ) and in any LVPECL termination voltages ( $P_{VTT\_PECL}$ ). The external power dissipation values can be calculated as follows:

$$P_{RT\_PECL} \text{ (per LVPECL pair)} = (V_{OH} - V_{TT})^2/R_T + (V_{OL} - V_{TT})^2/R_T \quad (8)$$

$$P_{VTT\_PECL} \text{ (per LVPECL pair)} = V_{TT} * [(V_{OH} - V_{TT})/R_T + (V_{OL} - V_{TT})/R_T] \quad (9)$$

$$P_{RT\_HCSL} \text{ (per HCSL pair)} = V_{OH}^2 / R_T \quad (10)$$

Finally, the IC power dissipation ( $P_{DEVICE}$ ) can be computed by subtracting the external power dissipation values from  $P_{TOTAL}$  as follows:

$$P_{DEVICE} = P_{TOTAL} - N_1 * (P_{RT\_PECL} + P_{VTT\_PECL}) - N_2 * P_{RT\_HCSL} \quad (11)$$

Where:

- $N_1$  is the number of LVPECL output pairs with termination resistors to  $V_{TT}$  (usually  $V_{CCO} - 2 V$  or GND).
- $N_2$  is the number of HCSL output pairs with termination resistors to GND.

#### 14.4.1.1 Power Dissipation Example: Worst-Case Dissipation

This example shows how to calculate IC power dissipation for a configuration to estimate **worst-case power dissipation**. In this case, the maximum supply voltage and supply current values specified in [Section 11.0 Electrical Characteristics](#) are used.

- $V_{CC} = V_{CC0} = 3.465 \text{ V}$ . Max  $I_{CC}$  and  $I_{CC0}$  values.
- CLKin0/CLKin0\* input is selected.
- Banks A and B are configured for LVPECL: all outputs terminated with  $50 \Omega$  to  $V_T = V_{CC0} - 2 \text{ V}$ .
- REFout is enabled with 5 pF load.
- $T_A = 85 \text{ }^\circ\text{C}$

Using the power calculations from the previous section and *maximum* supply current specifications, we can compute  $P_{TOTAL}$  and  $P_{DEVICE}$ :

- From [Equation 5](#):  $I_{CC\_TOTAL} = 10.5 \text{ mA} + 22.5 \text{ mA} + 22.5 \text{ mA} + 5.5 \text{ mA} = 61 \text{ mA}$
- From  $I_{CC0\_PECL}$  max spec:  $I_{CC0\_BANK\_A} = I_{CC0\_BANK\_B} = 115 \text{ mA}$
- From [Equation 7](#):  $P_{TOTAL} = 3.465 \text{ V} * (61 \text{ mA} + 115 \text{ mA} + 115 \text{ mA} + 10 \text{ mA}) = 1043 \text{ mW}$
- From [Equation 8](#):  $P_{RT\_PECL} = ((2.57 \text{ V} - 1.47 \text{ V})^2 / 50 \Omega) + ((1.72 \text{ V} - 1.47 \text{ V})^2 / 50 \Omega) = 25.5 \text{ mW}$  (per output pair)
- From [Equation 9](#):  $P_{VTT\_PECL} = 1.47 \text{ V} * [ ((2.57 \text{ V} - 1.47 \text{ V}) / 50 \Omega) + ((1.72 \text{ V} - 1.47 \text{ V}) / 50 \Omega) ] = 39.5 \text{ mW}$  (per output pair)
- From [Equation 10](#):  $P_{RT\_HCSL} = 0 \text{ mW}$  (no HCSL outputs)
- From [Equation 11](#):  $P_{DEVICE} = 1043 \text{ mW} - (6 * (25.5 \text{ mW} + 39.5 \text{ mW})) - 0 \text{ mW} = 653 \text{ mW}$

In this worst-case example, the IC device will dissipate about 653 mW or 63% of the total power (1043 mW), while the remaining 37% will be dissipated in the LVPECL emitter resistors (153 mW for 6 pairs) and termination voltage (237 mW into  $V_{CC0} - 2 \text{ V}$ ). Based on  $\theta_{JA}$  of 31.8  $^\circ\text{C}/\text{W}$ , the estimated die junction temperature would be about 21  $^\circ\text{C}$  above ambient, or 106  $^\circ\text{C}$  when  $T_A = 85 \text{ }^\circ\text{C}$ .

### 14.4.2 Power Supply Bypassing

The Vcc and Vcco power supplies should have a high-frequency bypass capacitor, such as 0.1 uF or 0.01 uF, placed very close to each supply pin. 1 uF to 10 uF decoupling capacitors should also be placed nearby the device between the supply and ground planes. All bypass and decoupling capacitors should have short connections to the supply and ground plane through a short trace or via to minimize series inductance.

#### 14.4.2.1 Power Supply Ripple Rejection

In practical system applications, power supply noise (ripple) can be generated from switching power supplies, digital ASICs or FPGAs, etc. While power supply bypassing will help filter out some of this noise, it is important to understand the effect of power supply ripple on the device performance. When a single-tone sinusoidal signal is applied to the power supply of a clock distribution device, such as LMK00306, it can produce narrow-band phase modulation as well as amplitude modulation on the clock output (carrier). In the single-side band phase noise spectrum, the ripple-induced phase modulation appears as a phase spur level relative to the carrier (measured in dBc).

For the LMK00306, power supply ripple rejection, or PSRR, was measured as the single-sideband phase spur level (in dBc) modulated onto the clock output when a ripple signal was injected onto the Vcco supply. The PSRR test setup is shown in *Figure 16*.

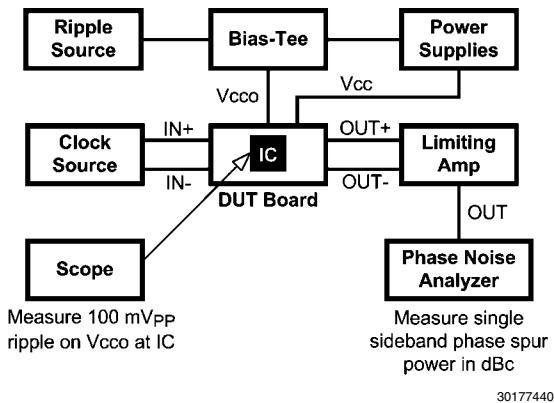


FIGURE 16. PSRR Test Setup

A signal generator was used to inject a sinusoidal signal onto the Vcco supply of the DUT board, and the peak-to-peak ripple amplitude was measured at the Vcco pins of the device. A limiting amplifier was used to remove amplitude modulation on the differential output clock and convert it to a single-ended signal for the phase noise analyzer. The phase spur level measurements were taken for clock frequencies of 156.25 MHz and 312.5 MHz under the following power supply ripple conditions:

- Ripple amplitude: 100 mVpp on Vcco = 2.5 V
- Ripple frequencies: 100 kHz, 1 MHz, and 10 MHz

Assuming no amplitude modulation effects and small index modulation, the peak-to-peak deterministic jitter (DJ) can be calculated using the measured single-sideband phase spur level (PSRR) as follows:

$$DJ \text{ (ps pk-pk)} = [(2 \cdot 10^{(PSRR / 20)}) / (\pi \cdot f_{CLK})] \cdot 10^{12} \quad (12)$$

The "PSRR vs. Ripple Frequency" plots in *Section 13.0 Typical Performance Characteristics* show the ripple-induced

phase spur levels for the differential output types at 156.25 MHz and 312.5 MHz. The LMK00306 exhibits very good and well-behaved PSRR characteristics across the ripple frequency range for all differential output types. The phase spur levels for LVPECL are below -64 dBc at 156.25 MHz and below -62 dBc at 312.5 MHz. Using *Equation 12*, these phase spur levels translate to Deterministic Jitter values of 2.57 ps pk-pk at 156.25 MHz and 1.62 ps pk-pk at 312.5 MHz. Testing has shown that the PSRR performance of the device improves for Vcco = 3.3 V under the same ripple amplitude and frequency conditions.

#### 14.4.3 Thermal Management

Power dissipation in the LMK00306 device can be high enough to require attention to thermal management. For reliability and performance reasons the die temperature should be limited to a maximum of 125 °C. That is, as an estimate, T<sub>A</sub> (ambient temperature) plus device power dissipation times θ<sub>JA</sub> should not exceed 125 °C.

The package of the device has an exposed pad that provides the primary heat removal path as well as excellent electrical grounding to the printed circuit board. To maximize the removal of heat from the package a thermal land pattern including multiple vias to a ground plane must be incorporated on the PCB within the footprint of the package. The exposed pad must be soldered down to ensure adequate heat conduction out of the package.

A recommended land and via pattern is shown in *Figure 17*. More information on soldering LLP packages can be obtained at: <http://www.national.com/analog/packaging/>.

A recommended footprint including recommended solder mask and solder paste layers can be found at: <http://www.national.com/analog/packaging/gerber> for the SQA36A package.

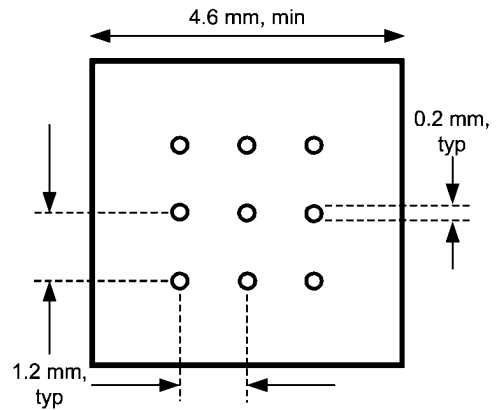
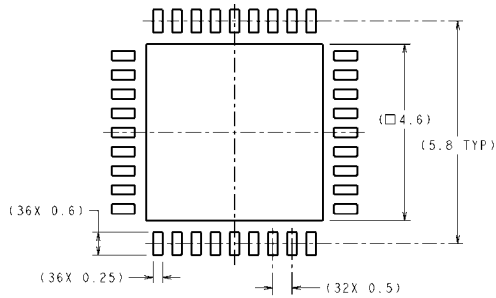


FIGURE 17. Recommended Land and Via Pattern

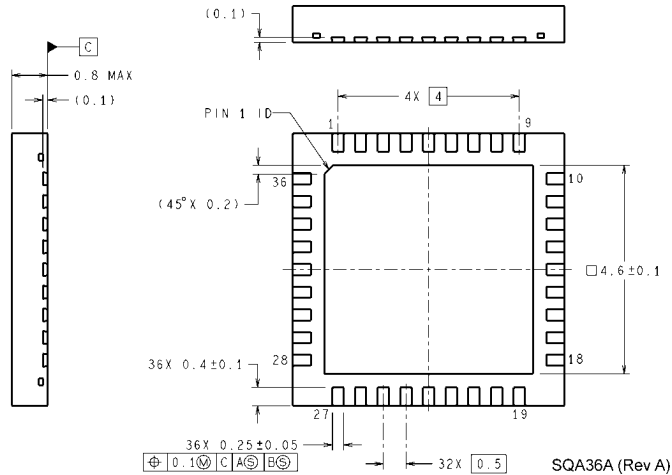
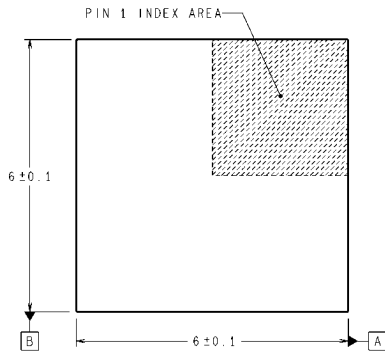
To minimize junction temperature it is recommended that a simple heat sink be built into the PCB (if the ground plane layer is not exposed). This is done by including a copper area of about 2 square inches on the opposite side of the PCB from the device. This copper area may be plated or solder coated to prevent corrosion but should not have conformal coating (if possible), which could provide thermal insulation. The vias shown in *Figure 17* should connect these top and bottom copper layers and to the ground layer. These vias act as "heat pipes" to carry the thermal energy away from the device side of the board to where it can be more effectively dissipated.

**15.0 Physical Dimensions** inches (millimeters) unless otherwise noted



DIMENSIONS ARE IN MILLIMETERS  
DIMENSIONS IN ( ) FOR REFERENCE ONLY

**RECOMMENDED LAND PATTERN**



**36-Pin LLP (SQA36A) Package**

SQA36A (Rev A)

Order Number	Package Marking	Packing
LMK00306SQX	LMK00306	2500 Unit Tape and Reel
LMK00306SQ		1000 Unit Tape and Reel
LMK00306SQE		250 Unit Tape and Reel

**Notes**



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DLP® Products	<a href="http://www.dlp.com">www.dlp.com</a>
DSP	<a href="http://dsp.ti.com">dsp.ti.com</a>
Clocks and Timers	<a href="http://www.ti.com/clocks">www.ti.com/clocks</a>
Interface	<a href="http://interface.ti.com">interface.ti.com</a>
Logic	<a href="http://logic.ti.com">logic.ti.com</a>
Power Mgmt	<a href="http://power.ti.com">power.ti.com</a>
Microcontrollers	<a href="http://microcontroller.ti.com">microcontroller.ti.com</a>
RFID	<a href="http://www.ti-rfid.com">www.ti-rfid.com</a>
OMAP Mobile Processors	<a href="http://www.ti.com/omap">www.ti.com/omap</a>
Wireless Connectivity	<a href="http://www.ti.com/wirelessconnectivity">www.ti.com/wirelessconnectivity</a>

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Computers and Peripherals	<a href="http://www.ti.com/computers">www.ti.com/computers</a>
Consumer Electronics	<a href="http://www.ti.com/consumer-apps">www.ti.com/consumer-apps</a>
Energy and Lighting	<a href="http://www.ti.com/energy">www.ti.com/energy</a>
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Medical	<a href="http://www.ti.com/medical">www.ti.com/medical</a>
Security	<a href="http://www.ti.com/security">www.ti.com/security</a>
Space, Avionics and Defense	<a href="http://www.ti.com/space-avionics-defense">www.ti.com/space-avionics-defense</a>
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